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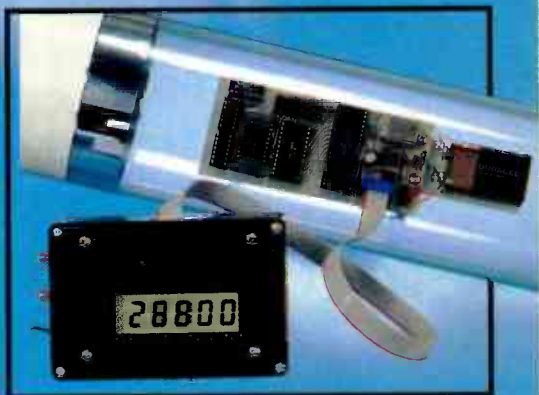
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OCTOBER 1990

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**FLUKE**



**PHILIPS**

**High Resolution Digital Meter:**  
4000 count digital readout; 20,000 count mode (Fluke 87) for 4 1/2 digit resolution

**Backlit display:** Makes it easy to read the DMM in dark, cramped quarters. Automatically shuts off after 68 seconds to save the battery.

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**Holster with Flex Stand™:** Protects meter and provides test lead storage. Flexible leg allows meter to be hung from peg, bent around a pipe, or used almost anywhere.

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## ON THE COVER



For those who already enjoy model rocketry—and for anyone who's thinking of trying it—our cover project offers a whole new dimension to the hobby. The Rocket Altimeter charts the flight path of rockets with an accuracy and ease unheard of with visual tracking methods. The device consists of an on-board flight recorder and an LCD module that's used to display the data back on the ground. The flight recorder takes four pressure samples during every second of flight time. When it's connected to the LCD module back on earth, it displays the rocket's peak altitude and gives a 1/4-speed playback of the entire flight. If you'd like to create your own small-scale space program, check out the Rocket Altimeter on page 37.

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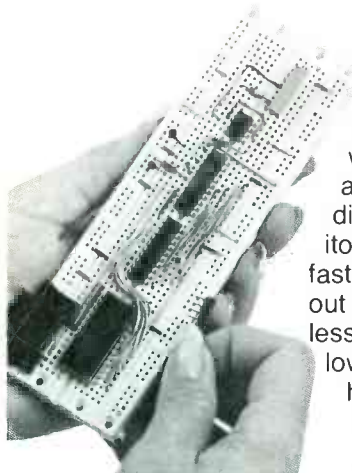
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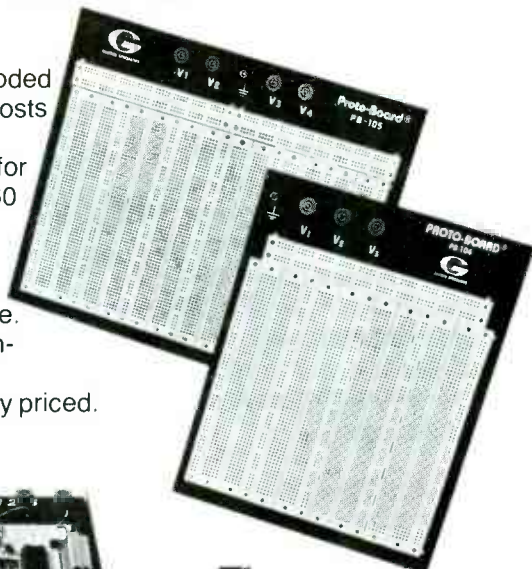


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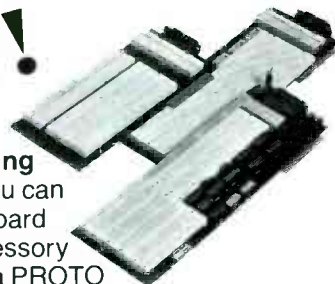
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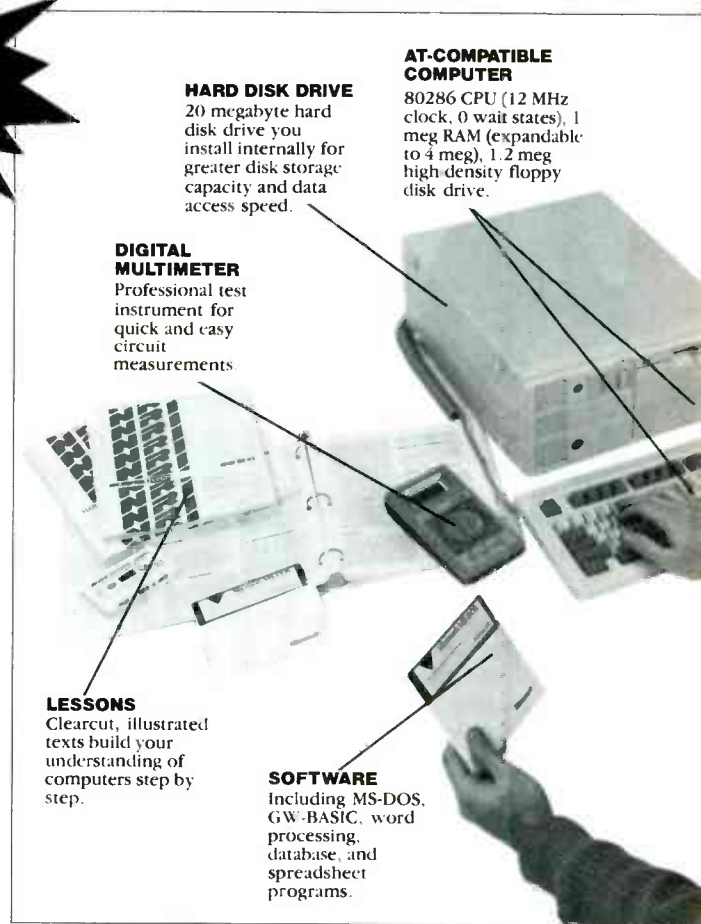
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# WHAT'S NEWS

*A review of the latest happenings in electronics.*

## Progress in handwriting recognition

IBM researchers in Yorktown Heights, NY, have reported the first accurate, real-time computer recognition of run-on, hand-printed characters—even those that run together, touch, or overlap. Previous handwriting-recognition systems could recognize only hand-printed characters that were spatially separated or confined to boxed areas.

The research effort, centered on the experimental IBM computer system called the Paperlike Interface, has as its ultimate goal computer recognition of natural, cursive writing. The recognition of run-on characters is considered a significant step toward that goal.

With the Paperlike Interface, a user "writes" with a stylus on a transparent digitizing tablet that is placed over a flat LCD. The tablet has a layer that allows the computer to sense the position of the stylus on the paper. The path of the stylus appears as "electronic ink" on the flat display directly below it.

In the traditional, "segment-then-recognize" approach, a group of strokes—a stroke is the stylus motion from the point where it first touches the tablet until it is lifted—is held in the computer's memory until the group forms a discrete character that the computer can recognize. In the IBM approach, called "recognize-then-segment," character samples are broken down into stroke templates that the computer can recognize. Written strokes are matched against the stroke templates and labeled to describe the possible character parts they might represent, and sequences of labels are examined to see if they correspond to the components of particular characters.

There are several advantages to the "recognize-then-segment" approach. Because a single template can represent a stroke common to several letters, the number of template-matching steps can be significantly smaller. In addition, the recognition process can begin as

BOXED DISCRETE CHARACTER

Spaced Discrete Characters

Run-on discretely written characters

Cursive script writing

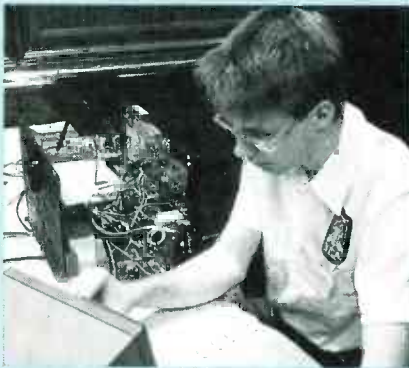
**IBM'S PAPERLIKE INTERFACE** computer system can recognize run-on characters, compared to existing handwriting recognition systems which are limited to boxed or spaced discrete characters. IBM hopes eventually to achieve real-time computer recognition of cursive script writing.

soon as a stroke is complete, rather than waiting for the completion of a character. Stroke labeling also allows built-in constraint functions—dictionaries, for example—so that irrelevant characters or words can be pruned at early stages of the recognition process. Finally, with stroke matching it is possible for the system to adapt to a particular writer, through an optional training process involving customized templates.

In addition to hand-printed letters,

the recognizable writing could include hand-drawn "gestures" such as lines, proofreader's marks, mathematical symbols, and musical notes. Gestures could be used as computer commands, and the stylus could be used to perform mouse-like functions. It is possible that handwriting and gesture analysis could become as popular as the use of keyboards and mice, providing a more natural and convenient way to use and control computers. **R-E**

## Consumer electronics trials



**CHRIS OSTERLOH (LEFT) AND CHARLES (TOMMY) WOOD (RIGHT) WON THEIR SEMI-final rounds in the consumer-electronics trials held in Washington, DC during a three-day competition hosted by the Electronic Industries Association (EIA) and the Vocational Industrial Clubs of America (VICA). Competitors were required to assemble a stereo receiver, take a written theory exam, and troubleshoot 15 different pieces of consumer-electronic equipment. The 19-year-old semifinalists started the year-long industry training programs in June—Osterloh with Matsushita and Wood with Sony—and will receive additional training from EIA instructors. One of the two will be selected in May, 1991 to represent the United States in the International Youth Skill Olympics in Amsterdam next summer.**



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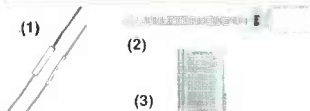
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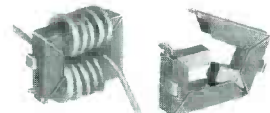
#### Tantalum Caps



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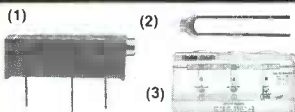
µF	VWDC	Cat. No.	Each
0.1	35	272-1432	.59
0.47	35	272-1433	.59
1.0	35	272-1434	.59
2.2	35	272-1435	.69
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22	16	272-1437	1.19

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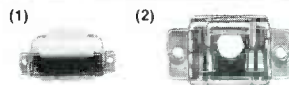


Fig.	Description	Cat. No.	Each
1	9-Position Metal	276-1508	2.19
	25-Position Metal	276-1510	2.79
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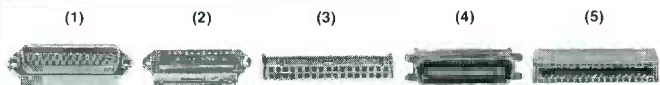


Fig.	Description	Cat. No.	Each
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2	25-Position D-Sub Female	276-1565	3.99
3	34-Position Header	276-1525	2.49
4	36-Position Male Printer Connector	276-1533	4.99
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*What's new in the fast-changing video industry.*

DAVID LACHENBRUCH

## • **Instant VCR programming.**

Several proposals to make programming a VCR "as simple as pushing a button" have cropped up recently—and at least two are close to reaching the public. Widespread attention—including a reference by President Bush and jokes by stand-up comics—has been focused on the difficulty of programming VCR's. Is help finally on the way? Three systems are described below.

**VCR Plus.** Several major newspapers and magazines, including *The New York Times*, the *Los Angeles Times*, the *San Francisco Chronicle*, and some editions of *TV Guide* will soon begin programming their readers' VCR's for them. That will be done by printing special six- or seven-digit code numbers along with the program listings. Viewers can punch those codes into a wireless remote gadget that will automatically set up VCR's and cable boxes to record the programs.

The \$59.95 gadget, VCR Plus, which is being marketed in selected areas by Gemstar Development Corp., Monterey Park, CA, contains a 14-event timer that substitutes for the VCR's timer. The numerical code printed in the TV program listing contains all the information needed to set up the VCR (and cable box, if any) to record the specific program. The device operates both VCR's and cable boxes, so it can be used to record cable programs on different channels (including premium channels) without any extra equipment. It can also "remember" cable channels. For example, if HBO is on cable Channel 33 on one system and Channel 11 on another, the same code number may be used for both systems. The key is in the initial setup of the home unit. It comes supplied with special numbers to correspond to the IR remote-control frequencies of various brands of VCR and cable boxes. Another part of the setup consists of informing VCR Plus of the channel numbers occupied by various cable networks. Thus the code numbers printed in the program listings automatically switch

the user's VCR or cable box to the proper channel. The system's proponents hope to go nationwide with VCR Plus next year.

**Instant Guide.** Gemstar's VCR Plus is just one approach to solving the VCR-programming problem. Something much more elaborate is in the wind. InSight Telecast of Palo Alto, CA, which is partly owned by the Japanese trading company Sumitomo, is cooperating with Public Broadcasting Service (PBS) on an on-screen program guide to be transmitted during the TV picture's vertical blanking interval. Using a VCR with a special adaptor, the viewer merely can select the program to record from the program listings without worrying about the time or channel. Pushing a button on the remote control automatically sets up the VCR to record the program.

The "Instant Guide" program service will be by subscription and will cost viewers about \$5 a month. VCR adaptors are expected to cost around \$100, but should be much less when built into a new VCR. The service is scheduled to start next year in the United States, with Sumitomo estimating that adaptors and adaptor-equipped decks will sell at the rate of one million per year.

**SuperGuide.** But Instant Guide also has some competition. Would you believe "SuperGuide?" The system, developed by a North Carolina company, was the subject of a paper at this year's International Conference on Consumer Electronics in Chicago. SuperGuide is described as "a low-cost, home-oriented, interactive, electronic, on-screen programming guide," designed to be "integrated with the TV tuner, remote control, and other devices." The TV set receives a broadcast database of "programming for only those services to which a viewer subscribes." The hardware is described as costing less than \$40. "Operation of the menus, as well as the Guide itself, requires six buttons on the handheld remote: cursor keys up and down, page forward and page back keys, a

select key, and a return key ... SuperGuide takes a show you want to record and passes the information to a standard event timer in a VCR or satellite receiver." Eventually, the system's proponents say, "SuperGuide will be ready to make recording on your VCR truly as simple as finding the show you want to record and pressing a single button."

• **Widescreen VCR.** A VCR that will play both widescreen (16:9 aspect ratio) and pictures of standard (4:3) TV proportions is under development by the VHS group. It already has been demonstrated in Europe by Thomson Consumer Electronics. In its normal mode, the VCR records conventional TV pictures. In the widescreen mode, tapes of 16:9 pictures are stored on the tape in horizontally squeezed form. A special signal on the sync track will automatically adjust future TV sets to display a "letterbox" picture, or on future widescreen sets the picture will fill the screen automatically. Letterbox pictures may be accommodated by many conventional sets without the automatic-adjustment facility by manual adjustment of the height control to obtain the proper picture proportion. TV sets that come equipped with widescreen picture tubes are expected to be on the European market some time this fall.

• **Dual-deck VCR's.** Go-Video, which filed lawsuits against several Japanese manufacturers, claiming that they refused to make double-deck VCR's for it, is finally marketing its two-slot VCR. The unit, made for Go-Video by Samsung of Korea, will copy tapes (except for those using Macrovision anti-copy encoding), play back one tape while another is being recorded, or record two tapes sequentially. The suggested list price is \$995. In Europe, Amstrad has announced its own similar unit, which it calls the "Double Decker," for about \$695, but says it has no plans to make one for sale in the American market.

**R-E**

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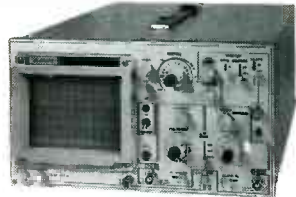
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# ASK R-E

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## EGA TO CGA CONVERSION

**I'm trying to build a circuit that would slow down the sync of EGA video to CGA speed. The reason I want to do this is so I can use a cheaper composite monitor or RF modulator/TV combination. I have a circuit that will allow me to convert an RGB signal into composite video but it doesn't work when I try it with an EGA signal. Would I be on the right track if I used the 5321 Video Sync Generator IC or some kind of video buffer? Any help would be appreciated.—J. Ayala, Fort Lee, NJ**

Whenever someone upgrades their computer from CGA to EGA or VGA, they're faced with the same problem and, so it would appear, the same thoughts cross their minds. Since they already have a CGA monitor, there must be something that can be done to convert it for use with EGA or VGA.

While it's certainly not impossible, converting a CGA monitor for use with a higher video standard is far from being a trivial task. You're correct in assuming that the sync rates are very different for the two video standards, but this difference is a lot more than a simple obstacle.

The chart in Fig. 1 lists the scan rates for several popular IBM video standards. As you can see, the CGA horizontal sync rate is a rather familiar number—15.75 kHz. This is exactly the same as NTSC video so it's possible to use a standard NTSC monitor along with the computer. Things are quite different when you switch to EGA or VGA and there's more involved than just worrying about the horizontal sync signal.

Since your EGA card is putting out video with a horizontal sync rate of 21.8 kHz, it's about 38% higher than the rate for which the NTSC-compatible CGA monitor was designed. If you were absolutely determined to use the CGA monitor for EGA, there are three approaches you could take. We'll look at them in the order of decreasing complexity.

Assuming that there's nothing you can do to your EGA card to make it work with a CGA monitor (some cards can be configured that way), the first way to solve the problem would be the one you're trying to take—convert the EGA signal to something compatible with CGA. Even though it is possible, it's going to be a lot of work, and the resulting image will probably be terrible.

Your first step would be to build an NTSC sync generator (using a chip like the 5321 or discrete components), and then you'd have to design a circuit that would detect the horizontal sync on the EGA signal and gen lock it to the sync from the NTSC generator. You'd need a phase locked loop to keep both of the signals in phase. Of course you have to strip the sync from the EGA signal as well.

The stuff I've described so far is a major undertaking in itself, and we're not even near the end. Since EGA video is being generated much faster than can be handled by a CGA monitor, you're going to need a bunch of memory to store the lines of EGA video until they can be sent out to the monitor at CGA speed. I haven't done the arithmetic but you'll need a lot of memory for the job. The good news is that there's probably enough time in the EGA vertical interval to finish sending out the stored video before the next frame begins. Since

both EGA and CGA operate at a vertical sync rate of 60 Hz, that's one less thing to worry about.

The second approach to the problem would be to look at the CGA monitor rather than the video being fed to it. If you're lucky enough to have the schematic of the monitor, it might be possible to increase the sweep speed of the flyback so the monitor's horizontal circuitry can lock to the EGA sync. Chances are you'll have to rebuild a good part of the monitor circuitry since the flyback transformer might not be able to handle the increased frequency. Even if you managed to overcome all this, you'll have to make sure that the persistence in the picture tube is up to EGA and that the dot pitch of the tube is at least 0.28 mm, since any larger pitch will create a really fuzzy image.

The third approach to the problem is to donate the CGA monitor to a worthy charity and spend the bucks for an EGA monitor. That's the quickest, easiest, and probably least costly way to solve the problem (depending on how you value your time and eyesight).

What you'd like to do isn't impossible, but the chances of getting a resulting image that's worth the time and money that it takes to work through all the design problems is about the same as finding intelligent life on Pluto.

## A NOISY SOLUTION

**Do you have a circuit for a simple analog noise generator? I'd like to use the output to generate random clocking edges for a circuit based around a 7474 flip-flop.—D. Gates, Wichita, KS**

Since you didn't specify the kind of noise you were looking for (pink or white), I'm guessing that it doesn't matter. And from what little you did mention about the application you have in mind indicates that all you're looking for is random-frequency sound.

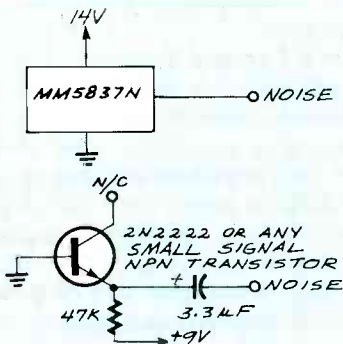
There are two ways you can easily generate the random pulses you're

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HERCULES GRAPHICS ADAPTER	HGA	B&W	18432 Hz
COLOR GRAPHICS ADAPTER	CGA	B	15750 Hz
ENHANCED GRAPHICS ADAPTER	EGA	16	21800 Hz
PROF. GRAPHICS ADAPTER	PGA	256	30480 Hz
VIDEO GRAPHICS ARRAY	VGA	256	31500 Hz

looking for. The first is to use a MM5837N noise generator chip, and the second is to use the old trick of reverse biasing any small-signal transistor. Neither of those methods will produce true analog signals but, since you're feeding them to a digital circuit, you're probably better off with square waves anyway.

Both methods are shown in Fig. 2. The component values aren't very critical and, as long as you stay within ten percent or so of the values shown, you won't have any problems with either circuit. The circuits are both self-starting and will produce the kind of random pulses you're looking for, but you'll more than likely need some buffering circuitry between them and the flip-flop.



**SURROUND SOUND VCR**  
**I recently purchased an LXI TV from Sears with Dolby Surround Sound. Do I have to buy a VCR with Surround Sound to get the most out of my TV, or will a regular stereo VCR decode the Surround signals from my pre-recorded tapes? Also, is anyone manufacturing VCR's that include Dolby Surround Sound?—George Foster, Detroit, MI**

In answer to your first question, the Surround signals are encoded in the standard left- and right-channel audio signals. As long as you are able to feed the left and right signals into a Surround-Sound decoder, the decoder will be able to do its job, regardless of where it is located. As for your second question, there are no Surround-Sound VCR's that I know of, but that doesn't mean that they don't exist. And, considering Surround Sound's increasing popularity, I'm sure you'll see it incorporated into VCR's in the near future. **R-E**

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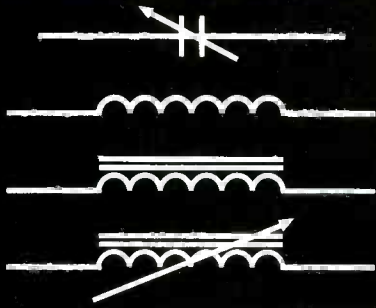
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What are out-of-phase signals?

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# LETTERS

Write to Letters, Radio-Electronics,  
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## BELLS A'RINGING

I had the same problem as the author of "Ring My Phone" (*Ask R-E*, **Radio-Electronics**, July 1990), due to the old-style phones with bell ringers. The newer phones with electronic ringers use very little current.

At first, I shut off the ringers, or disconnected some of them. I found that Motorola made an excellent "Telephone Tone Ringer," so I decided to either make one for each phone or run another phone line and place it in a central location so that it could be heard throughout the house. I turned off all of my old phones and I disconnected one wire to the ringer. I ran the ringer line down to the front doorbell box and installed my electronic ringer in it. If you want you can run another line to the garage workshop and another to the back patio. My phone rings loud enough now to be heard all over the house.

Motorola has an excellent book entitled "Telecommunications Device Data" (#DL136, Rev. 1). See pages 2-201 and 2-241. Everything is in the IC and outside requires 3 resistors, four capacitors, and one piezo sound element. The cost is only about \$4.80.

Figure 1 shows a complete telephone-bell replacement circuit with minimum external components, on-chip diode bridge and transient protection, direct drive for piezoelectric transducers. It rejects rotary dial transients and has an input impedance signature that meets Bell and EIA standards.

Three versions of MC34012 (-1, -2, and -3) are available. Motorola's other options are the MC34017-1, MC34017-2, and MC34017-3.

I hope that will be of interest to everyone. That's a much simpler circuit than the one in *Ask R-E*.

LLOYD F. THOMAS  
Oxnard, CA

## SERVICING VCR'S

After reading Larry Klein's *Audio Update* in the July issue of **Radio-Electronics**, I was very disturbed that he would extrapolate his unique experience with head cleaners in his older VCR to recommend them as safe "... if used precisely according to instructions ..."

I am a Certified Electronic Technician (ISCET) with over 20 years of experience, with 11 years servicing video tape recorders. The shop where I am employed services about 250 VCR's a week. Since January, I personally have removed more than 25 head cleaners from customers' machines. More than half of those machines required head replacement and straightening or aligning some part of the transport or basket assembly. *Not one* of the machines was over five years old.

To refute some of Mr. Klein's statements: Our shop is not "Factory Authorized" anything. The price we charge for a cleaning is \$9.95. For a complete mechanical overhaul—replace belts, clutched idler, resurface pinch roller, and complete lubrications—we charge \$79.95. That comes with a one-year warranty, which is void if a head cleaner is used.

Based on Mr. Klein's recommendations on protecting the cassettes, I assume he also covers his VCR and lives in a sterile, dust-free environment. I am sorry to say that the majority of VCR's passing through our

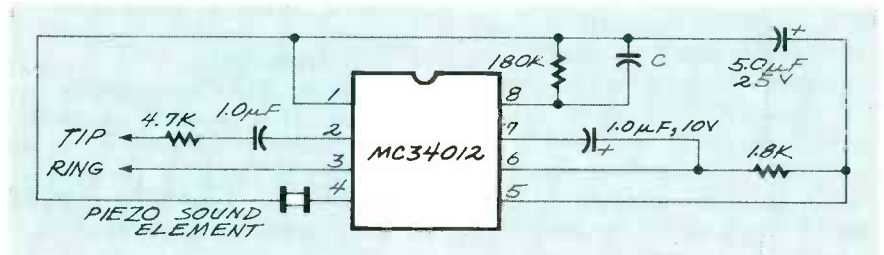


Fig. 1.

shop are so full of dust, fur, and assorted debris that we wear face masks to clean them.

To generalize from my experience, if your VCR weighs over 40 pounds and is more than six years old, you can probably follow Mr. Klein's advice without endangering more than the video heads. Those machines were very tough and could withstand abuse.

My own advice is to buy the very best high-grade tape, and, if the head clogs from a rented movie or cheap tape, put the new tape in and record for 15 minutes. The chemicals the tape manufacturer puts on the tape do a good job of cleaning.  
JO ANNE ABBOT, CET  
Portland, OR

Is Ms. Abbott implying that head-cleaner cassettes tend to jam in machines? That doesn't seem to happen in my neck of the woods. (Of course, cassettes of any type will sometimes jam.) Perhaps things are cheaper in Oregon than New York, but the cheapest price I've found a head-cleaning locally is \$35.00. The complete overhaul sounds like a great deal—it would cost a fortune in New York. I don't cover my VCR or live in a "sterile, dust-free environment and my consultants don't think that the new machines are more fragile than the old, although they are lighter. The cleaning method Ms. Abbott recommends is news to me.—Larry Klein, Audio Editor

### INGENUITY PAYS OFF

I have a Sabtronics multimeter similar to the one illustrated in the "Capacitance Adapter" article in the April issue of **Radio-Electronics**. A couple of years ago the high-current range indicated a malfunction while the meter was monitoring a battery-charging circuit that was supplying less than 4 amps. The 0.1-ohm power resistor was open.

I couldn't find a resistor of that value and tolerance, so the high-current range was useless. Then, recently, I stumbled onto a somewhat unlikely remedy—wind a coil! I'd like to pass the procedure along for any other readers who might encounter the same problem.

A few days ago, when I was checking an AWG table, I noticed that #18 wire has a resistance of one ohm-per 156 feet. It occurred to me that about 15.6 feet of #18 wire would give me

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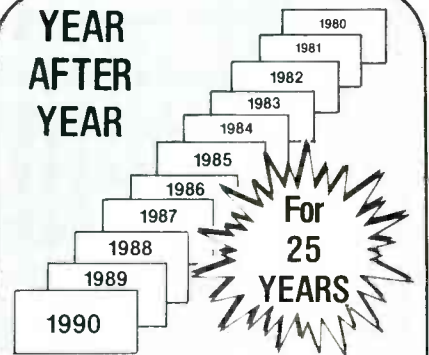
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my 0.1-ohm resistor, and it would monitor 4 amps all day without heating up. I had some #18 magnet wire on hand (from the good old days of audio-crossover projects), so I cut off about 17 feet, stripped the ends, cut the high-current leads of the dual-purpose resistor, and connected the magnet wire. Sure enough, it worked! The reading was high because of the excess margin I had allowed in cutting the wire, but it was easily trimmed down to the optimum resistance.

My Sabtronics multimeter, which

has been checked against a lab-standard meter, was accurate on voltage and resistance but not on high current, which violated Ohm's law in relation to its other readings on the same circuit. Careful trimming of the magnet wire corrected that condition. A lantern battery and a resistor make a good test circuit for Ohm's law evaluation. Of course, you can't use clip leads in calibrating the magnet-wire length; you have to solder both ends in place, take a reading, unsolder, trim, and resolder one end of the wire

until your reading conforms to Ohm's law. Then you unsolder both ends and start winding your coil. A light application of five-minute epoxy will keep the coil compact.

My calibrated wire came close to the 15.6 feet predicted on the AWG table, and wound into a neat two-layer coil on a piece of 1/2-inch dowel. It sits atop the four-lead, dual-purpose power resistor, which still serves the 200-mA range. The meter has been upgraded in both accuracy and durability, and I doubt if the 0.1-ohm coil would heat up any faster on a 10-amp current reading than the test leads.

R.R. DALLING  
San Diego, CA

#### PHONE LINE CORRECTIONS

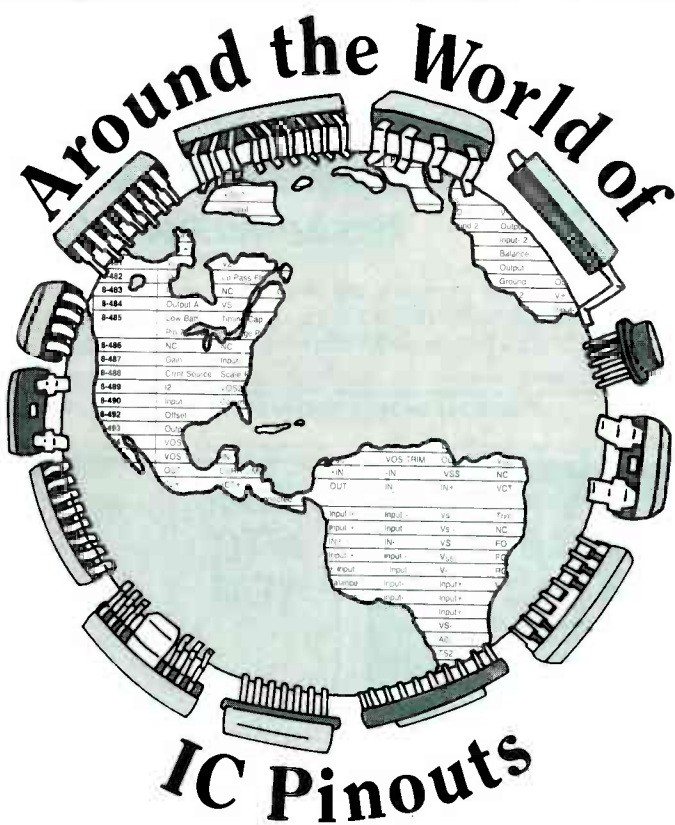
In last month's article, "Build R-E's Telephone-Line Controller," the schematic diagram might cause some confusion. The 9-pin D connector, J2, was shown as a 10-pin connector. Pins 1-9 are correct as shown; pin 10 should be ignored. On the 62-pin card edge connector, the labels A1-A31 should also be ignored. The metal PC mounting bracket that is available from AC&C includes cut-outs for all connectors.

R-E

#### CLEARER RESOLUTION

I would like to clarify the answer given in *Ask R-E* to the "Lines of Resolution" question (**Radio-Electronics**, June 1990). First, the conventional definition of lines of resolution in the horizontal direction is actually equal to the number of visible lines per unit picture height. That definition allows proper comparison for resolution in horizontal and vertical directions. For example, on a 4-by-3 aspect ratio display, 440 visible lines would correspond to 330 "lines of resolution."

Second, for a color CRT television, the electrical bandwidth is not the only limiting factor for resolution. The spacing of the color phosphors (or pitch) is a limiting factor, especially for higher performance sets. In fact, an artifact similar to digital sampling aliasing can occur if the electrical signal driving the tube has a bandwidth higher than the tube pitch can display.



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Finally, for the vertical direction, an NTSC display will not show 525 lines even though there are 525 lines of video available. Limiting factors include 42 lines used for vertical timing and blanking, the CRT pitch, and the Kell scanning factor (which defines how much detail from a real scene can be encoded into a scanned format. In NTSC format, vertical resolution generally works out to 330 lines, which is equal to the 330 horizontal "lines of resolution" that are possible for a broadcast NTSC signal.  
 KARL FRIEDLINE  
 Liverpool, NY

### SPEAKING OUT ABOUT CABLE TV

First, let me express my sincere appreciation for Robert Grossblatt's *Drawing Board* columns on PC-board fabrication and video systems. Both series were timely, informative, and entertaining.

I'm writing about cable-TV signal "piracy." I wholeheartedly agree with Mr. Grossblatt's concept that the cable-TV service should not put the signal on the line in the first place, if they won't permit you to intercept it. In some areas of the country, the premium channel signals are blocked at the pole, preventing the signal from entering the customer's premises if not subscribing.

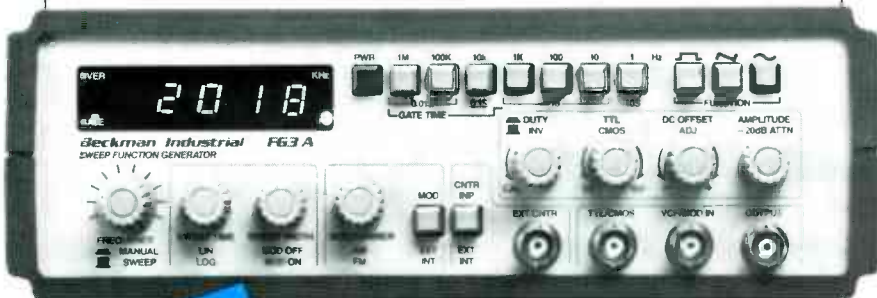
I've been preaching Mr. Grossblatt's message—that the cable companies have to catch up with the phone company in the area of "open access"—for some time now. A mid-1960's federal-court decision opened up the phone-company monopoly; we need an equivalent federal-government-level decision for the cable-TV systems.

What I find to be the most unnerving condition is that the fed's are regulating the EMF spectrum. It's as basic to our democracy as mom, apple pie, and the flag, that each and every individual could do with the EMF in the air what he pleased, as long as he didn't hurt anybody with it! Once it's propagating through the ether, it's free—or should be! Regulation of the signal on a wire is bad enough, but regulation of what we can do with what's not even on a conductor is unconscionable.

Finally, I want to thank you for continuing to publish such fine technical

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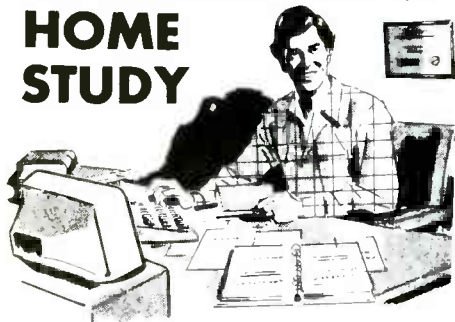
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 RAYMOND C. MINICH  
 Bradford, PA

**FREE CABLE TV**

I enjoy reading *Drawing Board* in **Radio-Electronics**, especially Robert Grossblatt's editorializing in the July issue. I agree that once the signal is inside your television set, you should be free to modify the TV for your own personal reasons in any manner you choose.

I also feel that signals should not be scrambled. Subscriptions to cable should be on a pay-one-price basis, similar to admission to amusement parks (unlimited rides for one price), subway fares (unlimited rides for one token), and the cost of a postage stamp (25 cents to send a letter across the country or across the street). After the cable enters your home, you should be responsible for running the cable to all of your cable-ready TV's. The responsibility of the cable company should end at an interface box on the side of your home, which would prevent a problem on your end from loading down the line.

Another gripe of mine is not knowing the channel allocations on my friends' cable systems. I propose that all channels be assigned a 3-digit identifier. For example, Showtime might be "347." Then, wherever I am, I could enter 347 in the cable box to receive Showtime. Cable boxes could even be configured to map channels in two modes—the current two-digit randomly assigned channel and a three-digit universal identifier—by pressing a selector button.  
 ROBERT ELBURN  
 Hicksville, NY

**DIGITAL DISPLAYS**

I have used the LCD display module mentioned in "Add a Digital Display to Your Project" in the June and July issues of **Radio-Electronics** in a Morse-code translator based on an 8085 microprocessor. I have found that, while it will respond to a 1-microsecond (minimum) write pulse on the E pin, it requires a minimum delay of 1 millisecond between data entries; that is, individual ASCII letter entries must be spaced 1-millisecond apart, even though they will write into the module with a 1-microsecond pulse on the E pin. The standard 6.144-MHz clock crystal was replaced to lengthen the T states.

Everything is done with software rather than hardware, as is done in other display devices. For example, if one wants to enter new data at the right of the display and push the old data off to the left, the shifting must be done by software addressing individual locations in the LCD. That gives flexibility, but with the limitation that the slow speed of the device is not compatible with normal Z80 or 8085 systems.

ADELBERT KELLEY  
 Tampa, FL

**THROWING CAUTION TO  
 THE WIND**

In practically every article on using CMOS integrated circuits, repeated warnings are given on how to avoid static-charge damage and overheating. As a matter of fact, one is always advised to use sockets, rather than direct soldering.

Recently, I bought a kit to assemble a "Radalert" Geiger counter (**Radio-Electronics**, June 1988, updated June 1989). Presumably due to space limitations, the 16 IC's had to be soldered directly to the PC board,

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with no sockets. The instructions outlined many items to avoid, especially overheating, and said to use a temperature-controlled iron (if not available, then a 25-watt iron) and to allow a short period of time between soldering the pins to prevent heat buildup.

In spite of all those warnings, I somehow managed to solder one IC in backward. That error was not discovered until all the chips, and most of the other components, were installed. Of course, I was dismayed to realize it.

There seemed to be three options: start over, with a new board and new components; remove the IC and buy a new one, or try to salvage the old one. It was obvious that to remove the chip, all 16 pins had to be unsoldered at the same time—impossible to do.

Since it was Sunday, I couldn't get any new parts, and waiting seemed intolerable, so I decided to throw caution to the wind. By jamming a small screwdriver under the offending IC, while using the soldering iron up and down over the rows of pins, I pried and jerked the thing out. It took about a half hour; all the pins were bent and one was broken about half way up. By that time, all the remaining pin holes were filled with solder, and I had to use a very small drill to remove it. I straightened the pins and put the chip back in, but I made sure that I did it properly this time.

Much to my amazement and relief, the IC worked beautifully. (It was the one that provides the pulse for the Radalert to measure the counts per minute.)

That experience leads me to believe that the extreme caution urged in handling IC's is overplayed and, quite often, unnecessary. There were also a few diodes that got in backwards, but they caused no particular problems. In the end, the project worked very well, and the Radalert is now measuring counts in 12-hour periods around the house to check the radon level.

J.F. BURTON  
Downers Grove, IL

*It might have worked for you, but we'd hesitate to recommend your technique to others! By the way, haven't you heard of any of commonly-used solder removal techniques? They would have saved you a lot of grief.—Editor*

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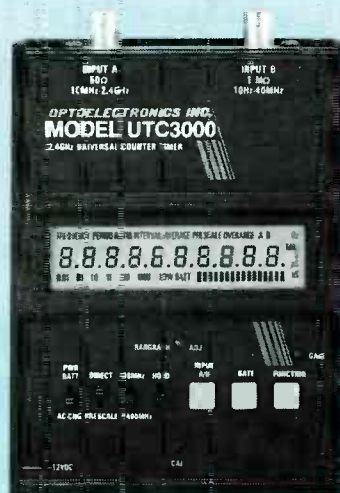
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## Optoelectronics Handi-Counter UTC3000

*A 10 Hz–2.4 GHz universal counter that lives up to its name.*

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Thanks to surface-mount technology and MMIC's (monolithic microwave integrated circuits), handheld frequency counters are rapidly approaching the capabilities of benchtop models. A good illustration of that trend is the UTC3000 Handi-Counter from Optoelectronics, Inc. (5821 N.E. 14th Avenue, Fort Lauderdale, FL 33334).

The UTC3000 is truly a handheld counter, measuring about  $5\frac{1}{8} \times 4 \times 1\frac{1}{2}$  inches. Even with its extruded-aluminum case and built-in Ni-Cd battery pack, the Handi-Counter weighs less than one pound. But don't let those statistics lead you to thinking that the counter is short on capabilities and features.

The Handi-Counter has two input

channels that provide a basic measurement range from 10 Hz to 2.4 GHz. One channel, input A, has an input impedance of 50 ohms, and can be used to measure signals from 10 MHz to 2.4 GHz. A whip antenna is perfect as a probe for input A, and is a good choice for RF measurements. The second channel, input B, has a high input-impedance (1 megohm, 30 pF) and can be used to measure signals from 10 Hz to 40 MHz.

The input sensitivity of the 50-ohm input is  $<1$  mV for signals with frequencies to 200 MHz, decreasing to  $<5$  mV to 2 GHz, and to  $<10$  mV to 2.4 GHz. Although outside the rated capabilities of the counter, the Handi-Counter can typically measure signals up to 3 GHz, but with reduced sensitivity.

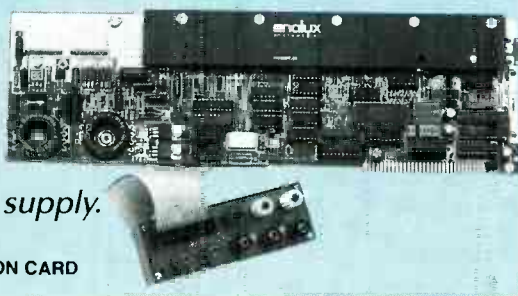
The rated sensitivity for the high-impedance input B is  $<10$  mV to 20 MHz, and  $<20$  mV to 40 MHz. Typical maximum readings extend up to 80 MHz, again with reduced sensitivity.

The front panel of the counter features a 10-digit LCD readout. The display features a built-in 16-segment

## Analyx Powercard PC-controlled Power Supply

*Transform your PC into a triple-output programmable power supply.*

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Although the IEEE-488 or General-Purpose Interface Bus (GPIB) is in no danger of becoming obsolete, test equipment controlled by the PC bus is becoming increasingly popular. That's great news for small test labs and even hobbyists who are looking for a lower-cost way to get automatic test and measurement capabilities. The latest example we've seen is the Powercard programmable power supply from Analyx, Inc. (P.O. Box 14644, Fremont, CA 94539).

The Powercard model PPS-1606 is

an add-on board that turns any IBM PC or compatible computer into a triple-output programmable instrumentation power supply and multimeter. It features one 0–6-volt, 2-amp supply, and two  $-15.7$ – $+15.7$ -volt, 200-mA bipolar supplies. This "power supply on a board" is completely contained within the PC; voltages are brought out to the user by a 26-pin ribbon cable and, if desired, into a convenient terminal box with 5-way binding posts.

Installing the Powercard is easy. You simply plug the card into an emp-

ty slot in the PC, and connect it to the computer's power supply. (If you don't have any free power-supply cables, there's no need to worry—a set of "Y" adapters is included.) Then you plug one end of the ribbon cable into the rear of the card, and the other end to the terminal box. If the Powercard conflicts with any other installed card, its base address can be changed by moving a set of jumpers.

The Powercard is controlled by an easy-to-use, intuitive program. The voltage and current output of each power supply is indicated numerically and with a bar graph. Voltage and current settings and limits can be entered numerically or they can be incremented using the cursor keys. Power-supply settings can be saved in files, and readings can be logged automatically. Our only complaint about the software is a minor one: The selected field is sometimes difficult to find because it is made dim rather than being highlighted. In color, the selected field is much more obvious.

# Coax It Your Way.

bargraph that indicates the relative strength of the input signal. That feature makes the counter ideal for relative field-strength measurements or even for locating hidden transmitters or bugs.

While the *Handi-Counter's* basic specifications are impressive, its additional features, including period-, time-interval-, and ratio-measurement modes, are what make it approach the capabilities of a bench-top unit.

The additional modes are selected by using a FUNCTION switch, which scrolls through the different options. When the power switch is turned on, the counter comes up in the frequency mode. Successive presses of the function switch will select period, interval, and ratio functions; the selected mode is indicated by LCD annunciators.

In the time-interval mode, the pulses that start and stop the timing must be applied to the A and B inputs respectively. In the ratio-measurement mode, the counter displays the ratio of the frequency of the signal at

the A input to that of the B input. Averaging modes for time-interval and period measurements can increase the resolution of the display. Averages of 10, 100, or 1000 measurements can be selected.

The *Handi-Counter* is supplied with a high-accuracy crystal timebase with a rated stability of 1 ppm (part-per-million). A TCXO (temperature-compensated crystal oscillator) timebase, with a rated accuracy of 0.2 ppm is available as an option.

With a base price of \$375, the *UTC3000* is a tough competitor that should come out a winner in most battles. The precision TCXO timebase will add \$80 to the counter's cost, and an extra Ni-Cd battery pack (that doubles the operation time to more than two hours) will cost an additional \$24. A custom-fit protective vinyl carrying case is available for \$15.

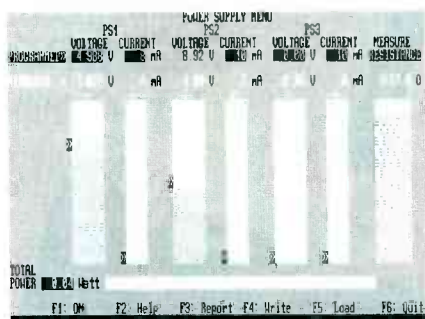
If you've been thinking of a benchtop counter, we encourage you to look at Optoelectronics' handheld that seems to offer the best of two worlds.

**R-E**

While the software supplied with the *Powercard* is adequate for most purposes, complete instructions are provided for reading from and writing to on-board registers so that the board can be controlled by user-written software.

We found the *Powercard* to perform flawlessly and according to the manufacturer's specifications. We liked the fact that—because our computer is already on our test bench—the supply added virtually no clutter to our already-crowded work surface. We also liked that, unlike other computer-controlled supplies, the *Powercard* is self-contained. A separate host interface card (as is required for GPIB equipment) isn't necessary. And since it's directly controlled from the PC bus, it's *fast*

Of course, since the *Powercard* gets its power from the PC's supply, its output power is limited. And even though most PC's have plenty of excess power-supply capacity (the *Powercard* consumes a maximum of 30 watts), there is the possibility of overtaxing the computer's supply.



**THIS SAMPLE SCREEN DISPLAY shows the settings of the three power supplies, and their readings as measured by the on-board 12-bit A/D converter. The multimeter section in this example is set to its resistance mode.**

You don't have to be worried about system crashes, however; the software continuously monitors the PC's supply voltage and displays a warning if the voltage drops below 4.75 volts. The *Powercard* will automatically shut down if the PC's supply voltage drops below 4.6 volts.

Although it's sure to be copied, the *Powercard* is for the time being a one-of-a-kind instrument. It's priced at \$995.

**R-E**



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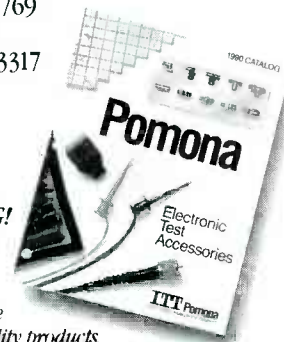
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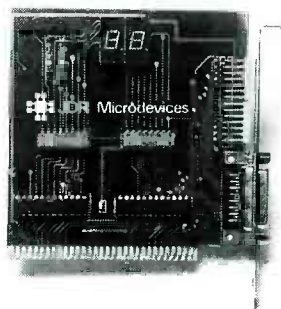
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# NEW PRODUCTS

Use the Free Information Card for more details on these products.

**DIAGNOSTIC DISPLAY CARD.** THE *JDR POST Code* display card provides system designers, engineers, integrators, and computer enthusiasts with a tool that locates the source of a system failure and displays a diagnostic code. Designed to alleviate the frustrating hours often spent trying to track down system failures, the card saves time, energy, and resources. In fact, the card can often solve problems in a matter of minutes, that would have taken hours.

The easy-to-use *POST Code* card plugs into an available bus slot and uses LED indicators to display



CIRCLE 12 ON FREE INFORMATION CARD

the code that corresponds to the problem. The meaning of the code can be found in the BIOS listings in the manual that comes with the card. That will help you to quickly locate almost any problem.

The 80286- and 80386-compatible card features switchless and jumperless design for easy installation and LED indicators for all power-supply voltages. Display LED's may be placed on-board, or on a back-panel bracket for easy readouts with a closed case. Because the circuit uses a dual GAL-chip design, it ensures ultra-low current operation and low noise.

The *POST Code* diagnostic card costs \$49.95.—**JDR Micro-devices**, 2233 Branham Lane, San Jose, CA 95124; Tel: 408-559-1200; Fax: 408-559-0250.

**OPTOELECTRONIC INTERFACES.** Dubbed the "Byte-to-Light" solution, the *FOXI* transmitter and receiver integrated circuits from *Advanced Micro Devices, Inc. (AMD)* and *BT&D Technologies* convert light waves directly to computer-readable data, thus eliminating the technical problems that once made optical connections difficult to use. The devices make it as easy for engineers to design optical links into electronic systems as it is to install any other integrated circuit. AMD expects the "first intelligent optoelectronic interface circuits" to dramatically increase the use of photonics in computing

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Price	\$375.	\$425.	\$239.	\$179.

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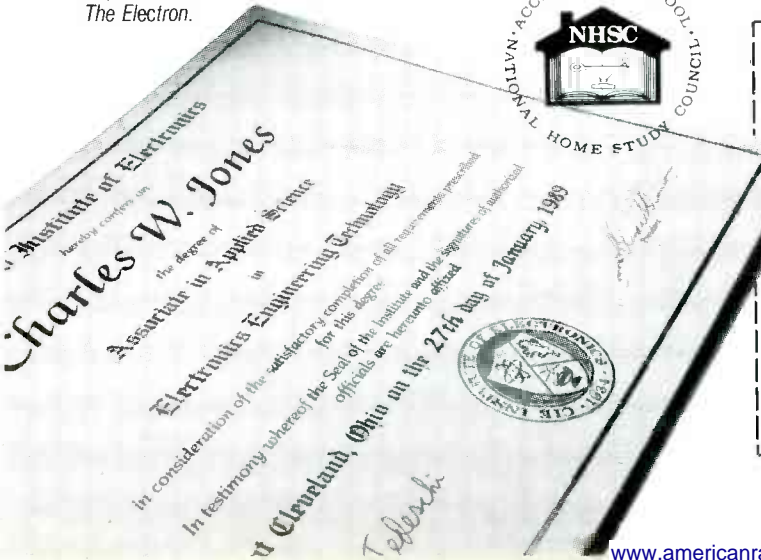
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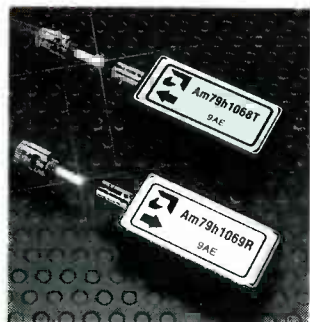
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and networking.

The *FOXI* transmitter converts bytes to light waves; the receiver retrieves the light wave signal from a fiber-optic cable and converts it into electronic data ready for use in computer systems. Each piece occupies the same amount of space on a PC board as does a standard 28-pin IC. The result is that designers—even hobbyists—can easily interface normal computer data to fiber-optic media to take advantage of the power of fiber-optic

cable in applications such as computer backplanes, switching in PBX's, and proprietary local area networks. *FOXI* is a 1300-nanometer LED solution, practical in high-end designs where lasers—the other light source used in light wave communications—would either be too expensive or require too much power.

The circuits are pin-compatible with AMD's *TAXI* chip set, a monolithic intelligent electronic interface that can be applied to optical systems; the IC's can therefore be used to lengthen data-transmission distances on boards that are already set up for coaxial cable. *FOXI* (actually an acronym for fiber optic TAXI), incorporates the *TAXI* chip solution and optical data links in a single package for a quick, cost-effective, and easy-to-use optoelectronic interface.

The *FOXI* set operates

up to a speed of 125 MHz and can transmit data at a rate of up to 12.5-million bytes per second—the equivalent of 150 million words per minute, and about ten times faster than most current wire-based connections.

The two-piece (Am791068/69) *FOXI* set is priced at \$295 per set in lots of 1,000.—**Advanced Micro Devices, Inc.**, 901 Thompson Place, P.O. Box 3453, Sunnyvale, CA 94088-3000; Tel. 800-538-8450, Ext. 45667 or 408-749-5667.

### LABELING SYSTEM.

Designed to take the guesswork out of computer-system hookups, *AMT Communications' Label Logic* kit includes 144 high-quality, silk-screened labels and an EZ Reference card. When used to mark ports, cables, drives, expansion slots, peripherals,



**CIRCLE 14 ON FREE INFORMATION CARD**

etc., the labels will completely identify the parts of almost any PC system. The EZ Reference card provides definitions for all the terms that are printed on the labels, as well as convenient places to write in peripheral information, set-up information, hard-disk partitions, error mapping, and documentation for installing the labels.

*Label Logic* has a suggested retail price of \$6.95.—**AMT Communications**, 2741 Plaza Del Amo #201, Torrance, CA 90503; Tel: 213-320-7757.

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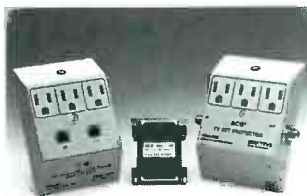
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**PARTS TESTER.** Designed for field-service, industrial, and hobbyist applications, the model 815 from B&K-Precision tests capacitance and resistance in a variety of components and tests transistors, SCR's, diodes, LED's, and batteries in 26 ranges. The rugged handheld instrument is designed to withstand a five-foot drop, and is water- and

**SURGE SUPPRESSORS.** Philips ECG is offering three surge suppressors that are each designed for the protection of specific types of electronic equipment. Used with TV's, VCR's, cable converters, satellite receivers, and audio receivers, the EMF-TV3 offers protection against transient voltage spikes on TV-signal lines from signal



**CIRCLE 16 ON FREE INFORMATION CARD**

to ground and from signal ground to AC-power ground. The EMF-325 tele-

communications surge suppressor offers protection against transient voltage spikes on all telephone lines—ring (red), tip (green), common (yellow), and auxiliary (black). It is intended for use with modems, fax machines, cordless phones, telephones, and answering machines. Both the EMF-TV3 and the EMF-325 protect the AC-power line in all three



B&K PRECISION

Model 815  
Parts Tester

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overload-resistant as well. Its case seals out rain, grease, dirt, and other contaminants. The tester features a 3½-digit LCD readout, a stand for bench use, test leads, and component-insertion sockets.

The 815 tests capacitance from 0.1 pF to 20 mF in capacitors, cables, switches, and other components, with accuracies ranging from 0.75% to 1.5%. Resistance measurements span from 0.1 ohm to 20 megohms. Transistors can be tested for both gain and leakage; SCR's, diodes, and LED's are tested for forward junction voltage, and batteries are tested under load for voltage output.

The model 815 parts tester has a suggested list price of \$99.00.—**B&K-Precision**, Division of Maxtec International Corp., 6470 West Cortland Street, Chicago 60635; Tel: 312-889-9087.

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- Tests capacitance from 0.1pF to 20mF in capacitors, cables, switches; other components.
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modes—hot to neutral, hot to ground, and neutral to ground. The surge suppressors have fused output and surge circuitry and a power/protection indicator lamp.

Designed to protect modems, computers, and peripherals using the RS-232 port from power surges that can cause loss of data and damage to sensitive microprocessors, the EMF-232C data-line protector features RX (receive), TX (transmit), and SG (signal ground) data-line protection. The device shunts transient voltage spikes through high-quality metal-oxide varistors (MOV's).

The EMF-TV3, EMF-325, and EMF-232C have suggested retail prices of \$18.70, \$16.25, and \$8.35, respectively.—**Philips ECG**, 1025 Westminster Drive, Williamsport, PA 17701; Tel: 800-526-9354.

**DIGITAL AND ANALOG MULTIMETER.** Called the "DAMM," model A-445 from *Protek* is a full-function digital and analog multimeter. Its easy-to-read,



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clean-looking, 4½-inch mirrored analog scale provides nulling, peaking, and trend indications, and the bold 3½-digit LCD readout delivers precise measurement values. The DAMM indicates true RMS for AC

voltage and current. Offering AC frequency responses over 100 kHz on the 200-mV range and 20 kHz on the 2-volt range, as well as dB-measurement capabilities, the meter is a useful tool for telecommunications, audio, and industrial technicians. Seven ranges of AC and DC current allow measurement from 10 amperes to a low 10 nA, which is convenient for checking circuits and components for leakage. Diode test and audible continuity check functions are also provided.

The DAMM digital and analog multimeter, complete with safety probes, battery, and spare fuse, costs less than \$100.00.—**Protek Inc.**, P.O. Box 59, Norwood, NJ 07648.

**ELECTRICAL TESTER.** Although it looks (and works) like an ordinary pocket-sized screwdriver,



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A.W. Sperry's model ST-400A does double duty as a high-voltage circuit tester. The fully-insulated tool checks voltages from 90 to 250 volts. It clips onto a shirt pocket, and comes in handy for driving or removing screws, too.

The model ST-400A electrical tester/screwdriver has a suggested retail price of \$2.99.—**A.W. Sperry Instruments, Inc.**, 245 Marcus Boulevard, Hauppauge, NY 11788; Tel: 516-231-7050.

**SURFACE-MOUNT TEST-CLIP SERIES.** *ITT Pomona* has introduced a family of clips for breaking out high-density leads of surface-mounted plastic-

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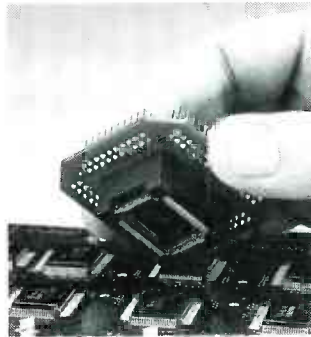
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quad flat-pack (PQFP) devices with 100 to 160 pins. The *5640 Series* of clips fit EIAJ IC's of 100, 120, and 160 pins, spaced on 0.65-mm (0.025-inch) and 0.80-mm (0.0315-inch) centers. Model *5643* fits the 120-pin (20 × 30), model *5644* fits the 120-pin (30 × 30), and model *5645* fits the 160-pin (40 × 40) devices. They "break out" each IC pin to a more accessible 0.64-mm (0.025-inch) square post.

The clips, which are cost effective compared to hand wiring or accessing difficult-to-test leads, feature a press-on design to fit directly over the surface-mounted IC's, keyed by a No. 1 pin locator. Contact with the IC's gull-wing leads is via specially configured, gold-plated, beryllium-copper pins. The clips' bodies are made of black, molded, liquid-crystal polymer. Multiple rows of gold-



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plated, phosphor-bronze square pins are positioned on a grid designed to match commercially available headers.

In single quantities, the list prices of the models *5643*, *5644*, and *5645* PQFP IC clips are \$317.00, \$353.00, and \$425.00, respectively.—**ITT Pomona Electronics**, an ITT EMC Worldwide Company, 1500 East Ninth Street, Pomona, CA 91769; Tel: 714-623-3463; Fax: 714-629-3317.

**DIGITAL TROUBLESHOOTING KITS.** For field-service and educational applications, *Global Specialties* has introduced three digital-logic test kits that are TTL and CMOS compatible. The models *LTC-6*, *LTC-7*, and *LTC-8* each feature a logic probe, a 16-channel logic monitor, a logic pulser, a tone-ohmmeter, and an accessory kit, all packaged in a rugged plastic carrying case. Each kit contains a logic probe to find pulses too fast for oscilloscopes: The *LTC-6* contains a 10-MHz probe, the *LTC-7* contains a 35-MHz probe, and the *LTC-8* contains a 100-MHz probe. The static and dynamic states of 16 logic inputs are simultaneously displayed on the logic monitor. The digital pulser is a pocket-size pulse generator used to stimulate logic circuits with a single pulse or a continuous pulse



CIRCLE 20 ON FREE INFORMATION CARD

train. The tone-ohmmeter locates bad IC's and circuit shorts without unsoldering parts. The accessory kit includes probe tips, ground clips, tip adapters, and quick hook cables, allowing "hands-free" testing.

Prices for the *LTC-6*, *LTC-7*, and *LTC-8* digital-logic test kits range from \$299.00 to \$379.00 each.—**Global Specialties**, 70 Fulton Terrace, New Haven, CT 06512; Tel: 1-800-572-1028. **R-E**



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# NEW LIT

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**1990 INDUSTRIAL HANDBOOK AND APPLICATION GUIDE.** Acculex, A MetraByte Company, 440 Myles Standish Blvd., Taunton, MA 02780; Tel: 508-880-3660; free.

Newly expanded to 80 pages, this catalog contains full product specifications and prices for a variety of industrial monitoring and control products for instrument manufacturers, industrial OEM's, and end users. Also included are applications, wiring diagrams, and 4-20-mA Process Loop accessories. Six sub-miniature thermocouple and RTD-input DPM's have



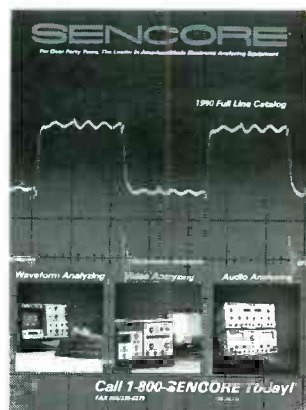
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been added to the Acculex line of digital panel meters. Other new items include a full line of calibrators, signal-conditioning modules, counters/timers, and the "Acupac" 4-20-mA Rack Mount Signal Conditioning

System. The wide array of products described covers virtually all industrial applications from temperature, position, pressure, pH, high/low-level voltage input, dynamic watt measurements, level sensing, and resistance bridges.

**1990 FULL LINE CATALOG.** Sencore, Inc., 3200 Sencore Drive, Sioux Falls, SD 57107; Tel: 1-800-SENCORE; free.

Sencore's entire line of products—all made in the U.S.A., and 93% patented—is described in this catalog. Included are the latest in instruments for testing audio, video, and cable systems. Also fea-



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tured are component and waveform analyzers, IEEE/RS232 instruments, and a full line of accessories. Specifications and application information are also provided.

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		TA-1000A		
		TA-3600		

\* Due to this special offer & low price, we can only exchange or repair any of these units (TA-3600, TA-477, TA-802 & TA-1000A) within 15 days of your receipt.  
\* The above prices are for the complete sets. For separate unit price, please see below

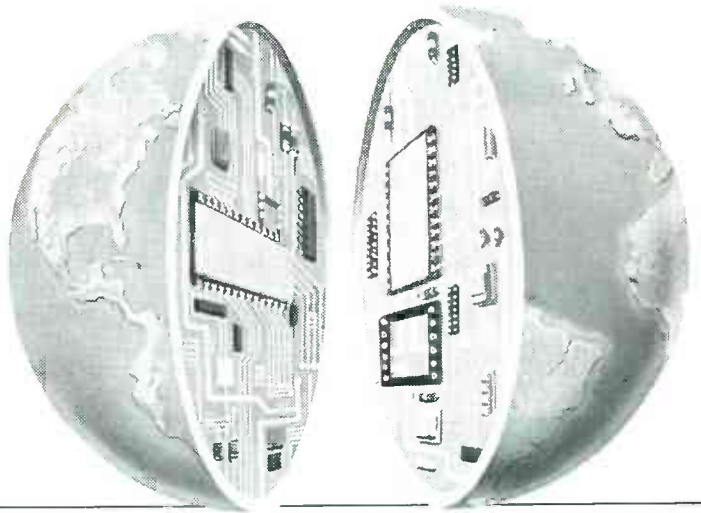
AMPLIFIERS		KIT	ASSMB.		
MODEL	DESCRIPTION				
TA-28MK2	Digital Voice Memo ▲▲	\$ 30.00			
TA-50A/B	Multi-Purpose Melody Generator ▲	12.84	\$ 17.20		
TA-50C	Multi-Purpose Melody Generator ▲	13.65	18.71		
TA-120MK2	35W Class "A" Main Power Mono Amp ▲▲	28.50	39.80		
TA-300	30W Multi-Purpose Single Channel Amp ▲	20.00	29.00		
TA-302	60W Stereo Power Booster (w/case) ▲▲	70.00	70.00		
TA-323A	30Wx2 Stereo Pre-main Amp ▲	29.50	38.35		
TA-377A	Hi-Quality FET Stereo Pre-Amp ▲▲	59.95	75.00		
TA-400	40W Solid State Mono Amp ▲	28.00	34.93		
TA-477	120W Mosfet Power Mono Amp ▲▲	68.00	85.00		
TA-800	80W+80W DC Pre-Main & Power Amp ▲▲	60.92	79.20		
TA-802	80W+80W DC Stereo Main Power Amp ▲▲	45.94	59.72		
TA-820A	60W+60W OCL DC Pre-Main Stereo Amp ▲▲	40.39	49.37		
TA-1000A	100W Dynamic Class "A" Main Power Mono Amp ▲▲	59.69	80.58		
TA-1500	100Wx2 Class "A" DC Stereo Pre-Main Amp ▲▲	73.70	95.81		
TA-2200	FET Super class "A" DC Pre-Amp ▲▲	47.70	58.24		
TA-2400A	Electronic Echo & Reverb/Generation Amp ▲▲	66.00	66.00		
TA-2500	HQ Pre-Amp w/10 band graphic equalizer ★		96.80		
TA-2800	Hi-FET IC Pre-Amp w/3 way tone control ▲	48.90	68.00		
TA-3000	Stereo Simulator (mono TV / any mono source) ▲	27.00	38.50		
TA-3600	300W HQ Hi-Fi Power Mono Amp ▲▲	79.00	103.00		
POWER SUPPLIES		KIT	ASSMB.		
TR-100A	O-15V 2A Regulated DC Power Supply (w/case) ▲▲	\$ 14.55	\$ 20.76		
TR-355A	O-30V 3A Regulated DC Power Supply ▲	14.55	20.76		
TR-355B	O-30V 3A Regulated DC Power Supply ▲	14.55	20.76		
TR-503	O-50V 3A Regulated DC Power Supply ▲	15.75	22.65		
INSTRUMENTS		KIT	ASSMB.		
SM-43	3 1/2 Multi-Functional Led D.P.M. (w/ABS plastic case) ▲▲	\$ 34.50	\$ 43.00		
SM-48	4 1/2 Hi-Precision D.P.M. ▲▲	38.00	48.00		
SM-48A	4 1/2 Hi-Precision D.P.M. (w/ABS plastic case) ▲▲	41.20	52.00		
SM-49	3 1/2 Multi-Functional LCD D.P.M. (w/hold function) ▲	36.00	44.50		
SM-100	150 MC Digital Frequency Counter ▲▲	79.00	90.00		
FC-1000A	1 GHz Frequency Counter ★	179.00	179.00		
MISCELLANEOUS		KIT	ASSMB.		
MODEL	DESCRIPTION				
TY-23B	3 Channel Color Light Controller ▲▲▲	\$ 51.20	\$ 65.00		
TY-25	Stereo Loudspeaker Protector ▲	13.85	19.85		
TY-35	FM Wireless Microphone	10.22			
TY-36	AC/DC Quartz Digital Clock ▲	19.00	26.20		
TY-38	Sound/Touch Control Switch ▲	12.00			
TY-41 MKV	Infrared Remote Control Unit w/case ▲▲	20.00	35.00		
TY-42	Bar/Dot Level Meter ▲	24.5			
TY-43	3 1/2 Digital Panel Meter ▲	29.00	38.00		
TY-45	20 Steps Bar/Dot Audio Level Display ▲	38.45	46.14		
TY-47	Superior Electronic Roulette ▲	19.46	27.24		
SM-222	7 Band Hi-Fi Graphic Equalizer ▲▲	26.80			
SM-328	4 Channel Professional Color Light Controller★		139.00		
SM-333	Audio/Video Surround Sound Processor ▲▲	62.00	70.00		
SM-666	Dynamic Noise Reduction ▲	26.00	34.00		
METAL CABINETS WITH ALUMINUM PANEL		KIT	ASSMB.		
MODEL	H" x W" x D"	MATCHING	PRICE		
LG-1273	3" x 12" x 7"	TA-2800, TA-377A, TA-2200	\$ 22.16		
LG-1684	4" x 16" x 8"	TA-323A, TA-377A, TA-2200	26.64		
LG-1924	4" x 19" x 11 1/2"	TA-802, TA-820A, TA-1500, TA-120MK 2, TA-860, TA-1000A	32.00		
LG-1925	5" x 19" x 11 1/2"	TA-477, TA-800, TA-1500, TA-1000A, TA-3500	35.00		
LG-1983	2 1/4" x 19" x 8"	TA-377A, TA-2800, TA-2200, TA-120MK 2	28.50		
POWER TRANSFORMERS		MODEL	DESCRIPTION	MATCHING	PRICE
#001	56VCT, 60VCT 6A	TA-800, TA-802, TA-820A, TA-1000A, TA-1500	\$ 26.00		
#002	72VCT 3A	TR-503, TA-323A, TA-400, TA-300	21.00		
#003	80VCT 6A	TA-477	27.00		
#004	48VCT 6A	TA-120 MK 2	21.00		
#005	52VCT 3A	TR-355B	15.00		
#006	36VCT 5A	TR-355A	14.50		
#007	112VCT 8A	TA-3600	42.00		

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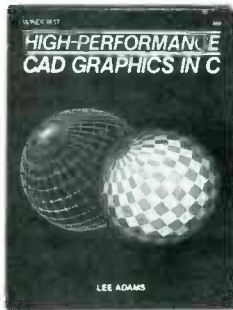
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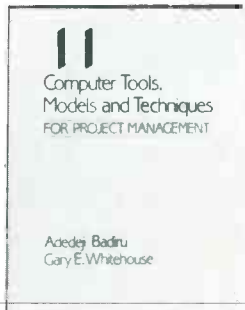
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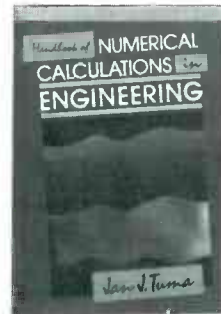
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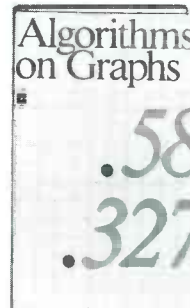
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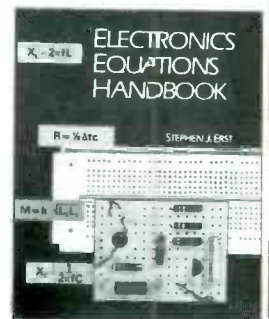
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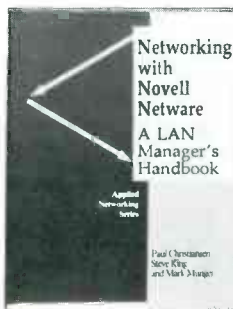
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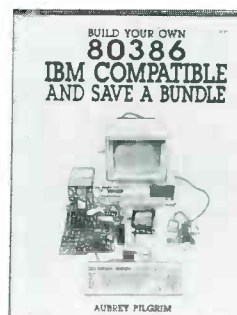
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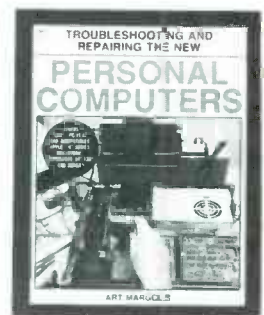
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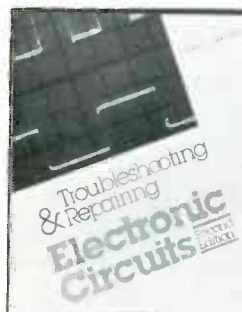


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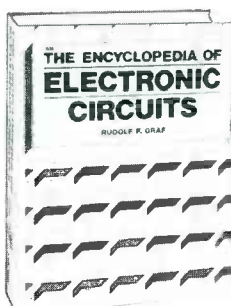


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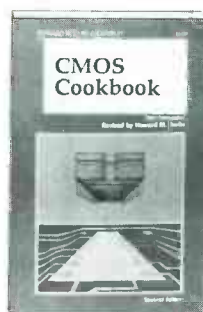
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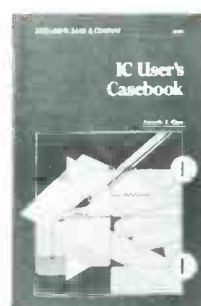
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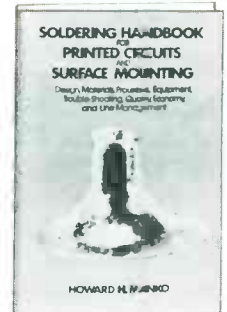
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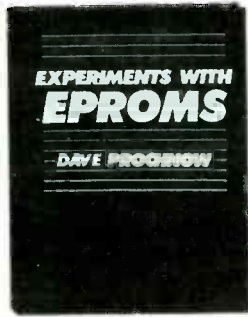
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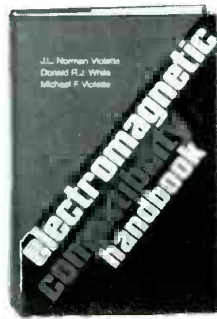
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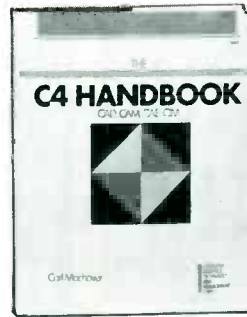
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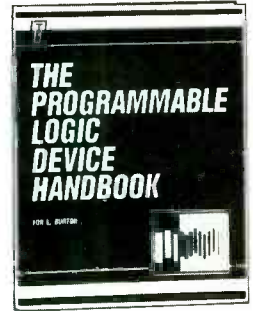
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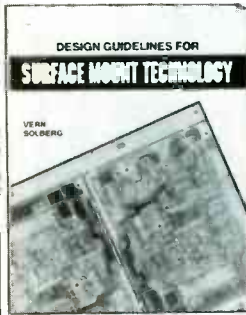


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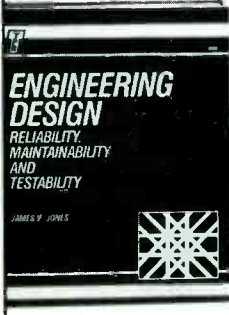
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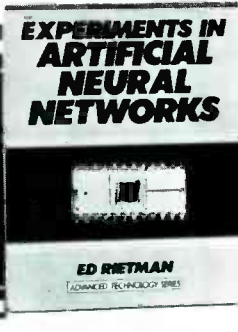
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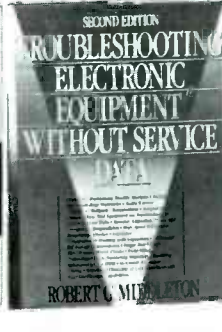
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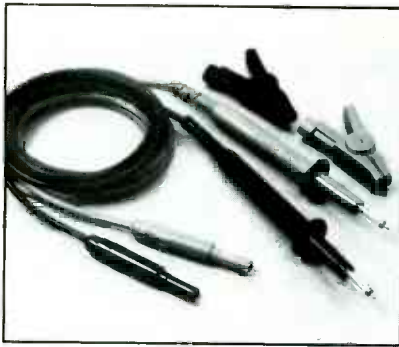
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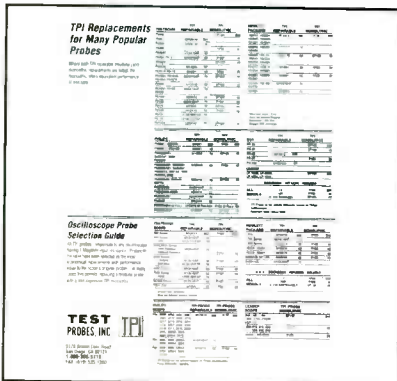


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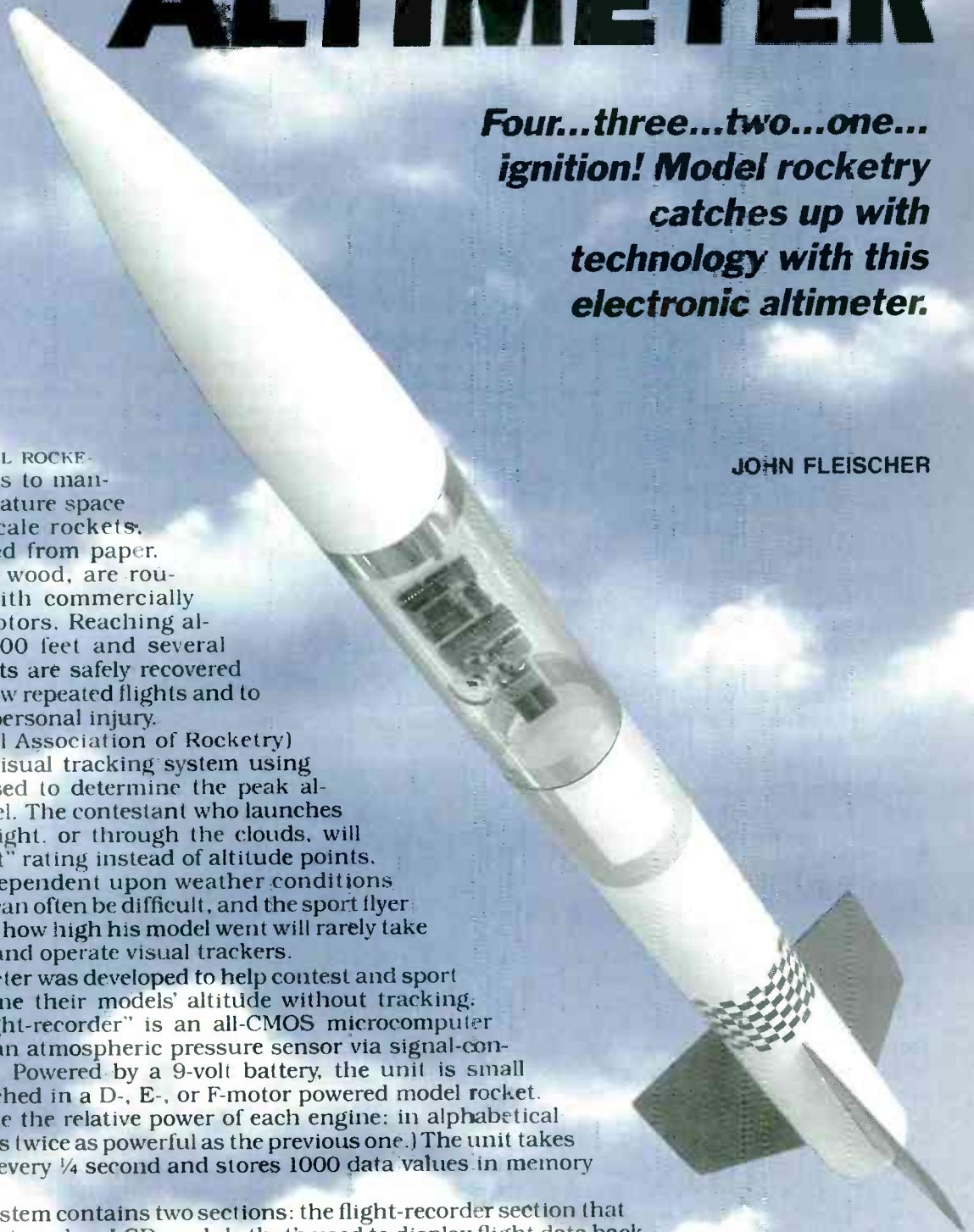
JOHN FLEISCHER

THE SPORT OF MODEL ROCKETRY allows hobbyists to manage their own miniature space program. Small-scale rockets, usually constructed from paper, plastic, and balsa wood, are routinely launched with commercially made solid-fuel motors. Reaching altitudes between 100 feet and several miles, model rockets are safely recovered by parachute to allow repeated flights and to reduce the risk of personal injury.

In NAR (National Association of Rocketry) contest events, a visual tracking system using triangulation is used to determine the peak altitude of each model. The contestant who launches his rocket out-of-sight, or through the clouds, will receive a "track lost" rating instead of altitude points. Visual tracking, dependent upon weather conditions and operator skill, can often be difficult, and the sport flyer who wants to know how high his model went will rarely take the time to set up and operate visual trackers.

Our rocket altimeter was developed to help contest and sport rocketeers determine their models' altitude without tracking. This airborne "flight-recorder" is an all-CMOS microcomputer that is coupled to an atmospheric pressure sensor via signal-conditioning circuitry. Powered by a 9-volt battery, the unit is small enough to be launched in a D-, E-, or F-motor powered model rocket. (The letters indicate the relative power of each engine: in alphabetical order, each engine is twice as powerful as the previous one.) The unit takes a pressure sample every 1/4 second and stores 1000 data values in memory during the flight.

The completed system contains two sections: the flight-recorder section that goes up in the rocket, and an LCD module that's used to display flight data back on the ground. When the rocket returns to Earth, the LCD module is connected to the flight recorder and the peak altitude achieved can be displayed in 50-foot increments, along with a 1/4-speed "playback" of the entire flight. Rocketeers now



have a reliable and accurate means to measure the altitude that a model reaches. The data obtained can then be used to calculate the speed and acceleration of the rocket.

Figure 1 shows the construction and pinout of the SCX15AN pressure sensor used in the altimeter. The sensor, manufactured by Sensym (1255 Reamwood Ave., Sunnyvale, CA 94089), is a low-cost (about \$42) piezoresistive IC in a strain-gauge bridge configuration. The monolithic circuitry inside the sensor (see Fig. 2) is deposited on a silicon chip that has a cavity etched out to form a diaphragm. A port is on top, and a vacuum reference cavity is on the bottom. The result is a sensor that measures absolute barometric pressure. Output voltage ( $V_1 - V_2$ ) ranges from 10–50 mV, and is proportional to atmospheric pressure—which, of course, varies with altitude. Although the entire unit is not temperature compensated, the sensor itself is, by means of two built-in thermistors. Best accuracy for the altimeter is achieved in the 55–75°F range. Outside that range, a shift of 2% for every 10°F will occur.

Figure 3 shows the block diagram of the system. The pressure sensor is buffered with an LM324 op-amp to feed an LM331 voltage-to-frequency (V/F) converter. At ground level, a signal of about 3.7 kHz will be output by the V/F converter. As the atmospheric pressure decreases (with increasing altitude), that frequency also decreases: at 15,000 feet, the signal is about 2.9 kHz. An RCA 1802 microprocessor calculates the altitude data from the frequency input.

The entire system is made up from three separate PC boards, although only two ever leave the ground. The pressure sensor, the LM324 buffer, the V/F converter, and other support circuitry is located on an "analog" PC board, and the microprocessor and data-logging circuitry are on a "CPU" board. The two boards are held together with screws, and electrical connections are jumpered between the two. The display module is built on a separate PC board, and it stays on the ground; the module must be con-

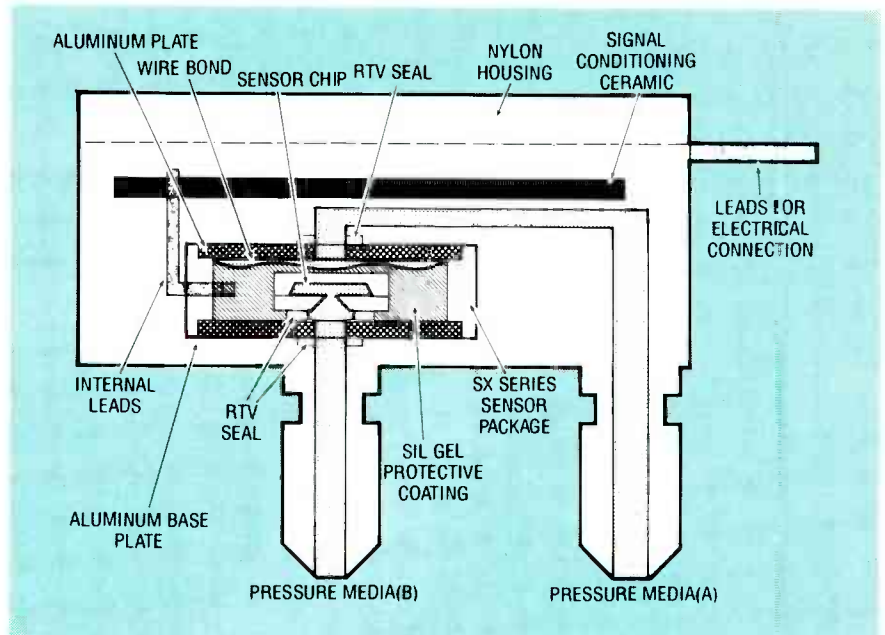


FIG. 1—THE MONOLITHIC CIRCUITRY inside the SCX15AN pressure sensor is deposited on a silicon chip that has a cavity etched out to form a diaphragm. A port is on top, and a vacuum reference cavity is on the bottom. The result is a sensor that measures absolute barometric pressure, which is then converted to altitude.

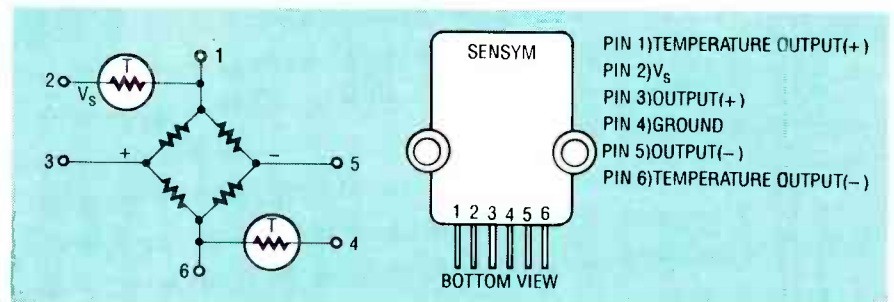


FIG. 2—THE SENSOR'S OUTPUT VOLTAGE ( $V_1 - V_2$ ) ranges from 10–50 mV, and is proportional to atmospheric pressure.

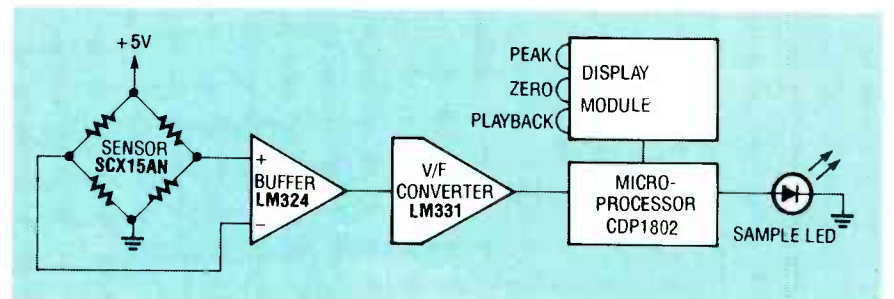


FIG. 3—THE BLOCK DIAGRAM OF THE SYSTEM. The pressure sensor is buffered with an op-amp to feed a voltage-to-frequency (V/F) converter. At ground level, a signal of about 3.7 kHz will be output by the V/F converter; at 15,000 feet, the signal is about 2.9 kHz.

nected to the other two boards via a ribbon cable to play back flight information.

Figure 4 shows the schematic of the CPU board: it gets its input from the analog board and logs the data every 1/4 second. The circuit consists of the microprocessor which calculates the altitude, the EPROM containing the operating software, and the RAM where the altitude data is

stored. Figure 5 shows the schematic of the analog board: the pressure sensor is located on this board. The output from the sensor is buffered and fed to the V/F converter, which provides the frequency input for the microprocessor. Figure 6 shows the schematic of the display module board. It is basically made up of the display driver and the display itself, but also contains the con-

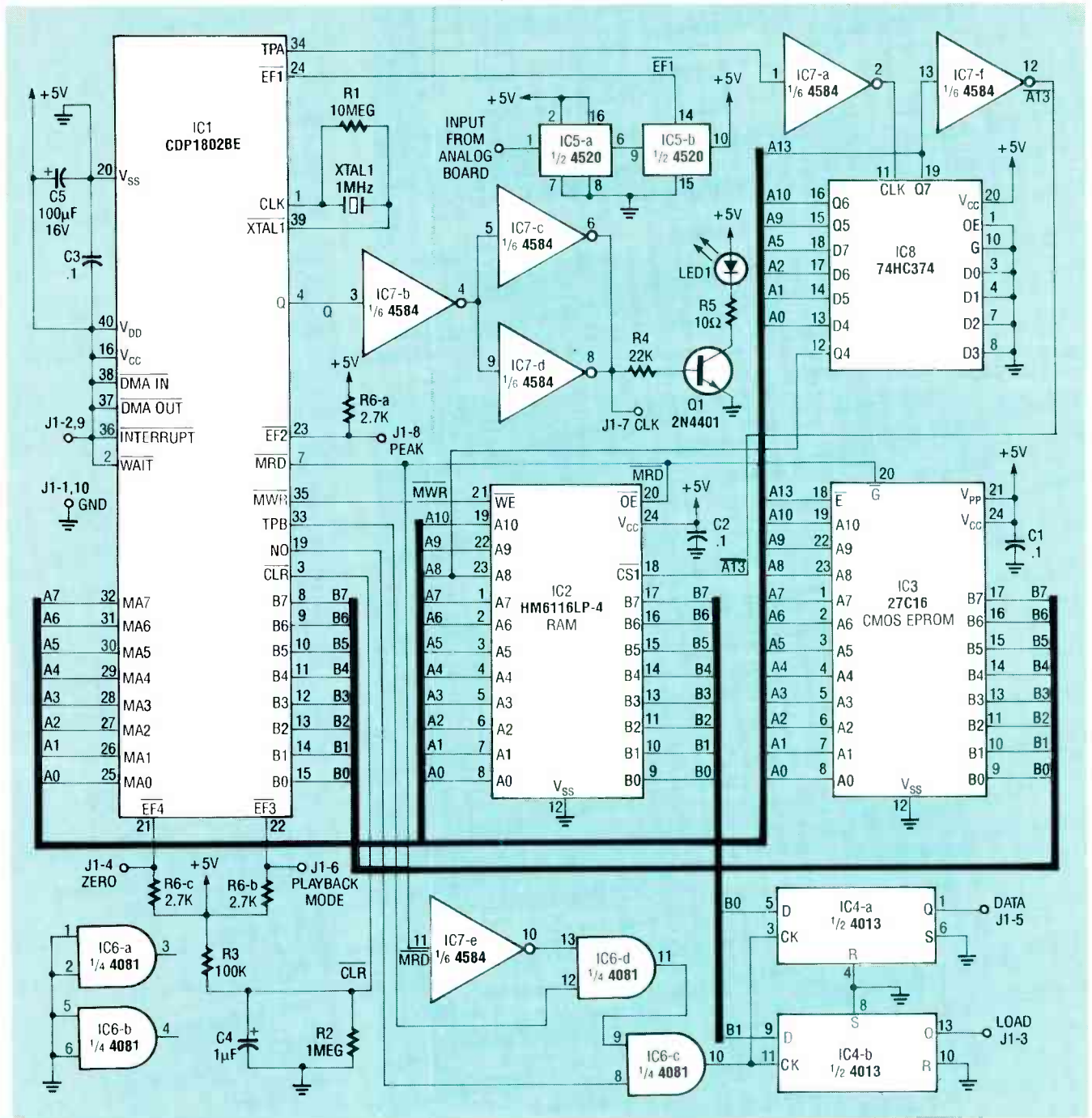


FIG. 4—THE SCHEMATIC OF THE CPU BOARD. It logs the data to be read back when the rocket returns to Earth.

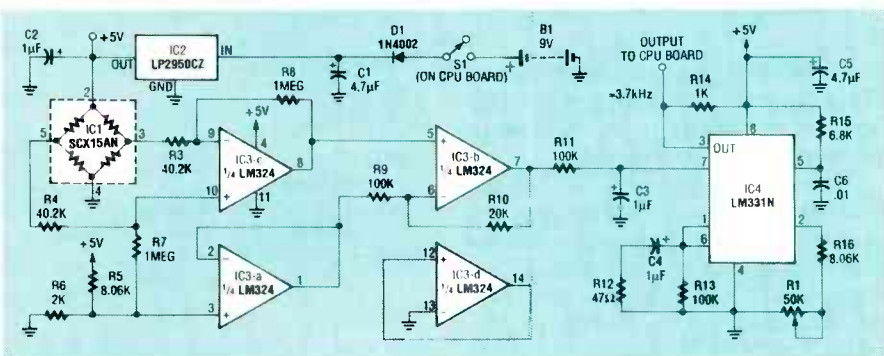


FIG. 5—THE ANALOG BOARD outputs a frequency that's proportional to altitude. The sensor (IC1) is located on this board.

control switches. Power for the display module comes from the other two boards via the ribbon cable.

The software for the altimeter is available on the R-E BBS—516-293-2283. (For those who prefer to type, the machine code for the EPROM is shown in Listing 1.) The flowchart for the program is shown in Fig. 7. The software handles data logging (the sample LED flashes every 1/4 second), mode switch input, and LCD interfacing.

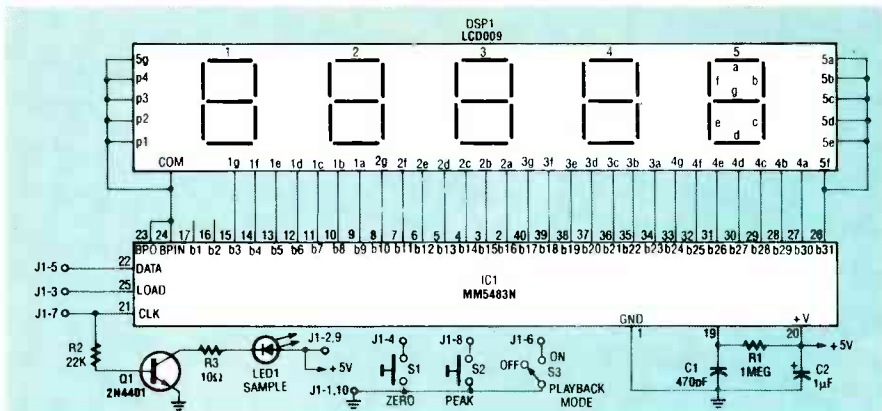


FIG. 6—THE DISPLAY MODULE stays on the ground; when the rocket is retrieved, the data from the CPU board is displayed on this module.

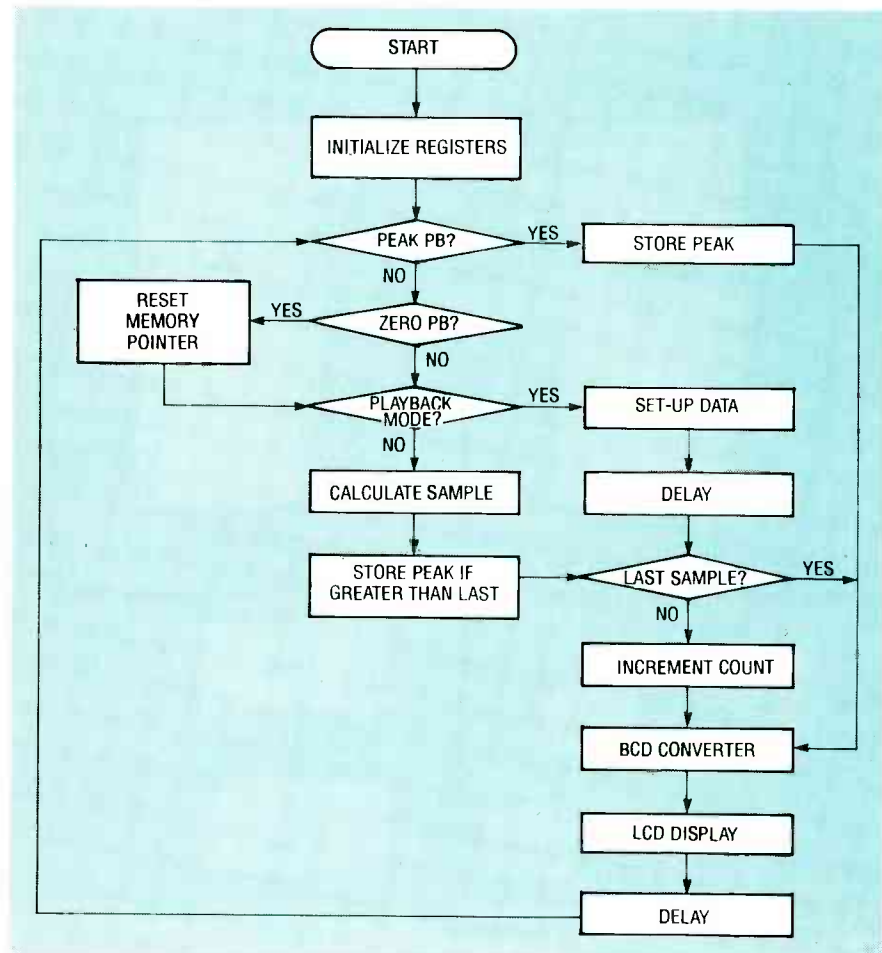


FIG. 7—THE SOFTWARE FOR THE ALTIMETER HANDLES data logging, mode switch input, and LCD interfacing.

### Construction

Three printed-circuit boards are used. The pressure sensor and analog section are combined on a single-sided PC board. The CPU board is double-sided, as is the board for the display module. If the holes in either of the double-sided boards are not plated-through, feed-through wires must be used instead. All pads on the top and bottom of the boards must be soldered to the compo-

nent lead or feed-through wire. (The boards available from the source mentioned in the parts list are plated-through.)

To assemble the CPU board, follow the parts-placement diagram shown in Fig. 8. Install the resistors, capacitors, connector, switch, LED, and transistor. The crystal may be fastened to the board with foam tape or RTV silicone cement. IC sockets should be used to ease any future repairs

### CPU BOARD

All resistors are ¼-watt, 5%, unless otherwise noted.

- R1—10 megohms
- R2—1 megohm
- R3—100,000 ohms
- R4—22,000 ohms
- R5—10 ohms
- R6—2700 ohms, SIP resistor (cut to fit board)

### Capacitors

- C1—C3—0.1 µF, monolithic
- C4—1 µF, 25 volts, tantalum
- C5—100 µF, 16 volts, electrolytic

### Semiconductors

- IC1—CDP1802CE microprocessor (GE/RCA)
- IC2—HM6116LP-4 RAM
- IC3—27C16 CMOS EPROM
- IC4—4013 dual D-type flip flop
- IC5—4520 dual synchronous up counter
- IC6—4081 quad 2-input AND gate
- IC7—4584 hex Schmitt trigger
- IC8—MM74HC374N octal tri-state D-type flip-flop
- LED1—red light-emitting diode
- Q1—2N4401 NPN transistor

### Other components

- XTAL1—2 MHz crystal
- S1—PC-mount slide switch
- J1—10-pin header

### Miscellaneous:

- 10-conductor ribbon cable, 3 ¼-inch #6 spacers, 3 #6-32 × ½-inch screws and nuts, PC board, IC sockets, wire, solder, etc..

### ANALOG BOARD

All resistors are ¼-watt, 5%, unless otherwise noted.

- R1—50,000 ohms, 25-turn trimmer potentiometer
- R2—not used
- R3, R4—40,200 ohms, ½-watt, 1%, metal-film
- R5, R16—8060 ohms, ½-watt, 1%, metal-film
- R6—2000 ohms, ½-watt, 1%, metal-film
- R7, R8—1 megohm, ½-watt, 1%, metal-film
- R9, R13—100,000 ohms, ½-watt, 1%, metal-film
- R10—20,000 ohms, ½-watt, 1%, metal-film
- R11—100,000 ohms, 5% resistor, 1/4W
- R12—47 ohms
- R14—1000 ohms
- R15—6800 ohms, ½-watt, 1%, metal-film

### Capacitors

- C1, C5—4.7 µF, 16 volts, tantalum
- C2—C4—1 µF, 25 volts, tantalum
- C6—0.01 µF, 50 volts, 5% film-type

### Semiconductor

- IC1—SCX15AN pressure sensor
- IC2—LP2950CZ-5.0, 5-volt regulator
- IC3—LM324N op-amp
- IC4—LM331N voltage-to-frequency converter
- D1—1N4002 diode

- Miscellaneous: 9-volt battery and clip, PC board, IC sockets, wire, solder, etc..

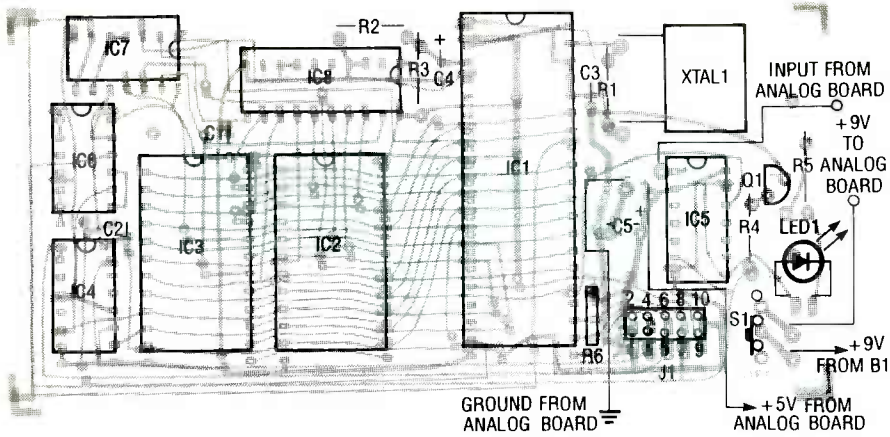


FIG. 8—WHEN ASSEMBLING THE CPU BOARD, the crystal should be fastened to the board with foam tape or RTV silicone cement to prevent damage due to vibration.

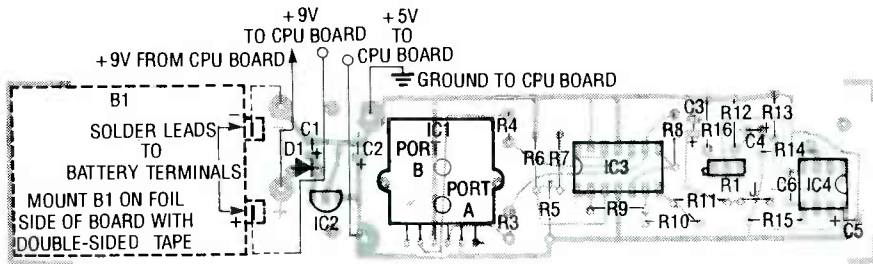


FIG. 9—THE ANALOG-BOARD PARTS LAYOUT. Carefully install the pressure sensor and, if you ever clean the PC board, do not allow any solvent or moisture to enter the sensor port.

### DISPLAY MODULE

All resistors are 1/4-watt, 5%, unless otherwise noted.

- R1—1 megohm
- R2—22,000 ohms
- R3—10 ohms

#### Capacitors

- C1—470 pF, ceramic disc
- C2—1 μF, 25 volts, tantalum

#### Semiconductors

- IC1—MM5483N display driver
- DSP1—LCD009 LCD module
- LED1—red light-emitting diode
- Q1—2N4401 NPN transistor

#### Other components

- J1—10-pin header
- S1, S2—momentary pushbutton switch
- S3—SPST toggle switch

**Miscellaneous:** 4 #6-32 × 1-inch screws and nuts, 8 1/4-inch #6 spacers, case, clear plastic sheet for display window, 40-pin wirewrap socket strip, PC board, wire, solder, etc..

**Note:** The following items are available from Transolve Corporation, 13361 Shady Lane, Chesterland, Ohio 44026 (216) 341-5970: Pressure sensor, \$42; PC board set, \$35; complete kit (except case), \$135; EPROM only, \$15; machined case and custom EPROM's available on request. For large-scale rocket kits contact North Coast Rocketry, P.O. Box 24468, Mayfield Heights, Ohio 44124. For more information on model rocketry in general, contact the National Association of Rocketry, 2140 Colburn Drive, Shakopee, MN 55379.

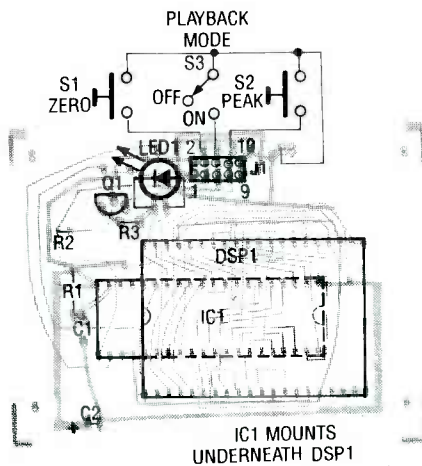


FIG. 10—DISPLAY BOARD parts-placement diagram. The LCD module is plugged into wire wrap socket strips above IC1.

(Transolve Corp. will not service any non-socketed unit).

Follow the analog-board parts layout shown in Fig. 9, and install the resistors, jumper wire, diode, and capacitors. Note that C6 must be a film-type capacitor—a disc capacitor will cause excessive drift with temperature. Next install the trimmer potentiometer and the IC's. Carefully install the pressure sensor as

shown. If you ever clean the PC board, do not allow any solvent or moisture to enter the sensor port, or you'll damage it. You must test the analog board before attaching it to the CPU board.

The display board parts-placement diagram is shown in Fig. 10. Install the resistors, capacitors, connector, LED, and IC1. The LCD module is plugged into wire-wrap socket strips above IC1. Space the top of the strips 1/4-inch from the board. Make sure the LCD pins are perfectly straight, and press the display into the socket strips. The finished analog/CPU assembly is shown in Fig. 11, and the display module in Fig. 12.

### Testing and calibration

Connect a 9-volt battery to the + and - battery input pads on the analog board. Connect your DVM and scope ground leads to battery -. The regulator output (IC3 pin 4) should measure 5 volts. Set R1 to midpoint. Connect scope probe to IC4 pin 3; this output signal should be a short, negative-going pulse, repeating at about 3.7 kHz. Adjust R1 to obtain that value. Use a frequency counter if one is available. Apply suction to sensor port A (draw a vacuum with your mouth) and verify that the signal frequency decreases slightly.

If the analog board is functioning, it can now be attached to the CPU board. The wire attachment points are designated in the three parts layouts. The 9-volt battery's positive lead connects to the CPU board, and the 9 volts from the CPU board is jumped over to the analog board. Also remember to connect ground, +5 volts, and the analog output between the two boards. A rocket is a very high vibration environment, so the 9-volt battery snap must be taped on, or the leads must be soldered to the battery. After the electrical connections are made between the two boards, the analog board is fastened to the CPU board with three screws, spacers, and nuts.

Wire the pushbutton and toggle switches to the display PC board as shown in the display-module parts-placement diagram. One of the normally open pushbuttons is used to select

PEAK, and the other ZERO. The toggle switch selects the playback mode (when closed). Install the header connectors on the ribbon cable that goes between the CPU and display boards, and connect the two boards together.

Turn the power switch on and open the playback switch. The sample LED on the CPU and display boards should be flashing four times per second. A value of several thousand feet should be displayed. Adjust R1 on the analog board for a reading of 100 feet, then 50 feet, and the unit will then be calibrated for ground level. Do not adjust past that threshold, or the altitude mea-

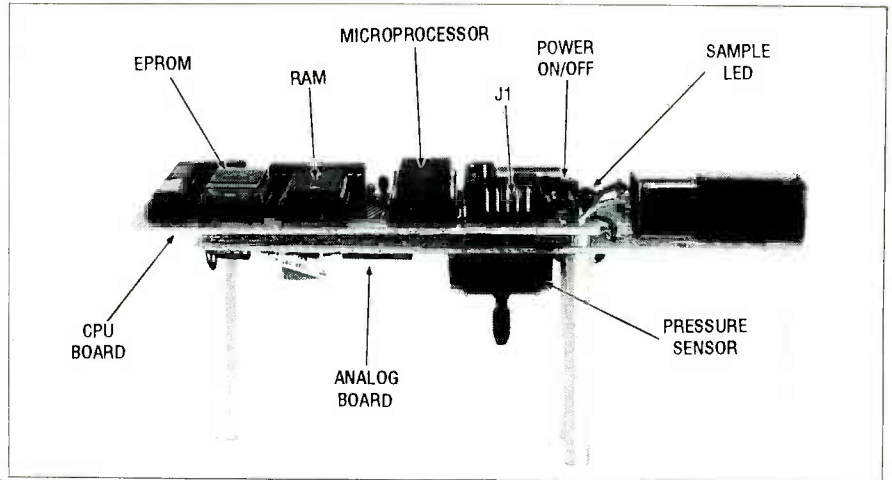


FIG. 11—THE FINISHED ANALOG/CPU ASSEMBLY. It fits in the payload section of a rocket.

LISTING 1

```

000000 c0 00 c5 f8 00 b3 f8 fa a3 7a e3 65 7b 7a 7b 7a
000010 f8 20 b5 b1 f8 06 a5 f8 02 a1 f8 00 b2 f8 f0 a2
000020 f8 02 55 e1 82 f4 a2 e5 02 f2 32 31 f8 fb a3 30
000030 34 f8 fa a3 7a e3 65 7b 7a 05 fe 55 3a 27 11 81
000040 fb 06 3a 1a f8 fb a3 7a e3 65 7b 7a 65 65 f8 00
000050 a9 b9 19 99 fb 10 3a 52 c0 00 db f8 00 a4 b4 3c
000060 5f 34 61 14 3c 63 f8 00 a5 f8 05 b5 c0 01 85 fb
000070 00 3a 6c c0 01 0e f8 05 a1 f8 20 b1 e1 f8 00 73
000080 73 73 51 c4 c4 f8 05 a1 01 32 90 f8 00 51 30 95
000090 f8 05 51 30 bb 21 01 fb 09 32 a1 f8 01 f4 51 30
0000a0 bb f8 00 73 01 fb 09 32 bb f8 01 f4 51 24 94 3a 85 84
0000b0 00 73 01 fb 09 32 bb f8 01 f4 51 24 94 3a 85 84
0000c0 3a 85 c0 00 03 f8 00 a6 b6 a7 b7 f8 20 ad bd c0
0000d0 01 c0 c4 c4 c4 c4 c4 c4 c4 c4 c4 35 e7 37 e4 36
0000e0 ea c0 01 45 c0 01 07 c0 01 00 c0 01 78 c4 c4 c4
0000f0 fc 60 da f2 66 b6 be e0 fe e6 00 01 02 00 c4 c4
000100 96 b4 86 a4 c0 00 76 f8 00 a7 b7 f8 20 ad bd c0
000110 00 df c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 94 bf
000120 84 af 96 be 86 ae 9f 3a 2c 8f 32 36 2f 9e 3a 33
000130 8e 32 26 2e 30 26 9e 3a 3c 8e 32 3e 30 42 94 b6
000140 84 a6 c0 01 a0 f8 00 a4 b4 3c 49 34 4b 14 3c 4d
000150 f8 00 a5 f8 05 b5 94 3a 61 84 fb 01 3a 61 c0 01
000160 70 24 25 95 3a 56 30 5e c4 c4 c4 c4 c4 c4 c4 c4
000170 94 5d 1d 84 5d 1d 30 1e 4d b4 4d a4 f8 00 a9 b9
000180 19 99 fb 30 3a 80 30 a0 c4 c4 c4 c4 c4 c4 c4 c4
000190 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4
0001a0 97 fb 03 3a af 87 fb f0 3a af 2d 2d c0 00 76 17
0001b0 30 ac c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4
0001c0 f8 20 a5 b5 f8 00 55 15 f8 01 55 15 95 fb 28 3a
0001d0 c4 c0 00 db c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4
0001e0 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4
0001f0 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4 c4
000200 c4 ...

```

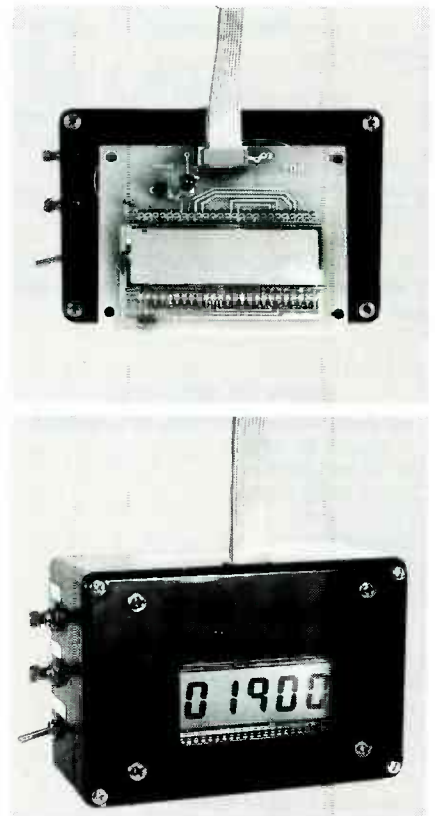
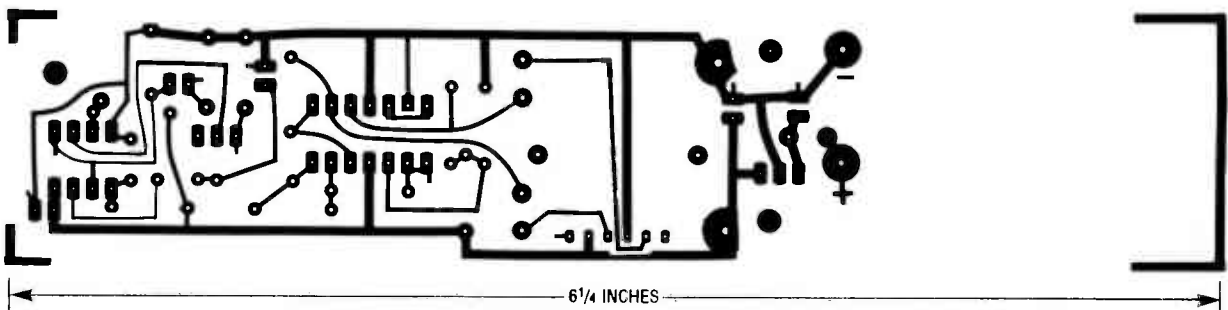


FIG. 12—THE DISPLAY MODULE can be housed in any kind of project case you can find.



THE ANALOG BOARD USES THIS FOIL PATTERN.

surements may be inaccurate. If the potentiometer adjustment is far off, the microprocessor may

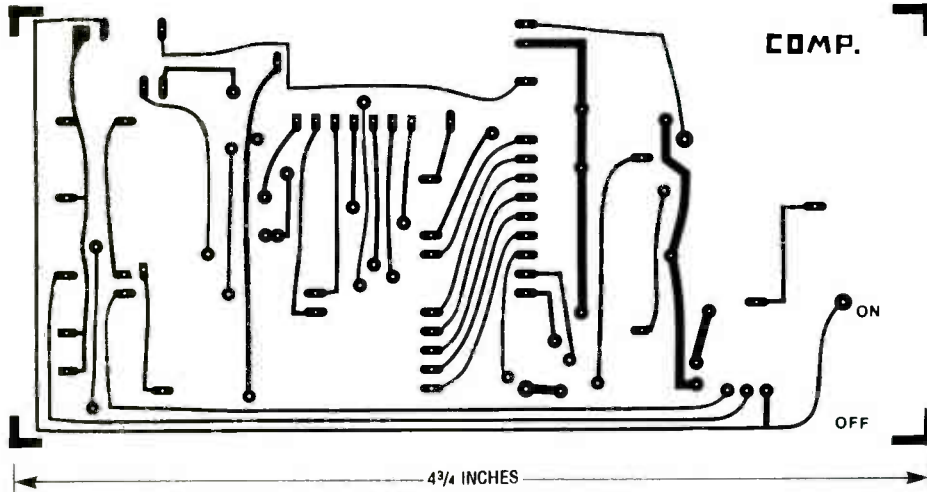
not cycle. If a 50-foot reading cannot be achieved, your altitude above sea level may be excessive.

In that case, simply adjust the value of R16 on the analog board: increase it by 1K to decrease the reading by 1000 feet, or decrease it by 1K to increase the reading by 1000 feet. Note that the potentiometer has enough range to allow for "simulated flights" of thousands of feet.

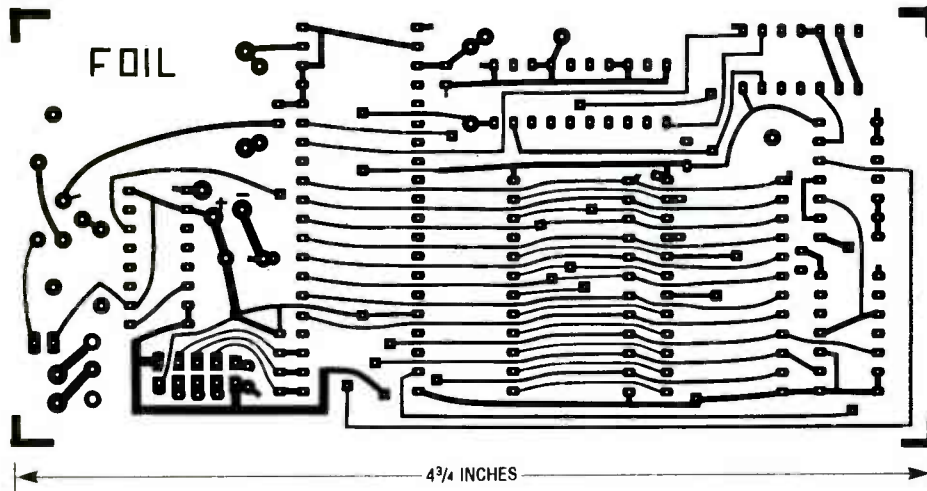
If the unit doesn't run, check for correct parts placement, solder bridges, and other defects. Verify that a 2-MHz signal exists on IC1 pin 1. The crystal circuit has a very high impedance. Any moisture or contamination may prevent oscillation (rosin flux won't hurt). Touching pins 1 or 39 of the microprocessor can cause the program to crash! Spraying the crystal area with clear lacquer is recommended. To reset the program, turn the power off for 5 seconds, then turn it back on. Removing the battery power will erase data. Switching the **PLAYBACK** switch to off will resume data logging at whatever sample was last displayed. The unit must be reset (turn off for 5 seconds, then on) before the next flight.

#### Prepare for launch

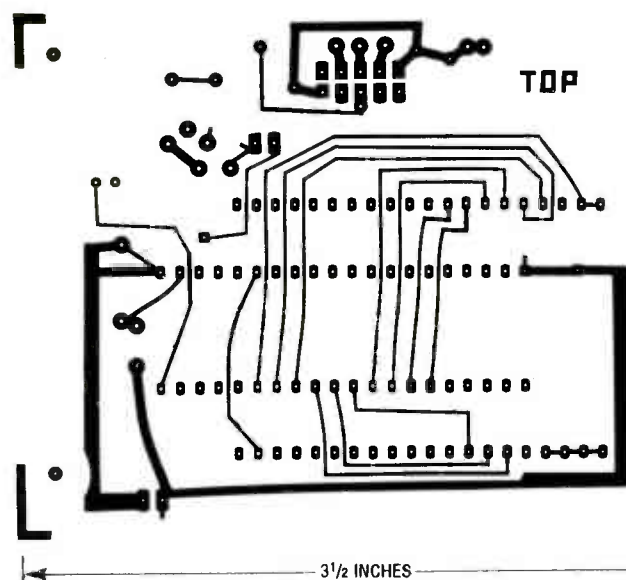
Mount the flight-recorder in the rocket payload section. Pack it securely with foam or some other support so that it will not rattle during flight. Punch several 1/4-inch holes in the body tube near the sensor. An access port may be cut out to allow the ribbon cable to be attached.



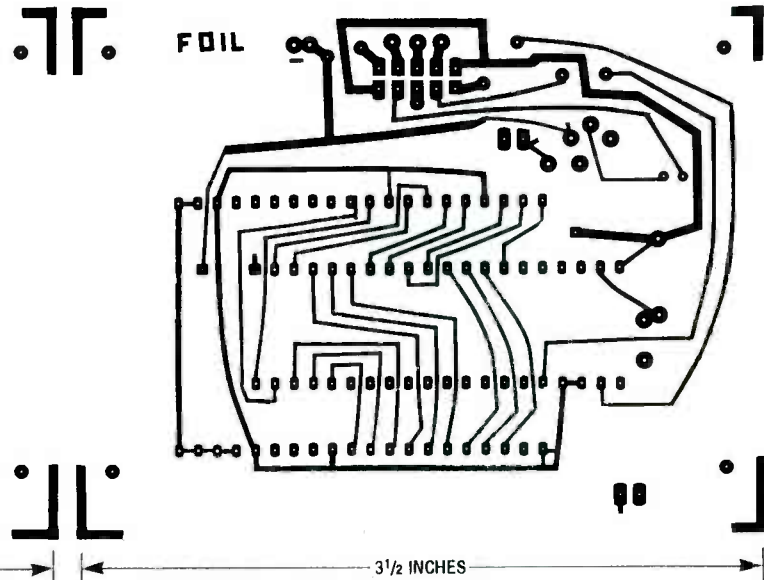
THE COMPONENT SIDE OF THE CPU BOARD.



THE SOLDER SIDE OF THE CPU BOARD.



DISPLAY MODULE COMPONENT SIDE.



DISPLAY MODULE SOLDER SIDE.



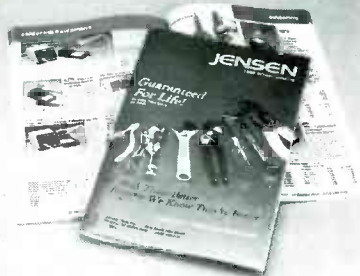
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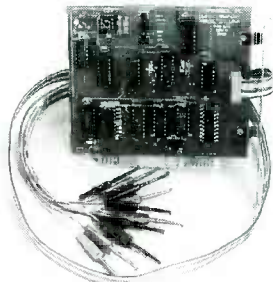
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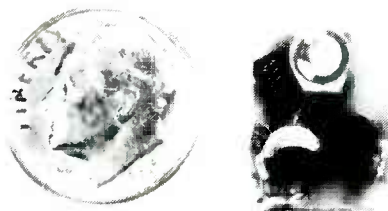
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Activate the unit with the display connected and verify ground calibration (a 50-foot reading). Unplug the display, verify that the sample LED is flashing, and secure the hatch.

Before launching, however, it is important to observe certain safety precautions in order to avoid unnecessary injury or property damage. First of all, always use properly constructed rockets, launchers, and factory-loaded NAR-certified rocket engines. A model rocket should always have a parachute recovery system. Never launch a rocket with a flammable, explosive, or live payload. Make sure that the launch area is free of obstructions such as trees, power lines, and low-flying planes. Also avoid launching rockets on windy days or when clouds will obstruct your view of the rocket. To avoid fire hazards, never launch a rocket from ground covered with dry grass or shrubs. Always make sure that nobody is near the launch site, especially children.

Launch the rocket using a remote ignition system. About four minutes of data will be stored, including the time on launch pad. When you recover the rocket, plug in the display, press the PEAK button, and the peak altitude achieved will be displayed.

Next, switch the playback toggle to the closed position. Press the ZERO button (hold it for two sample LED flashes) and release. This will start playback from location zero at ¼ speed (one sample per second). The flight can be played back as many times as desired by pushing ZERO. The ZERO button may be pushed at any time to restart.

### Conclusion

The collected data may be used to determine the performance of a model rocket. Many modelers are flying high-performance composite motors in their "birds" allowing altitudes of thousands of feet to be reached. Use of the altimeter can help optimize rocket designs to get maximum altitude for a given engine size.

Non-rocket uses of the system might include kites, hot-air balloons, hang-gliders, skydivers, and mountain climbers. Whatever your application, be careful...and have fun!

R-E



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ENGINEERS, TECHNICIANS, AND EXPERIMENTERS who work with state-of-the-art electronics have an almost continuous need to update their test equipment in this rapidly changing field. Higher-frequency, less expensive circuits have brought forth a new generation of inexpensive frequency counters with improved sensitivity that can measure into the microwave region.

With the increased usage of higher frequencies, many quality-built counters are being discarded mainly due to inadequate range. Many of these instruments may only work up to 50–100 MHz, but have valuable features, including ultra-stable timebases that might yield much greater accuracy than could be found in newer, less expensive models.

Enter our solution, a two-stage amplifier and divide-by-10 or -100 prescaler, with 10-segment LED signal strength indicator. It's inexpensive, compact, and can fit into a much larger instrument, like the Hewlett-Packard (HP) Corp. 5245L counter shown in Fig. 1. It has a typical sensitivity of 5 millivolts RMS from 50 MHz–1.6 GHz, and used with such a high-quality, low-range counter, is a practical way to update your gear.

Many high-quality, major brand, low-range counters are available as surplus for \$50–200. They're worth at least that much, if only for the time base, while a newer comparable counter may cost several times as much. The prescaler isn't just for old counters; it's for any counter you'd like to extend the range or sensitivity of, or provide with an LED bargraph indicator.

Several divider schemes were considered for the prescaler, trading off bandwidth against cost; the original goal was 50 MHz–1.5 GHz performance with excellent sensitivity. The prescaler divides (prescales) by 10 from 30–500 MHz, and by 100 from 300 MHz–1.6 GHz, for optimal resolution from a basic counter.

If you want to use a direct 50-MHz counter with 1-Hz resolution and a one-second gate to measure up to 450 MHz, you'd have to prescale by 10 for a 7-digit resolution in one second, compared with 6-digit resolution if you prescaled by 100. To maximize display resolution requires that the prescaler be able to divide by 10 to reach 500 MHz. Binary dividers are cheaper and more common than decimal versions, and prescaling by 256, 512 or 1024 is easier than by 100 or

1000, but decimal division lets you move a decimal point mentally, and easily understand the reading.

## Circuit description

Figure 2 shows the block diagram of the prescaler, and Fig. 3 shows its schematic. IC5 has both  $\div 2$  and  $\div 5$  outputs, the one in use being selected using S2. With S2 set to  $\div 100$ , IC3 is a  $\div 4$ , and IC4 and IC5 are  $\div 5$ 's, for a  $\div 100$ . With S2 set to  $\div 10$ , the input is routed around IC3 to IC4 by PIN diode D4 (acting as a bandswitch). IC4 is a  $\div 5$  counter, and IC5 is a  $\div 2$  counter, creating a  $\div 10$  counter overall. IC1 and IC2 are broadband Monolithic Microwave IC (MMIC) amplifiers used on both ranges. The output of IC1 drives LED bargraph DSP1, the RF signal strength indicator. It's very useful as a relative field strength meter, for peaking the output of a circuit, or just as a convenient indication of signal presence.

In the prescaler, D4 is used for bandswitching. When reverse-biased, it's capacitance is almost constant from 0.65–0.75 pF. When forward-biased, it's capacitance rises rapidly to 6 pF or more. Its cathode is kept at about +2.5 volts DC by voltage divider R7-R8; the drop across L4 is neg-

ligible. S2-a and S2-b switch the anode of D4 between +5 volts DC and ground, so there's  $\pm 2.5$  volts DC across D4, relative to the cathode.

With S2 set to  $\div 10$ , D4 is forward-biased, so its capacitance increases as noted above, and the total impedance looking into the anode of D4 goes down, routing the output of IC2 through D4 and C9 to IC4. When S2 is set to  $\div 10$ , IC3 is off, since pin 1 ( $V_{CC}$ ) is connected to +5 volts DC through R5. The R5-IC3 voltage divider reduces the potential at pin 1 to about 1.25 volts DC, turning IC3 off. However, you might wonder: Why not just turn off IC3 altogether?

The reason is that C10 still looks into pin 7 (OUT 2), and would see too low an impedance if IC3 were totally off, and too much of IC2's output would be diverted away from IC4. The value of R5 was found by trial-and-error, to maximize the impedance looking into pin 7 (OUT 2), while keeping IC3 off. Conversely, when S2 is on  $\div 100$ , IC3 is now on, since it's now connected to +5 volts DC through R5 and R6, and their parallel value is under 1.5 ohms. The cathode of D4 is still at +2.5 volts DC, but the anode is effectively grounded, so D4 is reverse-biased.

The capacitance of D4 is now about 10% of its forward-biased value, increasing capacitive reactance by about a factor of 10. The impedance looking into the anode of D4 thus increases, and almost no output from IC2 reaches IC4 directly. The output of IC2 enters IC3, is divided, and passed to IC4.

To avoid splitting the output of IC3 between IC4 and the path along C9, trial-and-error again resulted in a high-impedance path looking into the top of C9. In other words, the high impedance of a reverse-biased D4 works both ways. It keeps the output of IC2 from being diverted to IC4, while keeping the output of IC3 from being diverted backward. The loss of output of IC3 through C9-L4-R8 is minimal.

The input enters through J1 and is AC-coupled through IC1 and IC2. Avantek MSA0104 MMIC amplifiers. They have double grounds and indirect biasing, through R1-L1-C26 for IC1, and



FIG. 1—THE PANEL-MOUNTED VERSION of the prescaler, in an HP 5245L frequency counter. The HP5245L is often available as surplus for about \$200, and the prescaler is a good way to update it.

R2-L2-C15 for IC2. Carbon-composition resistors R1 and R2 temperature-compensate collector current in IC1 and IC2. L1 and L2 prevent R1 and R2 from affecting the load impedance, which would reduce amplifier gain. IC3 is an NEC UPB582  $\div 4$  MMIC prescaler, with R3, C8, C9, and D4 as its bypass for the  $\div 10$ . D4 is a Motorola MPN3401 PIN diode, while R7 and R8 produce a +2.5-

volt DC bias at the cathode (the output) of D4 via L4. D4 is biased on or off by the 0 or 5 volts DC switched through L3 at its anode.

Device IC4 is a Motorola MC12009 emitter-coupled logic (ECL)  $\div 5$  prescaler, with a built-in ECL-to-TTL output level converter. R9 keeps the circuit stable with no signal input. IC5 is a TI 74S196 presetable binary/de-

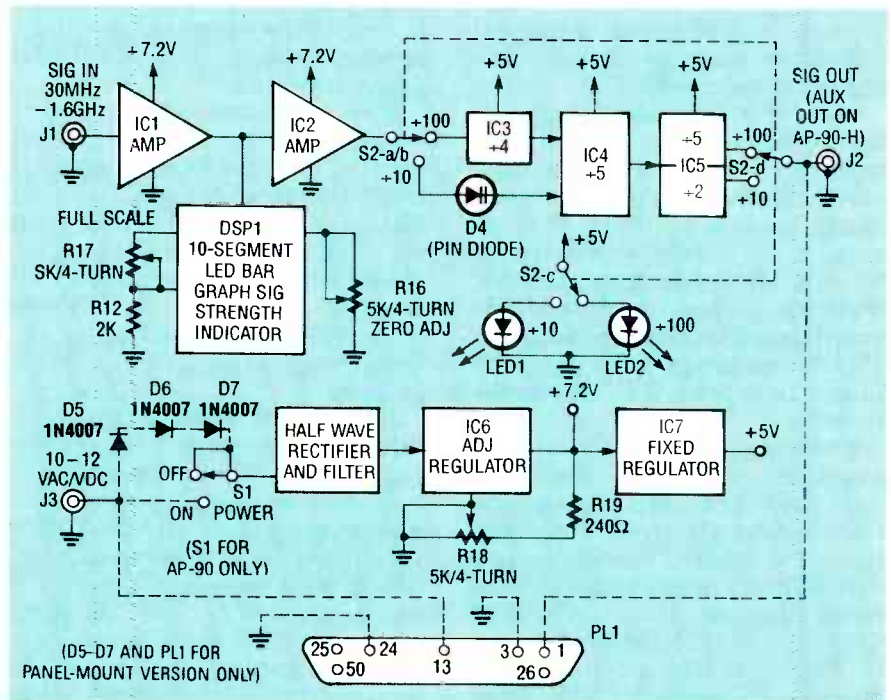


FIG. 2—THE BLOCK DIAGRAM OF THE prescaler. IC1 and IC2 are MMIC amplifiers. IC3 is a  $\div 4$  counter, IC4 is a  $\div 5$  counter, and IC5 has  $\div 2$  and  $\div 5$  outputs selected by S2. With S2 on  $\div 100$ , the input passes through IC3 and IC4, and IC5 is a  $\div 5$  counter. With S2 on  $\div 10$ , the input goes around IC3, through PIN diode D4 to IC4, and IC5 is a  $\div 2$  counter. IC1 drives DSP1, the RF signal indicator. PL1 is for the panel-mounted version only.

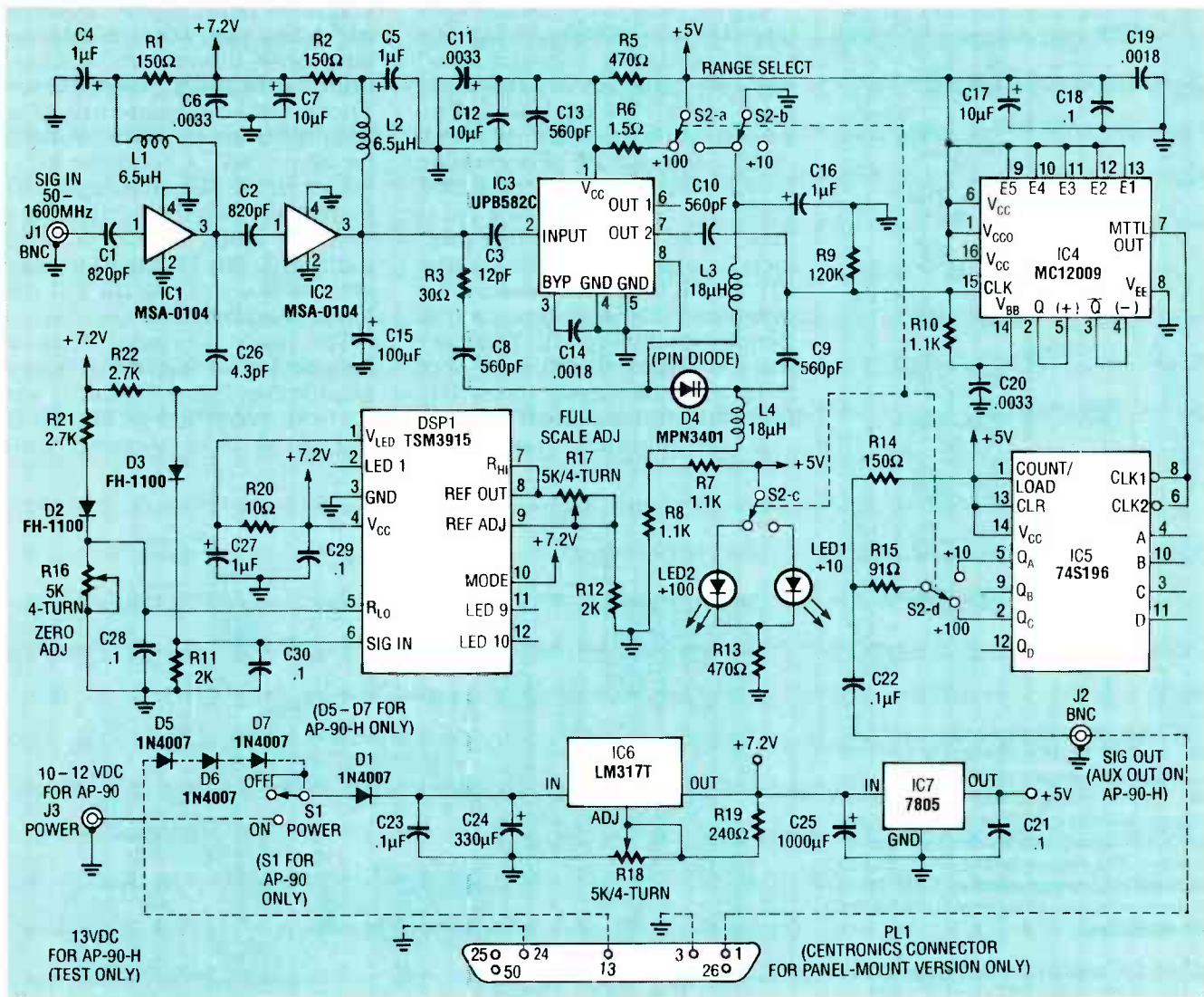


FIG. 3—THE SCHEMATIC DIAGRAM OF THE PRESCALER. DSP1 is a TSM3915 10-segment LED bar-graph display; R16 and R17 adjust zero and full-scale. D4 performs band-switching; it's reverse-biased capacitance is 0.65–0.75 pF, and over 6 pF forward-biased. With S2 on = 10, D4 is forward-biased, so its impedance goes down, and it passes the signal to IC4. IC3 is off, but pin 1 (V<sub>CC</sub>) is at 1.25 volts DC to raise the impedance on pin 7 (out 2). With S2 on = 100, D4 blocks the signal, and it's now passed to IC3.

cade counter. It has separate ÷2 and ÷5 sections; the prescaler drives both, and you select the desired output using S2. R14 and R15 shape and pull up the output; the output will be 1–2 volts peak-to-peak into a load of 50 ohms or more.

Display DSP1 is the Three-Five Systems, Inc. TSM3915 (formerly the National Semiconductor NSM3915) 10-segment LED bar-graph display; Fig. 4 shows the block diagram. It has an on-board monolithic IC with an adjustable internal voltage reference, high-impedance input buffer, accurate 10-step voltage divider, and 10 comparators. R11 and R22 bias D3 as an RF level

detector coupled by C26 from IC1. D2 is directly connected to the high impedance input buffer at pin 6. Within DSP1, the signal is applied to 10 comparators, each biased differently by the precision voltage divider, and driving one LED.

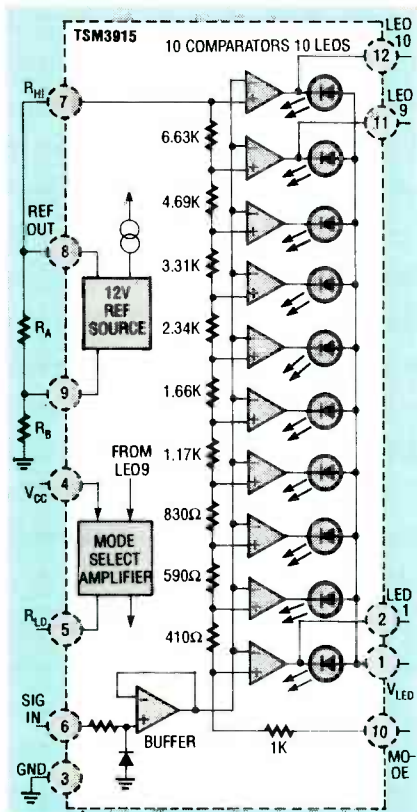
A low-voltage reference signal from R21-D2-R16 is applied to pin 5, to offset the input bias voltage making R16 the zero adjustment. R17 sets full-scale sensitivity by varying the internal reference voltage across the comparators. The current from REF out (pin 8) determines the display current and brightness. About 10 times this current is drawn through a lit segment, and

is fairly constant despite voltage and temperature changes.

The display is logarithmic, with segment thresholds at 3-dB intervals. If you remove V<sub>CC</sub> from MODE (pin 10) and join MODE (pin 10) and LED 9 (pin 11), the display changes from a bar graph to a dot graph, with only the top LED of a reading lit. That saves current, but the bar graph is easier to read.

The power supply provides regulated +7.2 volts DC from IC6 for IC1, IC2, and DSP1, and +5 volts DC from IC7 for all else. IC6 is an LM317T adjustable regulator set by R18 and R19. The input is polarity protected by D1. Capacitor C23 bypasses high-frequencies avoid instability, and C24 filters 60-Hz ripples. Power jack J3 needs a center-positive, 2.1–2.5-millimeter coaxial plug.

The maximum current through DSP1 with all segments lit is about 400 milliamps. An



**FIG. 4—THE BLOCK DIAGRAM OF THE TSM3915 10-segment LED bar-graph display.** The on-board IC has an adjustable voltage reference, high-impedance input buffer, 10-step voltage divider, and 10 comparators. The display is logarithmic; each segment represents another 3 dB. Maximum current with all segments lit is about 400 millamps.

AC-to-DC adaptor should provide +10–+12 volts DC under load at J3, but be careful, since excess voltage will burn out IC6. Such adaptors aren't regulated, so their voltage may vary greatly with load. The prescaler works fine with an adaptor rated at +9 volts DC and 500 millamps, that actually delivers +10.5–+11.5 volts DC. Diodes D5–D7 provide an additional 1.8–2.1 volt DC drop, to avoid overheating IC6.

**Construction**

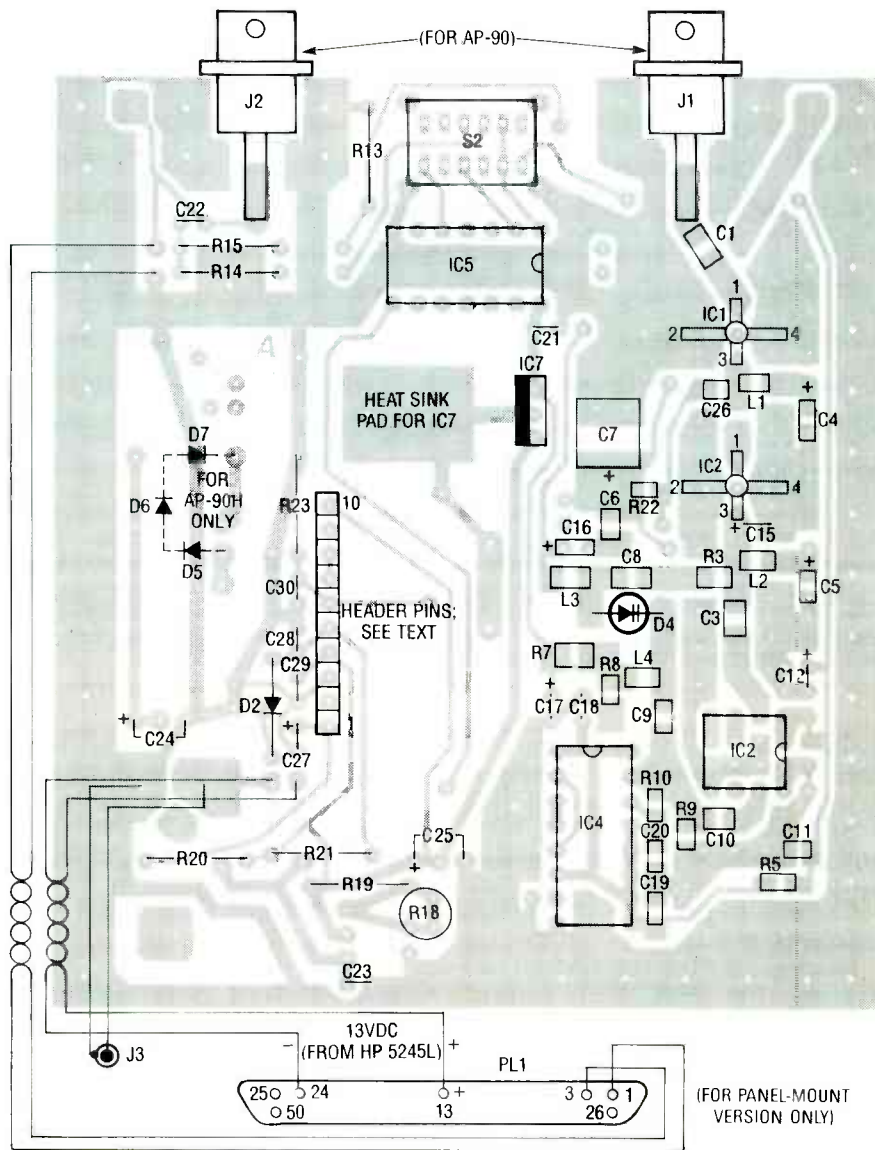
Build the PC board for the pre-scaler exactly as shown. Don't drill any additional holes, or modify the microstrip foils. If you do, you'll ruin the ground plane needed to achieve the 1.6-GHz bandwidth and excellent sensitivity. The cabinet-mounted and panel-mounted versions were designed for a 3.8×3.35-inch, double-sided, plated-through PC board, with solder masks and component screens on each side.

The PC board was laid out with tape 4× actual size, using 50-ohm microstrip signal paths, size calculated for a 0.062-inch glass-epoxy FR4 PC board. The 29 surface-mount devices (SMD's) improve RF performance by reducing size, component lead inductance, impedance mismatch, and poor grounding common in larger parts. MMIC's like IC1 and IC2 are mandatory for microwave circuits, and can be handled manually with practice; the prototypes shown here were built with no special tools. The parts are very small, so be careful.

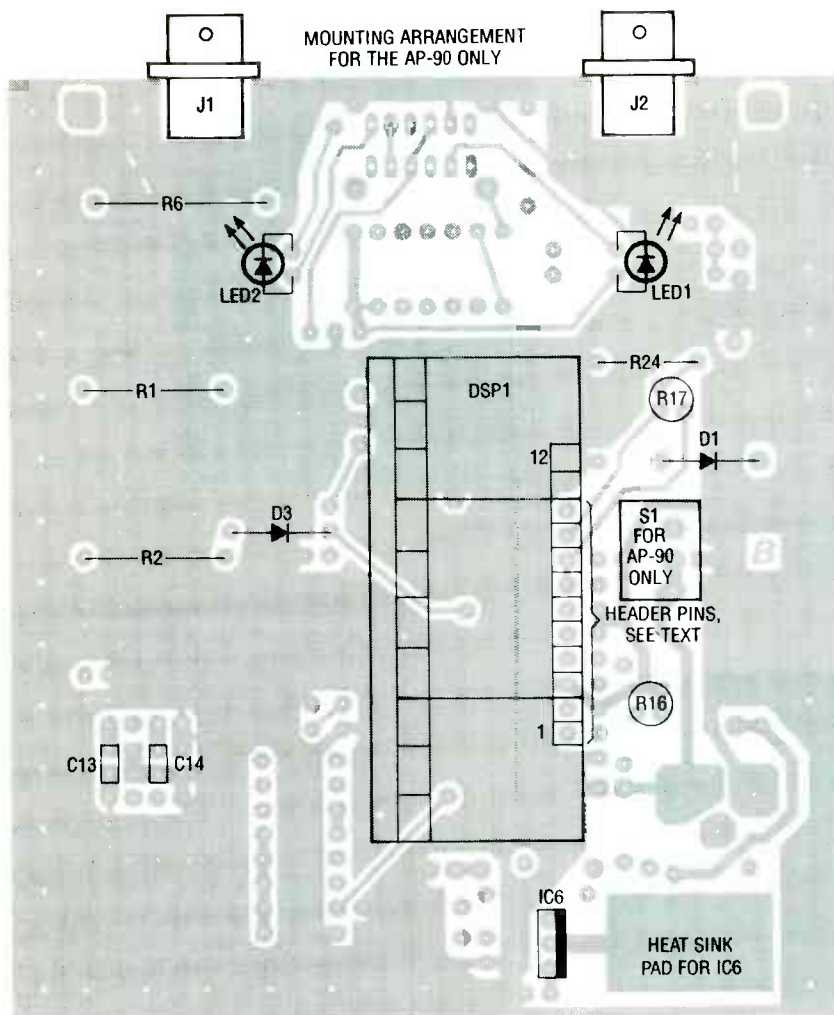
At bare minimum, you'll need a

magnifier lamp, small-tip soldering iron, tweezers, miniature long-nose pliers, and a sharp knife with a small, pointed blade. There are small vacuum tools with different tip sizes available for about \$10; a complete kit of solder creme dispenser gun with cartridges (called caplettes), and vacuum tools, is \$75 (see the parts list). The PC board is available, or you can use the foil patterns provided here.

The parts-placement diagram for side A is shown in Fig. 5, and for side B in Fig. 6. Install J1 and J2 first, modified as shown in Fig. 7, with a 1/16-inch wide



**FIG. 5—PARTS PLACEMENT DIAGRAM FOR side A of the PC board.** C15 has a hole for the negative lead; the positive lead is soldered to the foil where R3 meets L2. On IC1 and IC2, the dots are the outputs (pin 3); the input (pin 1) is opposite, and pins 2 and 4 are the grounds. D4 is black, rectangular, and has a brown ridge on the cathode end.



**FIG. 6—PARTS PLACEMENT DIAGRAM FOR side B of the PC board. In the cabinet-mounted version, the header pins protrude from side A to holes 1–10 of DSP1 on side B; the separator is on side A. In the panel-mounted version, the header pins are inserted into side B; their other ends go to holes 1–10 on DSP1, with the separator on side B.**

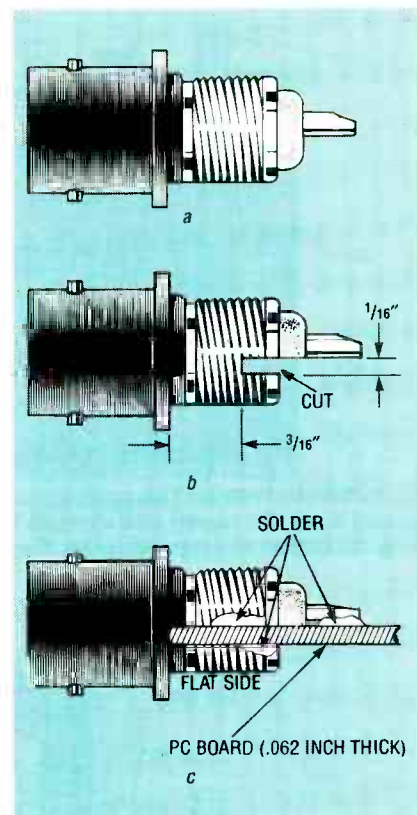
groove. Use a medium iron for them, and the small iron elsewhere. The kit in the parts list has IC socket pins for IC3 and IC4, to shorten the leads and get them closer to the ground plane for better frequency response. For IC5, use a regular 14-pin DIP socket, since it operates over a lower frequency range.

Install the SMD's next; note the polarity of amplifiers IC1 and IC2, tantalums C4, C5, C7, and C16, and LED1 and LED2, and install all parts from smallest to largest. IC1 and IC2 should both have dots indicating their outputs (pin 3); the input (pin 1) is opposite this, and pins 2 and 4 are the grounds. With the dot on pin 3 pointing toward the bottom as in Fig. 5, pin 1 points upward, pin 2 points left, and pin 4 points right.

For the SMD tantalums, C4, C5, and C16 are the same size,

while C7 is much larger. In the prototypes and the kit in the parts list, C4, C5, and C16 are orange in the center and silver on each end. They have a small tip on the positive end, and a green dot on the top side. C7 is yellow, with a brown band on the top of the positive end. Capacitor C15, at the middle right, will partially block IC2 and L2, so install them first. There's a hole for the negative lead of C15, but the positive lead is tack soldered to the foil where R3 meets L2. Insert the negative lead into its proper hole, and bend the positive lead outward at right angles. Diode D4 is black, rectangular, and has a brown ridge on the cathode end; the brown ridge faces to the right.

Install LED1 and LED2 last in the prescaler. For the case-mounted version, insert the LED's into their PC board holes



**FIG. 7—BNC SOCKET MODIFICATION for the cabinet-mounted version. In (a) a side view is shown of a female BNC panel-mount socket. In (b), a slot is cut in the threads with a hacksaw or file. In (c), the slot fits snugly over its PC board notch. Solder it on both sides of the PC board; the center pin goes on side A.**

without soldering. Hold them in place with your fingers and pull the leads through the holes, until they both almost touch the surface of side B. Fold the leads over slightly, so they can't fall out. Insert the PC board into the case, with side A facing out. Bend the LED leads back to vertical so they slide freely, maneuver the LED's so they protrude through their holes in front, then solder and trim. If you remove the PC board from the case, the LED's should slide out freely. When you put the PC board back in the case, the LED's should slide back into their holes.

For the panel-mounted version, don't install the LED's until you attach J1 and J2 to the faceplate, and are ready to attach the PC board. Pull the LED's through their holes in the PC board, and bend the leads to hold them in place. Insert the center pins and ground lugs of J1 and J2 into the holes next to the notches, and bolt the bottom of the PC board to

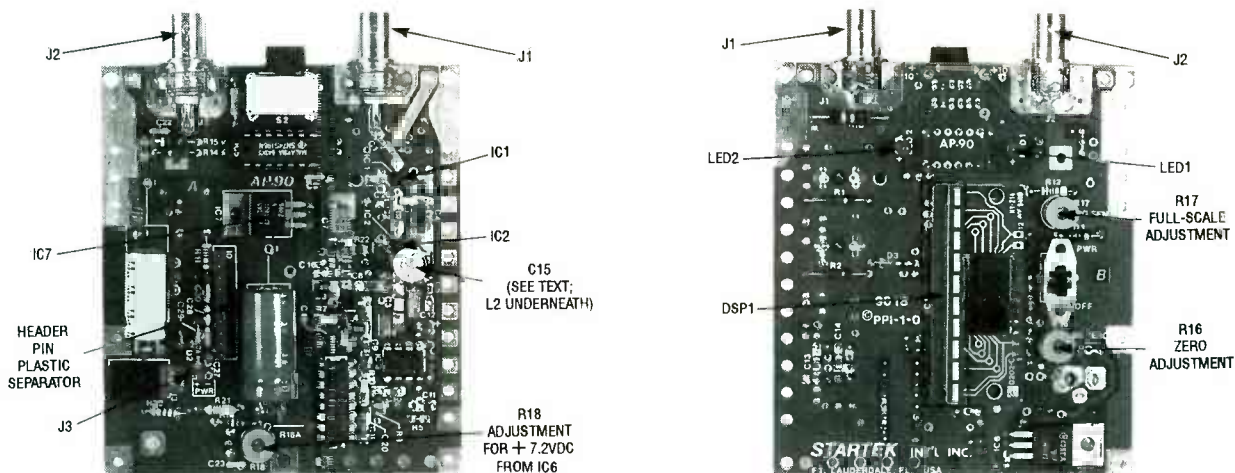


FIG. 8—PROTOTYPE OF THE CABINET-MOUNTED version; side A appears in (a), side B appears in (b). The header pins protrude through from side A, and are soldered to DSP1 using the bottom 10 pin holes on the display PC board.

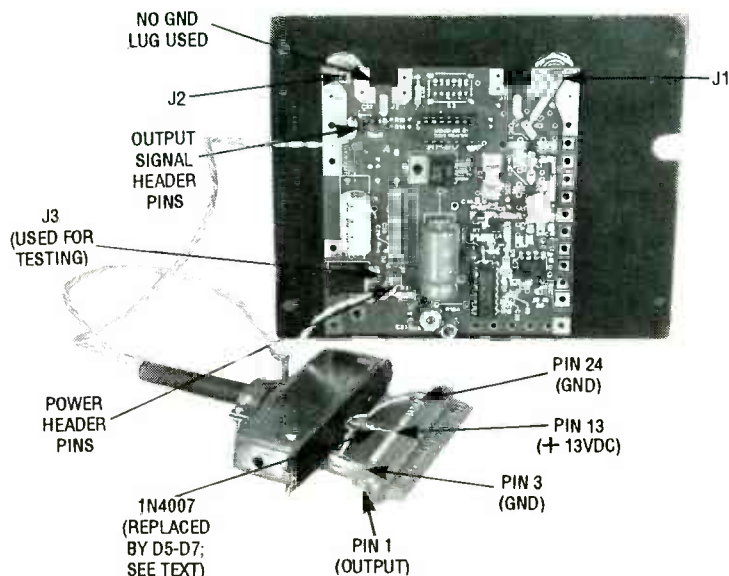


FIG. 9—PROTOTYPE OF THE PANEL-MOUNTED version, showing side A. The header pins are inserted into side B; the separator is on the same side. PL1 connects two twisted pairs; the output to the HP 5245L is from the header pins at upper left, and the +13 volts DC from the HP 5245L to those at lower right. The 1N4007 on pin 13 of PL1 has been replaced by D5-D7 at S1's location (see text), to avoid damaging IC6. Use heatshrink tubing with all four wires to avoid shorts.

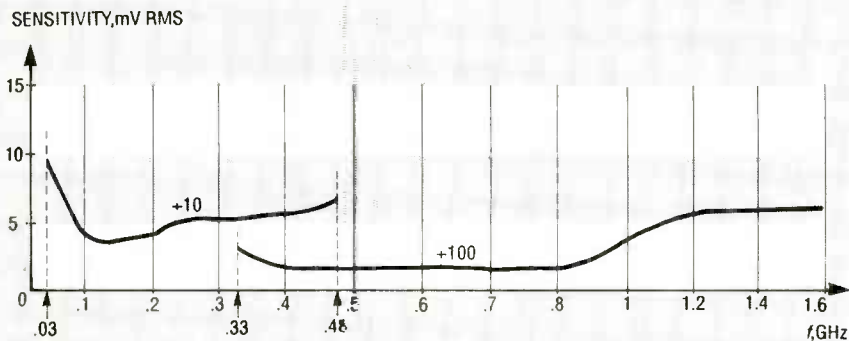


FIG. 10—SENSITIVITY CURVES FOR BOTH the  $\pm 10$  and  $\pm 100$  ranges. The  $\pm 10$  range covers 30-480 MHz, and the  $\pm 100$  range covers 330 MHz-1.6 GHz.

the faceplate with nylon washers and a nonconductive spacer. Solder the center pins and lugs for J1 and J2; use two lugs for J1, and one for J2. When the PC board is attached to the faceplate, maneuver the LED's as before, solder and trim.

If you have no SMD tools, hold the SMD in place with a small, sharp knife, a pencil, or a probe. Tack solder one side to hold it in place so you can solder the remainder with both hands; then, resolder the first side. There are kits of SMD tools available that can make working with the devices easier.

Solder creme is powdered solder mixed with flux. With a gun dispenser, place a very tiny spot on each SMD solder pad, and position the SMD with a vacuum tool; it should stick to the solder creme. Heat the foil, and the solder creme should melt; never heat the solder creme directly.

Figure 8-a shows side A of the cabinet-mounted prototype, and Fig. 8-b shows side B. In Fig. 8-a, IC7 has been folded over to lie on its heatsink pad. You can't bolt the heatsink to the PC board in the precaler, since DSP1 is in the way, but even if you could, it's unnecessary. The center pins of J1 and J2 are on side A; both the threads and center pins were separately soldered. In Fig. 8-b, IC6 has been folded over like IC7, but also needn't be bolted down. The header pins protrude through from side A, and are soldered to holes 1-10 on DSP1 on side B; the plastic separator is on side A.

Figure 9 shows side A of the

## PARTS LIST

All resistors are 1/4-watt, 5%, carbon-composition or film, unless otherwise noted.

R1, R2—150 ohms carbon-composition  
 R3—30 ohms, SMD  
 R4—unused  
 R5—470 ohms, SMD  
 R6—1.5 ohms  
 R7, R8, R10—1100 ohms, SMD  
 R9—120,000 ohms, SMD  
 R11, R12—2000 ohms, 1%  
 R13—470 ohms  
 R14—150 ohms, 10%  
 R15—91 ohms, 10%  
 R16—R18—5000-ohm, 4-turn, sub-miniature, PC-mounted potentiometer  
 R19—240 ohms  
 R20—10 ohms  
 R21—2700 ohms  
 R22—2700 ohms, SMD

### Capacitors

C1, C2—820 pF, SMD  
 C3—12 pF, SMD  
 C4, C5, C16—1  $\mu$ F, tantalum, SMD  
 C6, C11, C20—0.0033  $\mu$ F, SMD  
 C7—10  $\mu$ F, tantalum, SMD  
 C8—C10, C13, C14—560 pF, SMD  
 C12, C17—10  $\mu$ F, tantalum, axial leads  
 C15—100  $\mu$ F, electrolytic, axial leads  
 C18, C21—C23, C28—C30—0.1  $\mu$ F, monolithic ceramic, axial leads  
 C19—0.0018  $\mu$ F, SMD  
 C24—330  $\mu$ F, 25-volt, electrolytic  
 C25—1000  $\mu$ F, 10-volt, electrolytic  
 C26—4.3 pF, SMD  
 C27—1  $\mu$ F, 16-volt, tantalum

### Inductors

L1, L2—6.5  $\mu$ H, SMD  
 L3, L4—18  $\mu$ H, SMD

### Semiconductors

D1, D5—D7—1N4007 silicon diode  
 D2, D3—FH-1100 diode  
 D4—Motorola MPN3401 PIN diode  
 DSP1—Three-Five Systems TSM3915 10-segment LED bargraph display

LED1, LED2—subminiature red LED  
 IC1, IC2—Avantek MSA-0104 MMIC amplifier  
 IC3—NEC UPB582C MMIC divide-by-4 prescaler  
 IC4—Motorola MC12009P ECL two-mode prescaler  
 IC5—TI 74S196 presettable binary/decade counter  
 IC6—LM317T adjustable 1.25–37-volt DC regulator  
 IC7—LM340T-5 or 7805 fixed 5-volt DC regulator

### Other components

S1—SPDT PC-mount slide switch (used in the cabinet-mounted version)  
 S2—4PDT right-angle PC-mount slide switch (used in the cabinet-mounted version)  
 S2—4PDT PC-mount slide switch (for the panel-mounted version)  
 PL1—Centronics 50-pin male plug with hood  
 J1, J2—UG1094-U female BNC socket (see text)  
 J3—2.1-millimeter coaxial power jack

**Miscellaneous:** Case for the cabinet-mounted version (two-piece anodized aluminum, four machine screws, with specially punched and printed front), red lens for DSP1 (0.03 × 1 × 3-inches), front panel (optional for the panel-mounted version), three BNC socket solder lugs, 4-40 × 0.25-inch black Phillips pan head screws (for the cabinet-mounted version enclosure), two 6-32 × 0.5-inch black Phillips pan head screws, two 8-32 × 0.5-inch black Phillips pan head screws, 4-40 nylon locknut, 4-40 × 0.3-inch threaded spacer, nylon washer, 2 feet of #22 stranded twisted-pair wire, two BNC socket lock-washers, one 10-pin header pin with plastic separator (for both

the cabinet-mounted version and the panel-mounted version), two 2-pin header pins with plastic separators (for the panel-mounted version), heatshrink tubing, AC power adapter with an output of 10–12 volts DC at 400 mA.

**NOTE:** The following items are available from STARTEK International, Inc., 5200 N Federal Hwy., Suite #2-1181, Ft. Lauderdale, FL 33308, (305) 783-0008 or (800) 638-8050. A complete set of all parts (#AP-90K) for the cabinet-mounted version is \$99.95, an enclosure (#CAB-90) is \$25.00, and the AC adaptor (#AC-90) is \$9.00. A factory-assembled and tested version with the aforementioned items (#AP-90) is \$179.00. The telescoping antenna with BNC plug (#TA-90) is \$12.00, and the PC board (#PCB-90) only is \$25.00. All seven IC's (#ICS-90), including voltage regulators and DSP1, is \$55.00. A complete kit of parts for custom installation of the panel-mounted version into the HP 5245L (#AP-90-HK) is \$159.00, and an assembled and factory-tested version (#AP-90-H) is \$199.95. A partially assembled kit (SMD components installed) is available. Call Startek or send SASE for information. For SMD tools, a Vac Tweezer pick-and-place tool kit (#VT-1) is \$9.50, and a Dot.Maker solder creme dispenser kit containing the Vac Tweezer kit and an assortment of about 20 solder creme caplettes (#DMK-1) is \$75.00. Add 5% (a minimum of \$4.00 to a maximum of \$10.00) for shipping/handling. Visa, MasterCard, C.O.D., cash, or money orders accepted; allow three weeks for personal checks.

panel-mounted prototype. PL1 is connected to the PC board by two twisted pairs and two pairs of header pins. The output fed back into the HP 5245L comes from the header pins at upper left. The upper pin is the output, the lower pin is ground. Power goes into the header pins at lower left: the left one goes to the +13 volts DC from the HP 5245L, and the right one is ground.

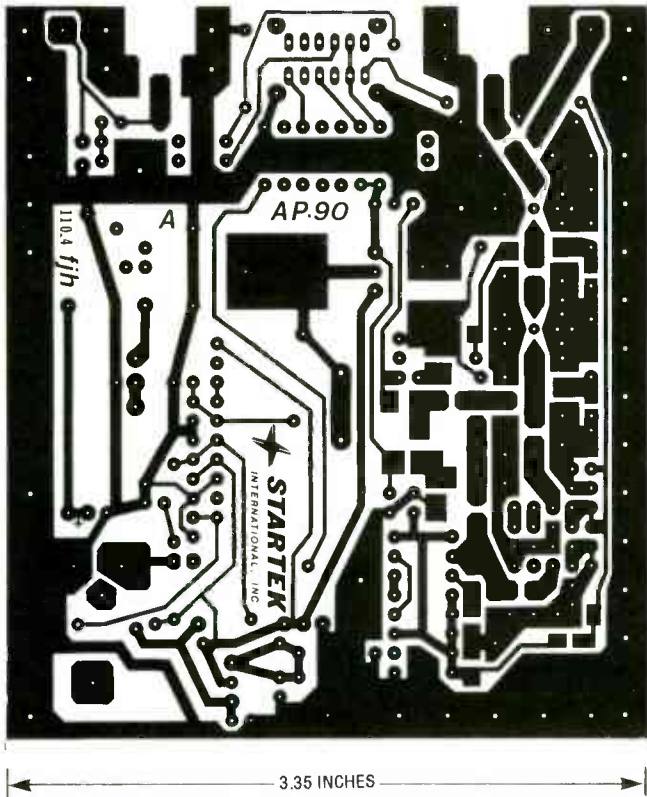
The prototype was built before using D5–D7; the anode of a

1N4007 was soldered to pin 13 of PL1, and the cathode to the positive power wire (blocked by the black heatshrink tubing). PL1 is a standard male Centronics plug. Cover both ends of all four wires with heatshrink tubing to avoid shorts. However, one 1N4007 didn't provide a sufficient drop, so D5–D7 were used thereafter.

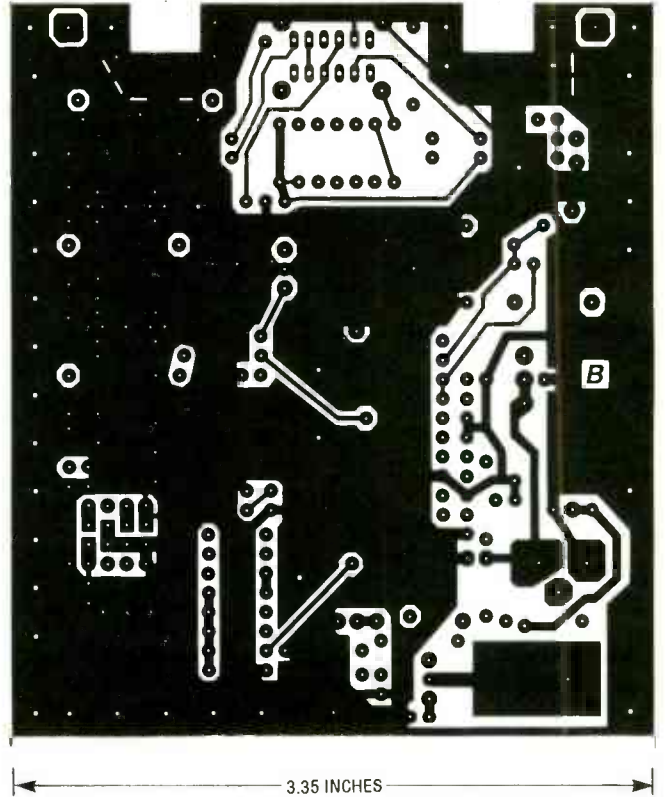
Figures 2, 3, and 6 all show D5–D7; in the panel-mounted version they replace S1, to pro-

vide an additional 1.8–2.1-volt DC drop, as mentioned above, to reduce the +13 volts DC from the HP 5245L. IC6 doesn't overheat to the point of exceeding specification. The drops across D1 and D5–D7 reduce the +13 volts DC from the HP 5245L to +10.2–10.6 volts DC, enough to run IC6 with minimum heat dissipation.

To install D5–D7, wrap the cathode of D5 around the anode of D6, and the anode of D7



COMPONENT SIDE OF THE PRESCALER.



SOLDER SIDE OF THE PRESCALER.

around the cathode of D6, solder and trim. Insert the anode of D5 and the cathode of D7 into their PC board holes, and leave enough lead length on side B to bend D5–D7 flat to the PC board.

In the panel-mount version, install the DSP1 header pins with the plastic separator on side B (the separator is on side A for cabinet installation) to hold

DSP1 off the PC board and flush with the red lens and panel.

The PC board and red lens is a precise fit inside the case and shouldn't move around. In the panel-mounted version, the lens is sandwiched between DSP1 and the rear of the faceplate, and has a hole drilled in its bottom for the screw that attaches the PC board to the bottom of the faceplate.

The lens goes between the rear of the faceplate and the nylon washer at the base of the nonconducting spacer.

#### Power-on checkout

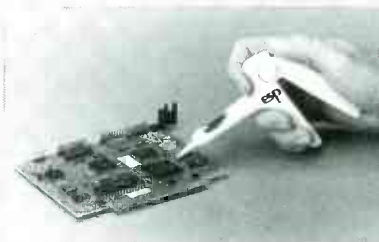
Turn the power on, and check for proper voltages:

- At J3, +10–+12 volts DC, input power.
- At the output of IC6, +7.1–+7.3 volts DC (adjust R18).
- At the output of IC7, +4.9–+5.1 volts DC.
- At the outputs of IC1 and IC2, a bias of 4.6–4.7 volts DC (with no input signal).

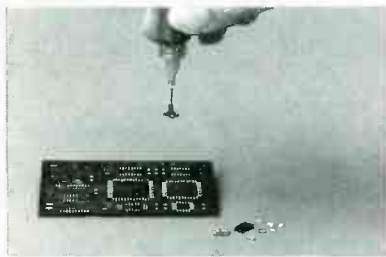
For the panel-mounted version, J3 is included to let you test it without connecting it to the HP 5245L. If all voltages are right, adjust R16 to zero the bar graph, and R17 for full scale. The two potentiometers interact, but you should get a good setting with a signal generator and some experimenting. The bar graph varies with frequency, but is a convenient relative RF signal strength indicator. With careful assembly, sensitivity should be 1–9 millivolts RMS from 50 MHz–1.6 GHz, consistent with the curves shown in Fig. 10. R-E



a



b



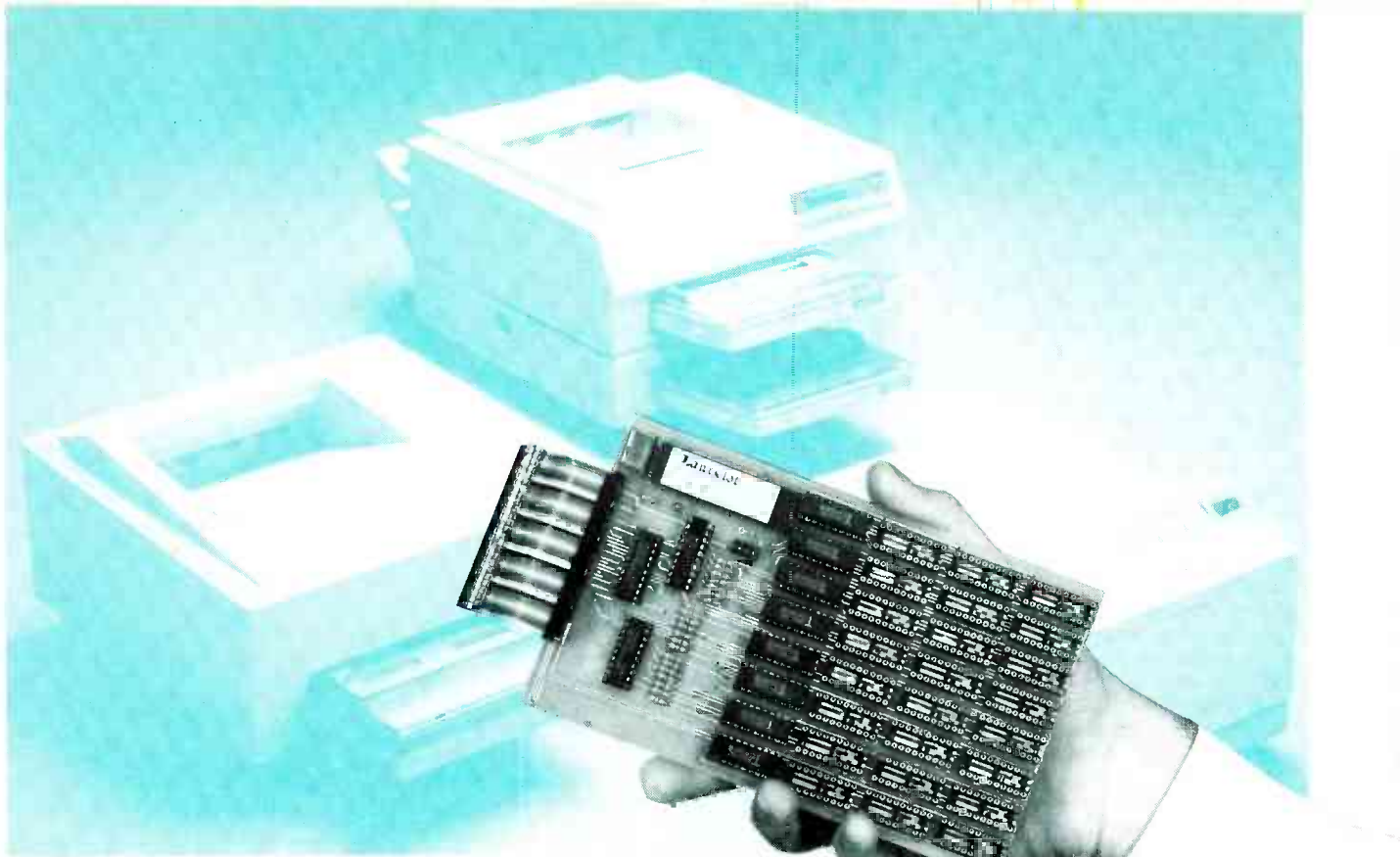
c



d

IF YOU WANT SMD TOOLS, (a) shows a kit mentioned in the parts list. Solder creme is powdered solder mixed with flux. With the gun in (b), place a spot on each pad, and position the SMD with the vacuum tool in (c); it should stick to the solder creme. Heat the foil, and the solder creme should melt. In (d) a close-up of the gun and three caplettes is shown.





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for your LaserJet Model IIP/III printer.***

**BILL GREEN**

LASER PRINTERS HAVE BEEN AROUND for some time but, until recently, they have been expensive. About a year ago Hewlett Packard introduced their LaserJet IIP, the first low-priced entry in the market. It lists for \$1495 but can be purchased through mail-order outlets for under \$1000, making it a truly "personal" laser printer. The Model IIP has many of the features of HP's newest and substantially more expensive entry, the Model III. The Model IIP falls short of the Model III in that it is half as fast and has half the built-in memory.

The Model IIP has 512K of memory built in, but that amount won't even allow you to

print a full page of graphics at 300 dpi (300 dots-per-inch) resolution, let alone store a couple of softfonts (downloadable typefaces) in the printer. The fact is, laser printers are powerful in such applications as desktop publishing and for printing the output of CAD and CAM software (the PC board foil patterns for this project were printed on a LaserJet IIP), as well as for everyday printing. But having only 512K of memory severely limits the power.

You can, of course, expand the memory in the printer, but the cost to purchase 4-megabytes of memory from Hewlett Packard will set you back a cool \$2000.

The prices of laser printers have come down, and they now fit into the personal-computer market, but the price of expansion memory has kept the cost of laser printing well above what it should be.

The memory-board construction project which we will detail here can add up to 4-megabytes of additional memory to your LaserJet IIP, and also works with Hewlett Packard's newest laser printer, the Model III. A kit is available to build it (see parts list) for under \$100. Memory is not included at that price, but is available for around \$56 per megabyte through a number of mail-order sources. You can now add up to 4-megabytes to your

## PARTS LIST

### Resistors

R1-R3—7 × 47-ohm DIP resistor pack or discrete resistors

### Capacitors

C1—1 μF, 30 volts, tantalum  
 C2—0.1 μF, 10 volts, monolythic  
 C3, C4—27 pF, ceramic disc  
 C5—100 μF, 10 volts, electrolytic

### Semiconductors

IC1—8048 programed microcontroller  
 IC2—011273 memory decoder  
 IC3, IC4—74LS244 octal buffers  
 IC5-IC36—514256 256K × 4-bit 120 ns dynamic RAM (8 per megabyte)

### Other components

J1—8-pin male header or 4-position DIP switch

J2—48-pin male header

XTAL1—6 MHz HC-18 crystal

**Miscellaneous:** 2-inch long 48-conductor ribbon cable with a 48-pin female IDC connector on each end, 35 20-pin IC sockets with built-in 0.1 μF bypass capacitors or standard 20-pin sockets with 0.1 μF capacitors installed on the board, 1 40-pin IC socket, PC board, solder, etc..

**Note:** The following items are available from Lancelot, P.O. Box 541005, Merritt Island, Florida 32954-1Q05: a complete kit for the memory board (less memory IC's), \$99.95 plus \$5.00 P&H; a partial kit including the PC board, programed 8048, and the 011273 decoder, \$63.00 plus \$5.00 P&H. Canadian orders add \$3.00. All other countries add sufficient postage for air shipment and insurance. Florida orders add 6% state sales tax. Orders by check or money order only. For technical information and dealer inquiries call 407-454-9082.

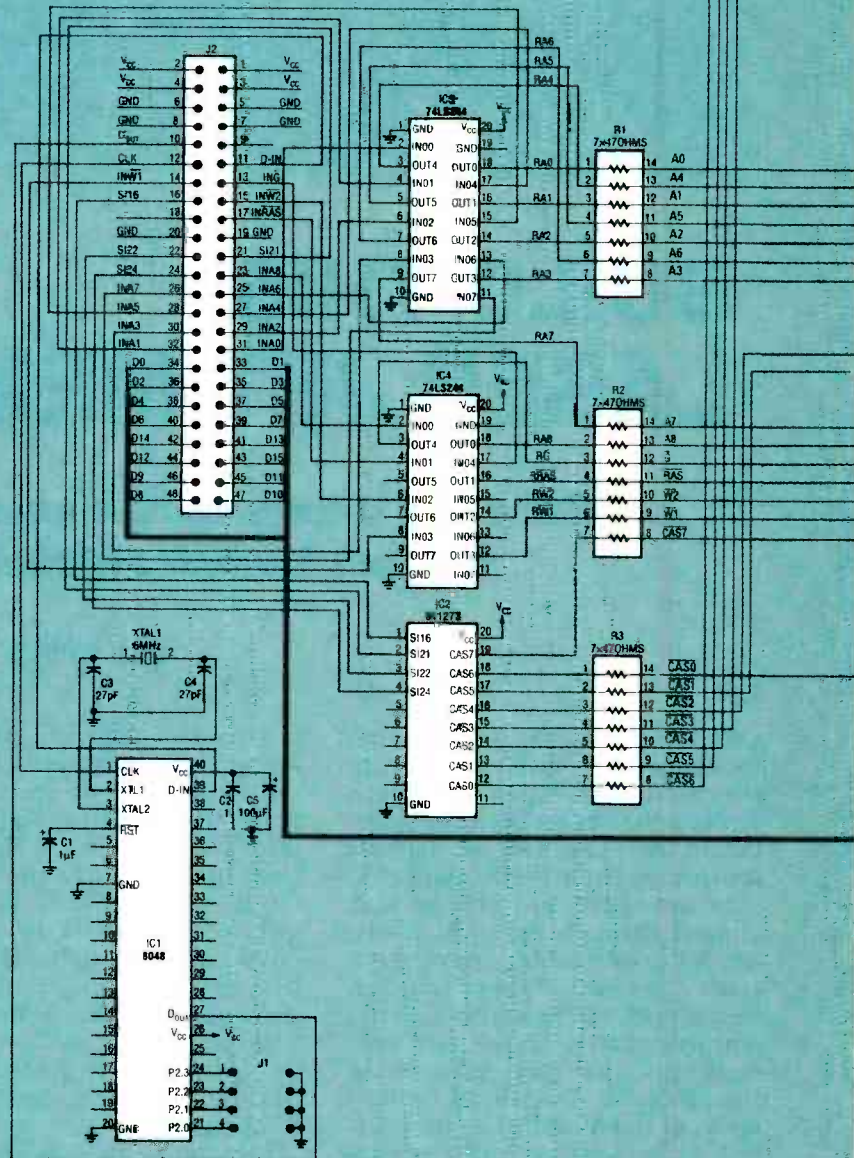
printer for less than \$325—that's megabytes without the megabucks!

### About the circuit

The circuit, shown in Fig. 1, is quite simple because dynamic RAM memory refresh and address multiplexing is done in the laser printer. The interface to the printer is through a 48-pin connector. The data bus is 16 bits (one 16-bit word) wide, and the 18-bit address bus is multiplexed into 9 bits. The remaining pins are for power, ground, memory enable, write enable, and for the controller serial communications.

The 1-megabit dynamic RAM's are organized 256K × 4 bits. They are addressed in quads by the printer as 256K 16-bit words. The four memory-enable signals from the printer are decoded by IC2 into  $\overline{\text{CAS}}$  (column-address-

*Text continued on page 75*



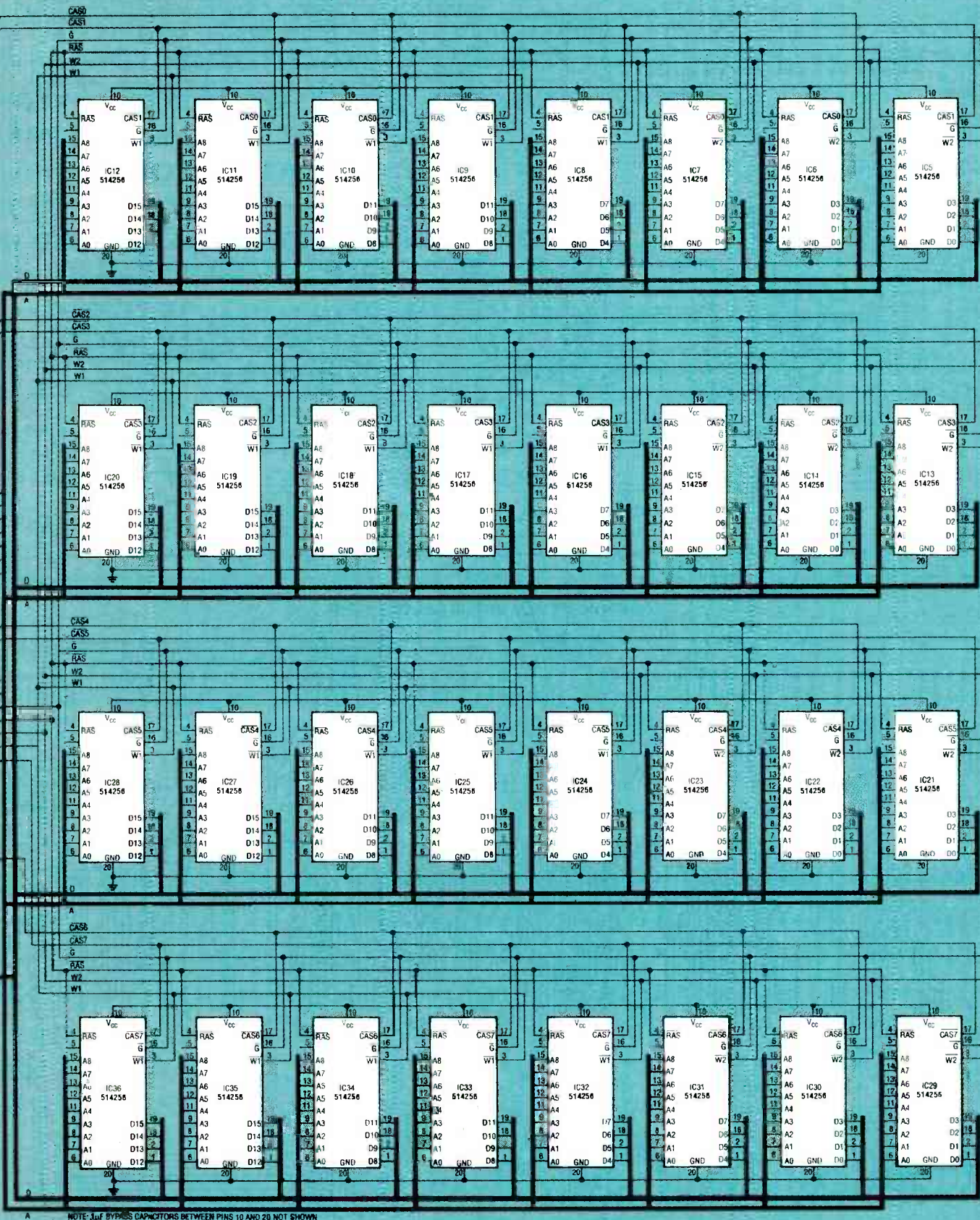
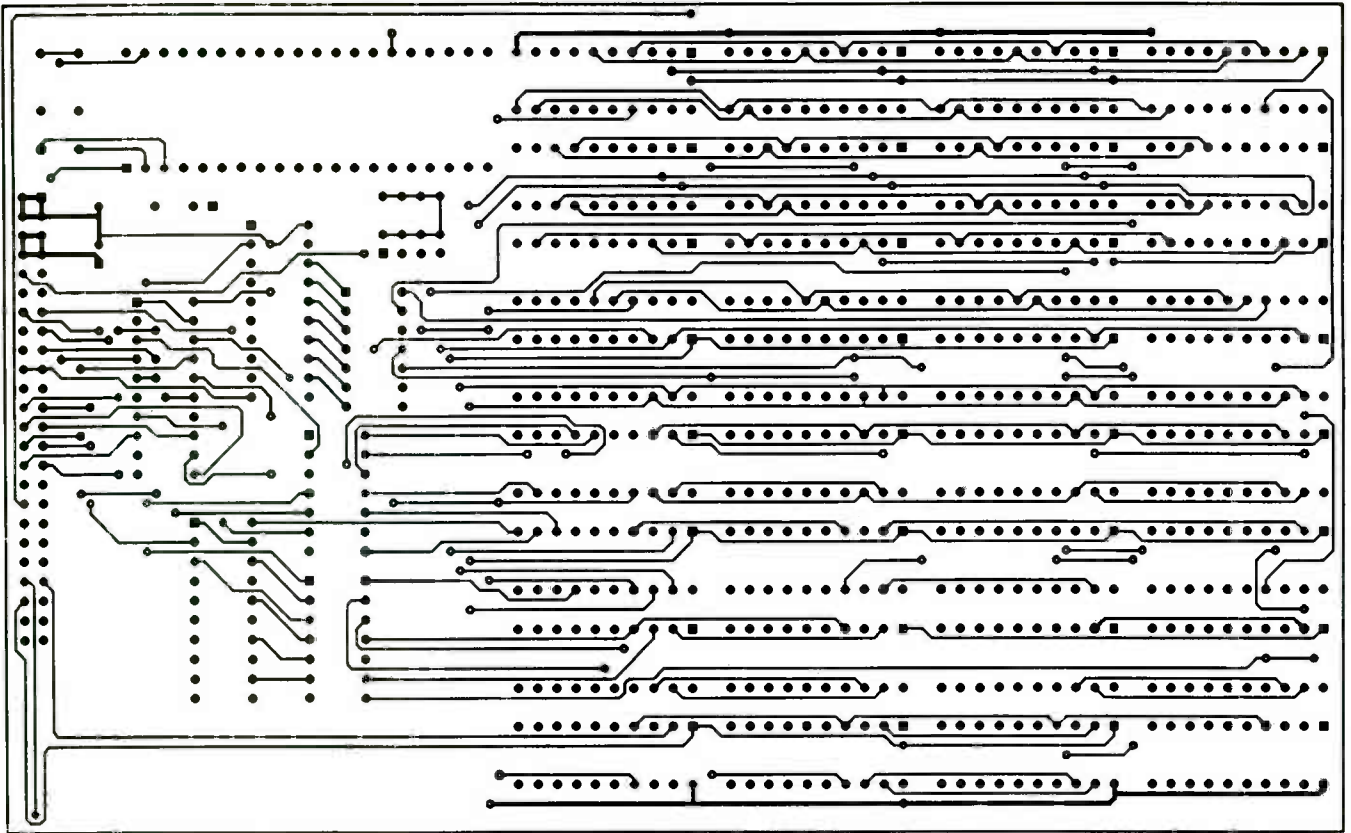
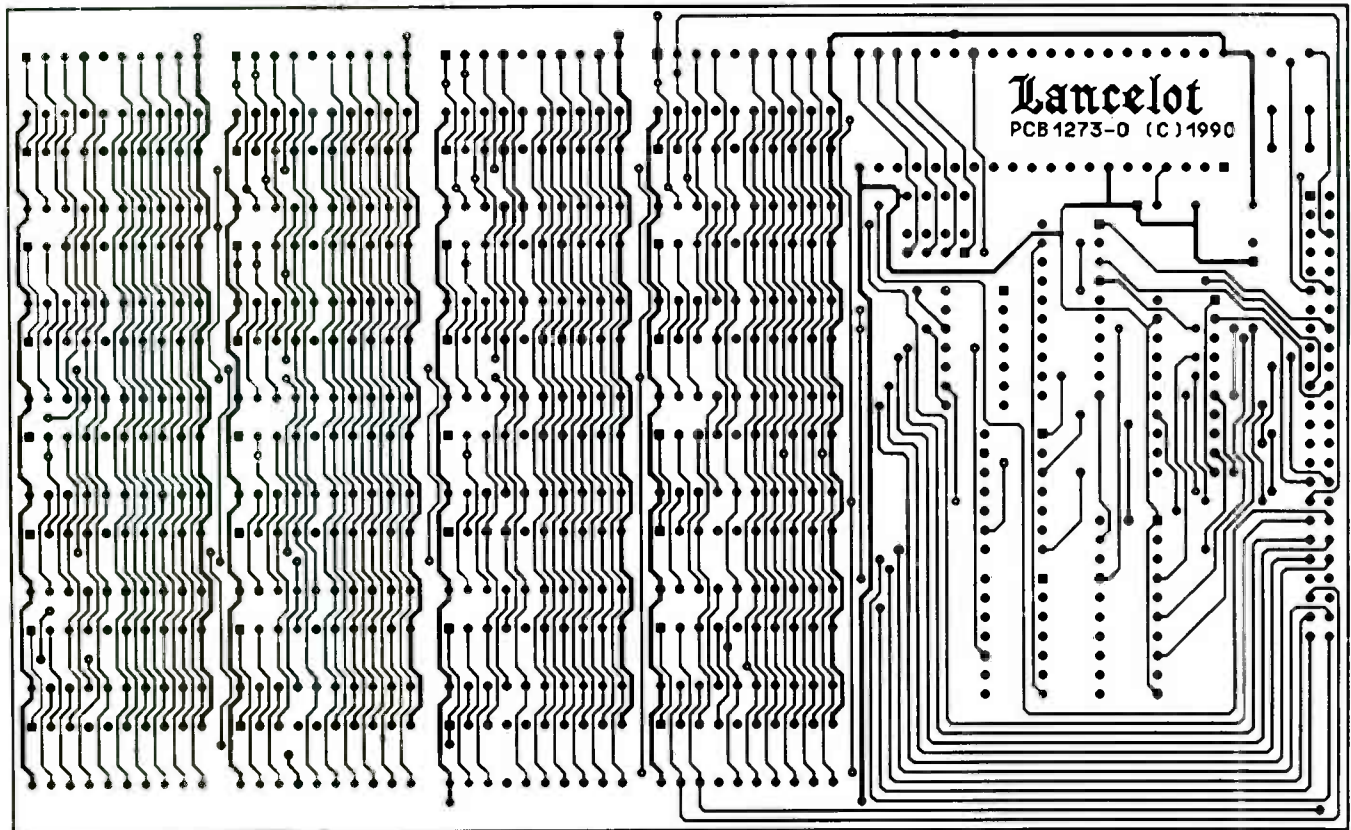


FIG. 1—THIS CIRCUIT WILL ALLOW YOU TO ADD UP TO 4 MEGABYTES OF EXTRA MEMORY TO A Hewlett Packard LaserJet III or the more expensive Model III.



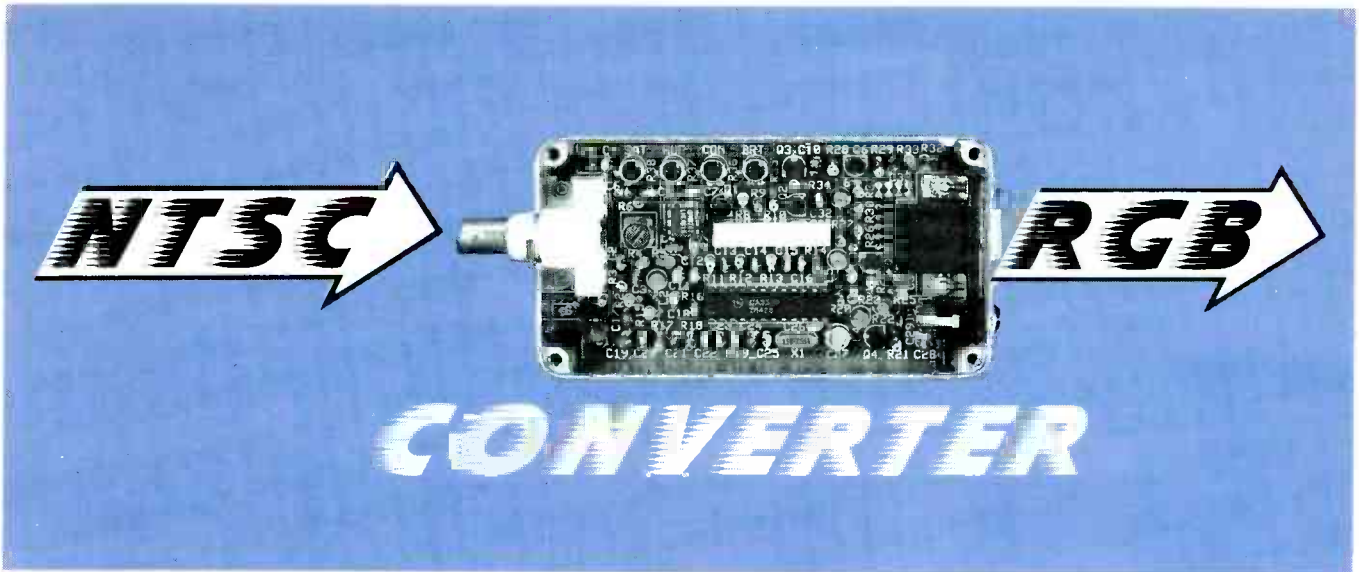
7 INCHES

COMPONENT SIDE OF THE MEMORY CARD.



7 INCHES

SOLDER SIDE OF THE MEMORY CARD.



## Put a TV in your VGA monitor.

JIM HARRIGFELD

AT BOTTOM, A TV AND A COMPUTER monitor are more alike than they are different. As a matter of fact, a monitor is really just a TV in disguise less a few circuit boards and knobs.

At one time, when computers used teletypewriters for display, television pictures were considered high-resolution. Today, even the best TV sets cannot compare with the latest breed of computer monitors in terms of resolution, stability, convergence, and fidelity. So wouldn't it be nice if you could simply connect a VCR or camcorder to your monitor and enjoy some of that extra fidelity?

This article will show you how to build a simple decoder that will take any standard NTSC video signal (from a VCR, camera, tuner, or what have you), and convert it into the analog RGB signals that computer monitors work with. The circuit costs well under \$100 to build, and requires no fancy test equipment to align. In addition, if you would like to build one, partial and complete kits are available.

### Some basics

A color monitor has a simple interface. It generally requires four separate signals to operate: red, green, blue, and sync. Sync tells the monitor where and when to start each scan line, and the RGB signals determine how much red, green, or blue to dis-

play in the picture at any instant in time.

The composite video signal used in a television is more complicated, because it combines all the RGB signals, as well as other timing information, into a single high-frequency signal. In the United States, this signal is based on the NTSC/RS-170A video standard.

The disadvantage of composite video is that a great amount of processing is required to combine and encode the separate signals into one composite signal. The advantage of composite video, of course, is that the signal may be broadcast over the air or sent down a single piece of coaxial cable. But to be displayed, eventually the signal must be broken down into its individual red, green, blue, and sync components. By contrast, the advantage of the RGB system is that no decoding circuitry is required, so circuit designs are simpler and cheaper. The disadvantage of the RGB system is that several wires and multi-pin connectors are required to make connections.

Given the similarity between a television and a monitor, what exactly is required to display NTSC video on an RGB monitor? First and foremost, we need an analog monitor that is capable of scanning at standard NTSC video rates (60 Hz vertical, 15,750 Hz horizontal). That requirement immediately eliminates most

fixed-frequency (digital) monitors—i.e., most CGA and EGA types. However, most multi-frequency type monitors work beautifully.

We also need a video source. You can choose any VCR, video camera, camcorder, or component tuner that has a video output in the NTSC/RS-170A format. Those devices usually have some kind of audio output that you can use to drive a pair of headphones or your home stereo system.

Of course, there's still one thing missing: a gadget that can be used to convert the composite video from your source device into the separate RGB signals that your monitor understands.

### About the circuit

Figure 1 shows a block diagram of the circuit, and Fig. 2 shows the complete schematic. The heart of the circuit is IC2, a TDA3330. That highly integrated Motorola IC is specifically designed to break a composite video signal down into its individual components. The TDA3330 requires three inputs to operate: chroma (color information), luminance (brightness information), and burst flag (timing information).

The other major component is IC1, an LM1881 video-sync separator made by National Semiconductor. It extracts most of the important timing information

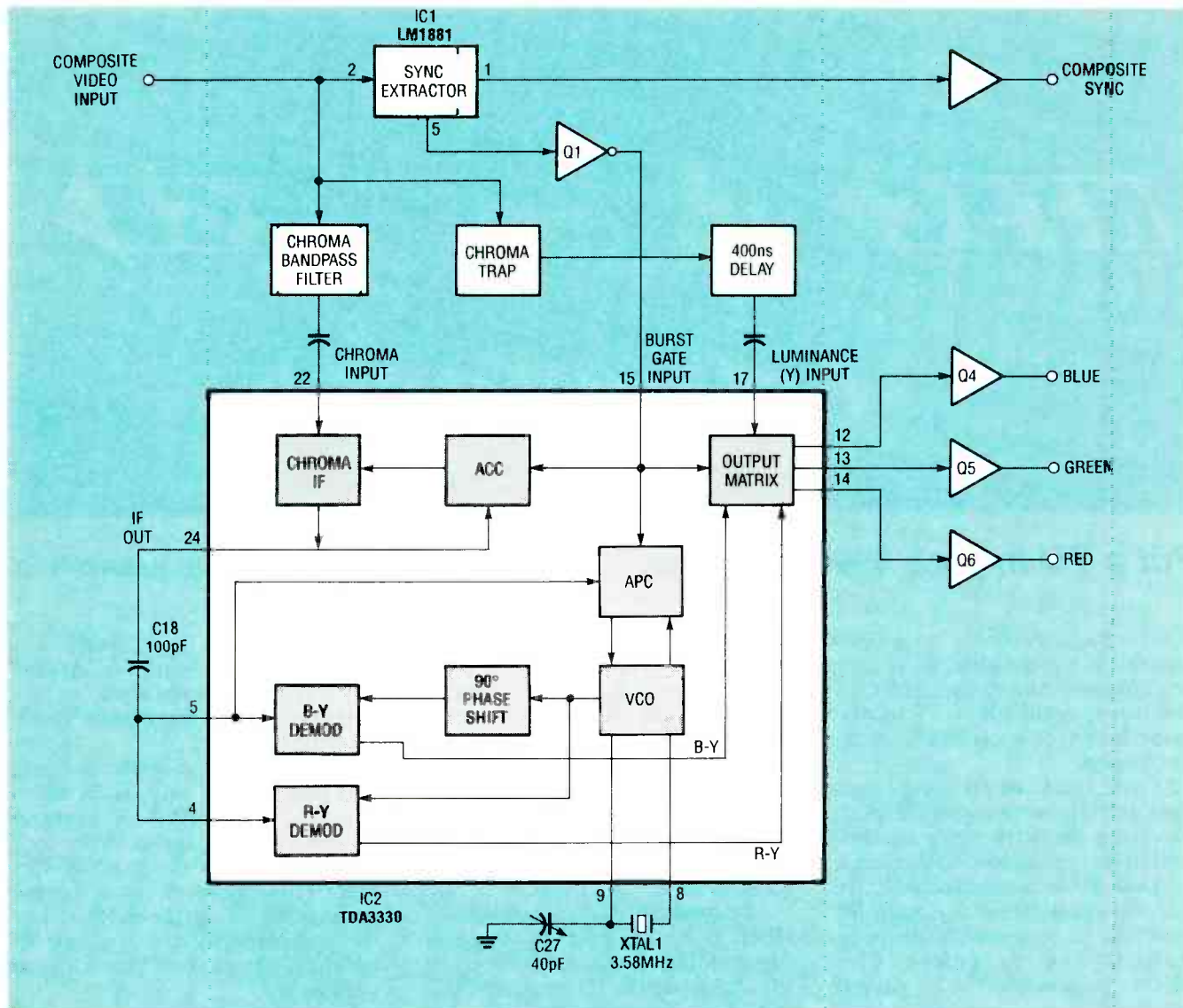


FIG. 1—BLOCK DIAGRAM. IC1 derives the sync signal and timing information. IC2 uses the latter to decode the red, green, and blue outputs.

from a standard video signal, and it needs only three external (passive) components to operate. Our circuit uses two of its three outputs: composite sync, which after buffering becomes one of our outputs; and the burst flag, which is inverted by Q1 to furnish the necessary timing information to IC2.

The other signals that are needed by IC2 are derived from the composite video input signal by means of several passive filters. The chroma bandpass filter consists of R2, L2, C11, and C12. That circuit works by allowing only 3.58-MHz signals to pass into pin 22 of IC2, while blocking all others. The luminance input (pin 17) is just the opposite, in that the 3.58-MHz component must be blocked and all other frequencies allowed to pass

through. That is accomplished with the chroma trap consisting of L1, R3, R4, C2, and C3. Basically, the output of the chroma trap is monochrome video. To meet NTSC timing requirements, that signal must also be delayed (by R5, R14, and L3) before entering IC2.

With proper input signals, IC2 requires only a few more passive components to enable it to lock on to the incoming signals. Once locked, the IC performs all I/Q demodulation, quadrature decoding, R-Y, and B-Y processing, and it then delivers red, green, and blue signals at pins 14, 13, and 12, respectively. Those signals are buffered in turn by Q4, Q5, and Q6, which are set up as emitter followers designed to drive 75-ohm loads.

The circuit has four controls

for setting operational characteristics. The brightness control (R35) sets the black level of the RGB outputs; for most applications, it should be set at minimum. The three other controls (hue, R37; saturation, R38; and contrast, R36) work much like their counterparts on a standard TV. After they have been properly adjusted, none of those controls should require operator intervention. The brightness control shifts the black level without affecting the overall peak-to-peak amplitude of the signal. On the other hand, the contrast control varies the peak-to-peak amplitude without affecting the black level.

Figure 3 shows several waveforms and timing relationships for a color-bar input signal at several points in the circuit: (a) The

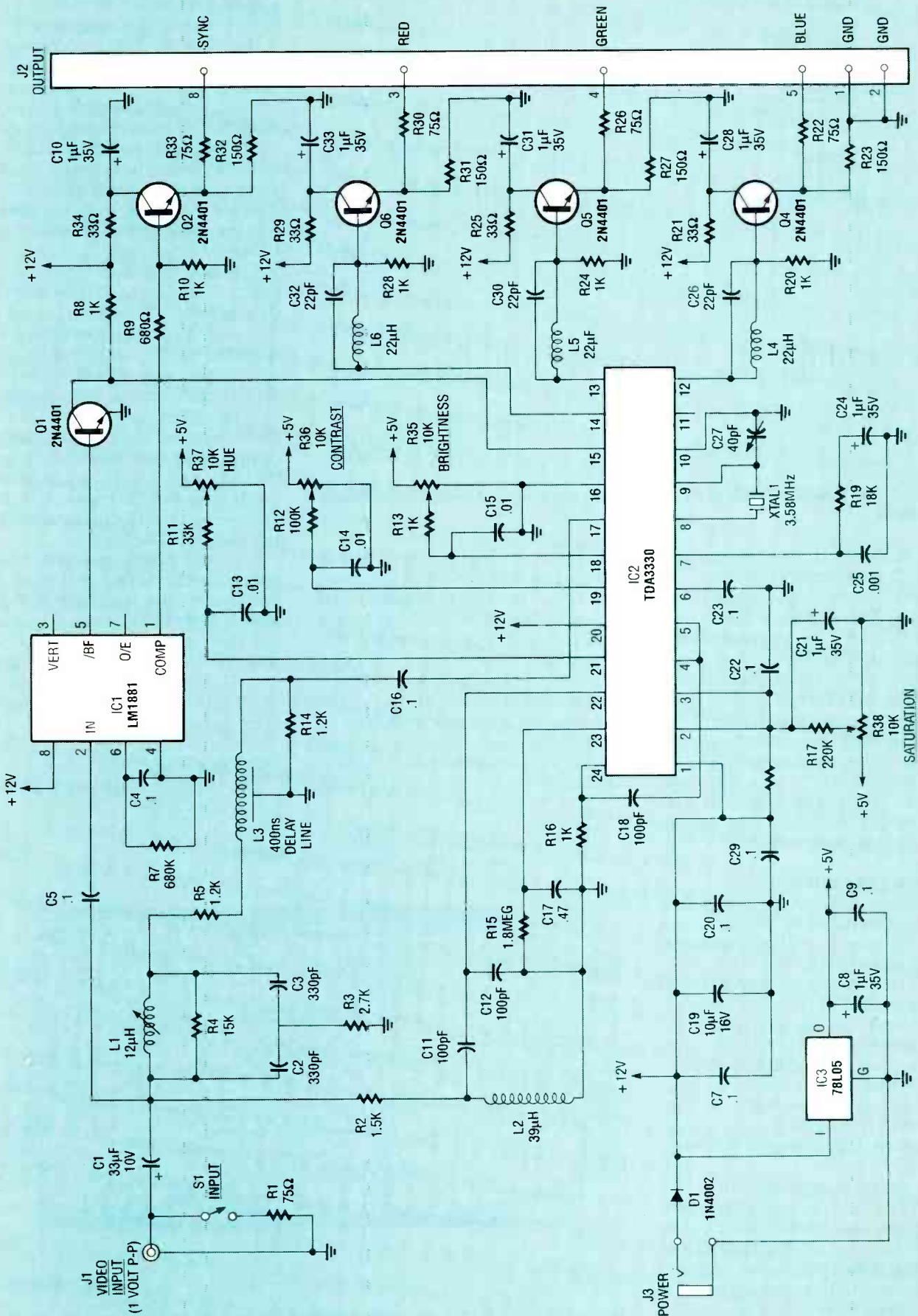


FIG. 2—COMPLETE SCHEMATIC. The circuit accepts a 1-volt peak-to-peak composite input, and delivers RGB and sync outputs, also with a swing of 1 volt peak-to-peak.

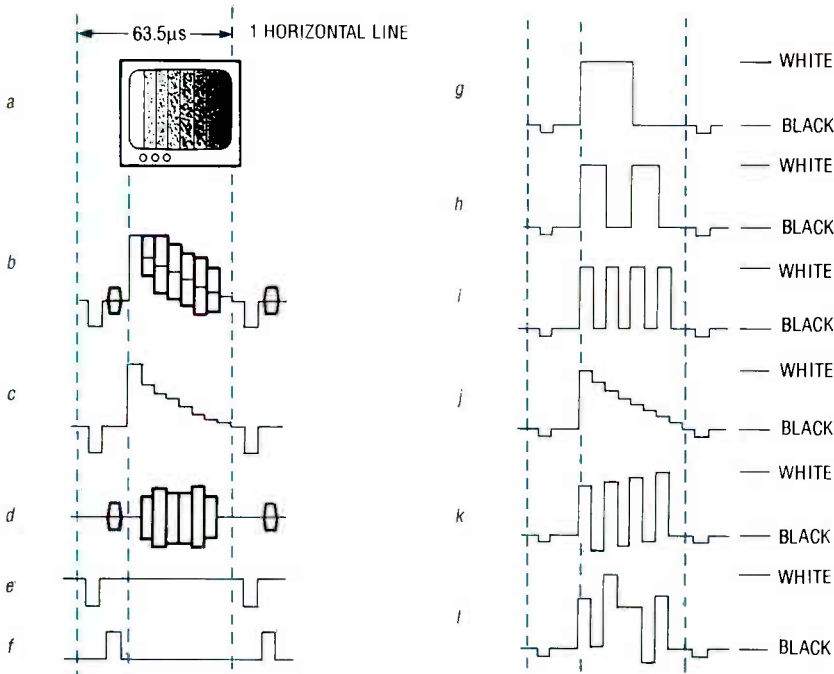


FIG. 3—SAMPLE WAVEFORMS. At (a) is a color-bar input; the text describes the remaining signals.

color-bar input. (b) Composite video across one scan line. (c) The luminance input (pin 17) of IC2. (d) The chroma input (pin 22) of IC2. (e) The composite sync output. (f) The burst-flag input (pin 15) of IC2. (g) The green output (Q5). (h) The red output (Q6). (i) The blue output (Q4). (j) All outputs with the saturation control (R38) at minimum. (k) The blue output with the saturation control (R38) too high. (l) The blue output with the hue control (R37) improperly adjusted.

### Building the circuit

With the high frequencies that are involved, stray capacitance and crosstalk will almost certainly cause problems with most breadboarding and wirewrap techniques. Therefore, we recommend that you use a PC board for the project. Patterns for the board are provided if you wish to make your own; boards are also available commercially, as discussed in the parts list. If you use our board, Fig. 4 shows the parts layout.

All parts except possibly IC2 (the TDA3330) are readily available from the mail-order houses advertising in **Radio-Electronics**. If you purchase a partial kit, be careful in selecting capacitors. Only tantalum or monolithic DIP types are suitable, as

electrolytic, Mylar, or ceramic disc types may not fit in the allotted space on the printed circuit board. Also note that resistors and inductors are mounted vertically. Bend one of the leads back parallel to the body of the part and mount the body of the part in the hole with the circle around it, and then pass the bent lead through the other hole. Mount the inductors (except L3) in the

same manner. This method saves space and also furnishes you with good debug/test points.

We also strongly recommend the use of IC sockets. If you are unable to locate a 24-pin socket for IC2, you can use 16- and 8-pin sockets mounted end-to-end. The pads around the trimmer potentiometers have been laid out so that several types of trimmers may be installed. Just be sure to mount the trimmer's wiper arm in the correct pad.

The board was designed to accept PC-mounted connectors for J1 (input), J2 (output), and J3 (power). However, you may not want or need these types. Our prototype uses a BNC connector for J1, but a simple RCA jack may suffice. Likewise, J2 and J3 may be eliminated entirely or changed depending on what your particular application involves. Switch S1 may be replaced with a simple jumper/header combination for most setups.

For best operation, the board should be installed in a shielded enclosure. The template in Fig. 5 shows hole locations for mounting the board in the project box that is mentioned in the parts list. The board is held in place in the box by the connector hardware (J1–J3).

### Hooking it up

Regardless of the type of con-

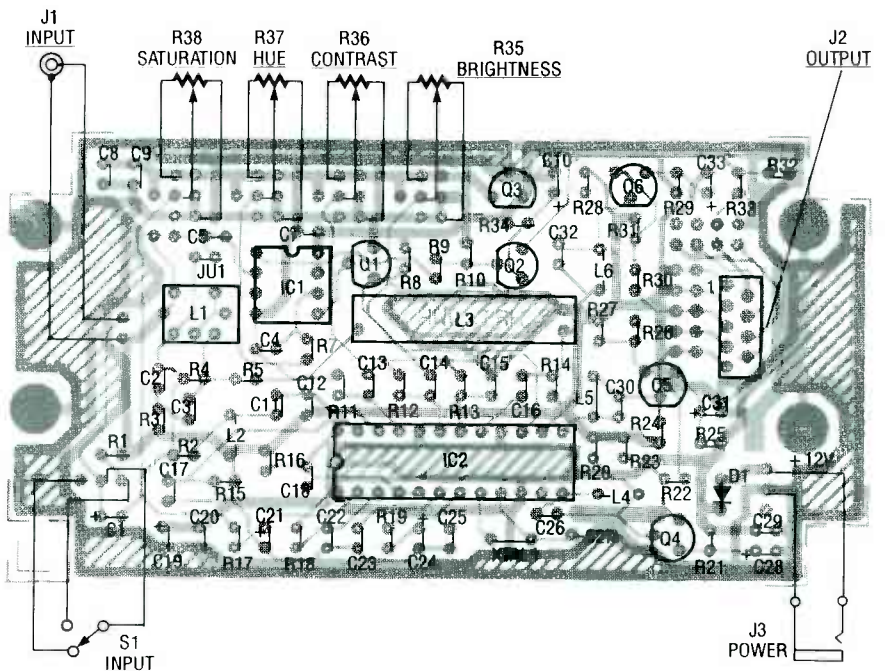
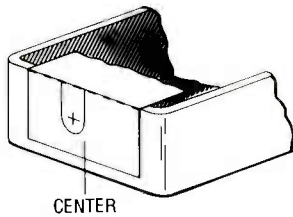


FIG. 4—PARTS LAYOUT. All parts, including the variable resistors and the I/O jacks, mount on the board.





-FOLD ALONG DOTTED LINE  
 -ALIGN FOLD ON TOP OF BOX  
 AND CENTER - TAPE ON  
 -PUNCH CENTERS

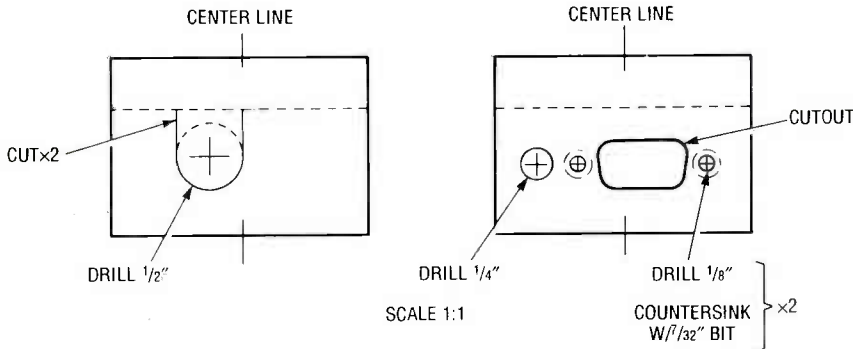


FIG. 5—DRILLING TEMPLATE. If you use our board and the box mentioned in the parts list, drill the box as shown here.

### PARTS LIST

All resistors are 1/4-watt, 5%, unless otherwise noted.

- R1, R22, R26, R30, R33—75 ohms
- R2—1500 ohms
- R3—2700 ohms
- R4—15,000 ohms
- R5, R14—1200 ohms
- R6—not used
- R7—680,000 ohms
- R8, R10, R13, R16, R20, R24, R28—1000 ohms
- R9—680 ohms
- R11, R18—33,000 ohms
- R12—100,000 ohms
- R15—1.8 megohms
- R17—220,000 ohms
- R19—18,000 ohms
- R21, R25, R29, R34—33 ohms
- R23, R27, R31, R32—150 ohms
- R35—R38—10,000 ohms, cermet potentiometer, Panasonic #SOGA01B1

#### Capacitors

- C1—33  $\mu$ F, 10 volts, tantalum
- C2, C3—330 pf, 50 volts, monolithic
- C4, C5, C7, C9, C16, C20, C22, C23, C29—0.1  $\mu$ F, 50 volts, monolithic
- C6—not used
- C8, C10, C21, C24, C28, C31, C33—1  $\mu$ F, 35 volts, tantalum
- C11, C12, C18—100 pF, 50 volts, monolithic
- C13—C15—0.01  $\mu$ F, 50 volts, monolithic
- C17—0.47  $\mu$ F, 50 volts, monolithic
- C19—10  $\mu$ F, 16 volts, tantalum
- C25—0.001  $\mu$ F, 50 volts, monolithic
- C26, C30, C32—22 pf, 50 volts, monolithic
- C27—5–30 pF, trimmer

#### Semiconductors

- IC1—LM1881N video sync separator (National)
- IC2—TDA3330 NTSC to RGB decoder (Motorola)
- IC3—78L05 low-power 5-volt regulator
- Q1, Q2, Q4—Q6—2N4401
- Q3—not used
- D1—1N4002 rectifier diode

#### Other components

- J1—PC-mount BNC connector (AMP #226978-1)
- J2—9-pin D connector, female, PC mount
- J3—3.5mm mono phone jack
- L1—12  $\mu$ H variable inductor (Toko #A119ANS-T1034)
- L2—47  $\mu$ H fixed inductor (Toko #348LS-470K)
- L3—400 ns delay line (Toko #H321LNP-1436P)
- L4—L6—22  $\mu$ H fixed inductor (Toko #348LS-220K)
- S1—SPST, PC board right-angle mount
- XTAL1—3.579-MHz crystal
- Miscellaneous: Metal case—(Hammond #1590B), 12-volt regulated wall transformer, solder, etc..

**Note:** The following items are available from Harmonic Research, Inc., 193 Villanova Drive, Paramus, NJ 07652 (201) 652-3277: Complete kit including PC board and all parts except wall transformer, \$95.95; Partial kit including all parts except box, S1 and J1, \$81.50; Etched, drilled, and silk-screened PC board, \$20; TDA3330 (IC2), \$4.75. All orders add \$2.50 for shipping and handling. New Jersey residents add appropriate sales tax.

nectors that you use, the input should be wired using high-quality coaxial cable for best results. Your VCR or camera may have come from the factory with a cable of this type. Otherwise you can buy or build an input cable with RG59U coax and either BNC or RCA connectors.

The output cable depends on your application and use. Refer to your monitor's manual to determine its input wiring requirements. The decoder's output (J3) is a DB-9 connector that conforms to the PC standard. Many multi-frequency monitors adhere to that standard; but it's a good idea to check the manual just to be sure. With a little luck, you should be able to unplug the cable from the display adapter in your PC and plug it directly into the decoder.

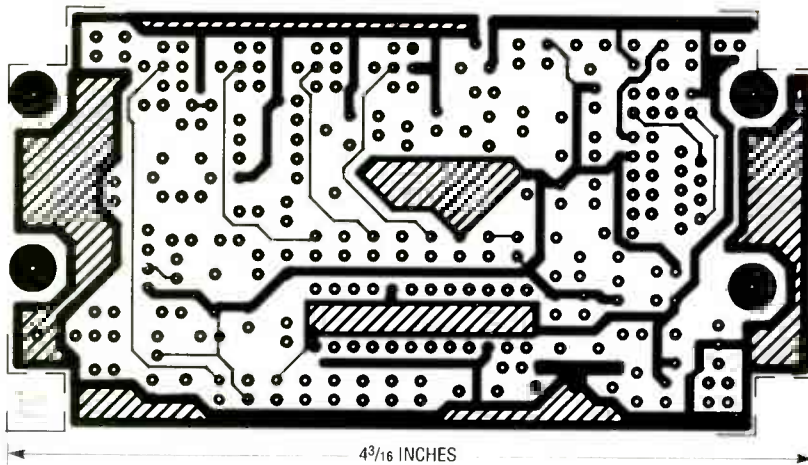
If you're not so lucky, you'll have to wire up a cable or an adapter. In addition, we left a row of pads just behind J2 on the PC board; you might find it easier to simply cut the traces between the two rows and add jumpers to reconfigure the pinout of J2. That could save you from having to modify a cable.

The power supply for the NTSC converter can be any well-regulated 12-volt supply that is capable of furnishing 250 mA of current on a continuous basis. Apply power to J3 through a 1/8" phono plug with positive tip and grounded shield.

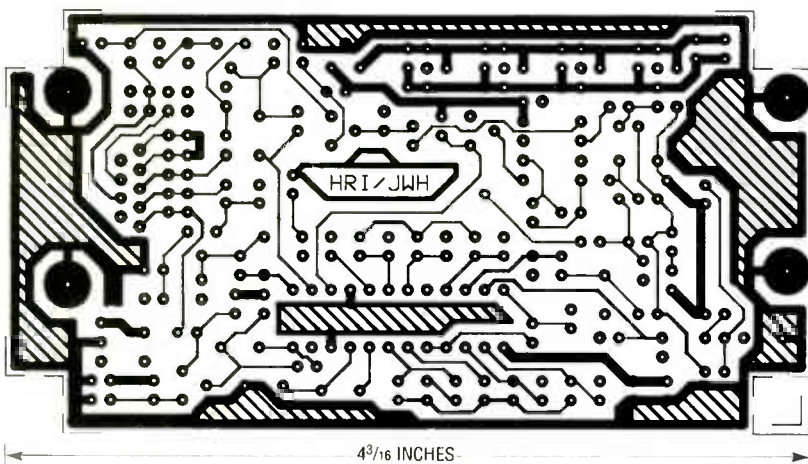
#### Testing and adjustment

Before applying power, check the PC board for solder splashes, bad or shorted connections, etc.. Do not install the IC's in their sockets yet; rather, first apply power to the circuit and check for smoke and overheated components. Using a DMM, verify that pins 1 and 20 of IC2, and pin 8 of IC1, are all about +12 volts. In addition, verify that the positive side of C8 is +5 volts.

After everything checks out, remove power from the board, install the IC's in their sockets, and make the external connections. A color-bar generator is nice for making the adjustments, but if you don't have access to one, any stable video signal will do. Use a camera or an off-the-air signal; don't try to set up from a tape. Turn the saturation, hue, and



HERE'S THE COMPONENT SIDE OF THE NTSC/RGB CONVERTER



HERE'S THE SOLDER SIDE OF THE NTSC/RGB CONVERTER.

contrast controls (R36–R38) to maximum, and the brightness control (R35) to minimum.

**Adjusting without test equipment.** With everything hooked up and the monitor on, plug in the power supply. You should immediately see some kind of picture, although it will probably be black and white and possibly flashing on and off. Adjust C27 with a small screwdriver for the most stable picture and the best color. You may find two spots where performance seems equal; either will do. Next, adjust L1 for the deepest, richest color. Then adjust the saturation, hue, and contrast controls for the most natural look, just as you would on a normal television. You should leave the brightness control set at minimum unless you have a specific reason for wanting the black level set higher than it already is. That's all it takes to adjust the unit, and you will probably be very close to the optimum settings.

### Adjustment with color-bar generator and oscilloscope.

With S1 closed, verify with the scope that you have a 1-volt peak-to-peak signal similar to that shown in Fig. 3-a at the input connector. Next, verify that a burst-flag pulse is present at pin 15 of IC2. That signal should look like the waveform shown in Fig. 3-f, and must be at least eight

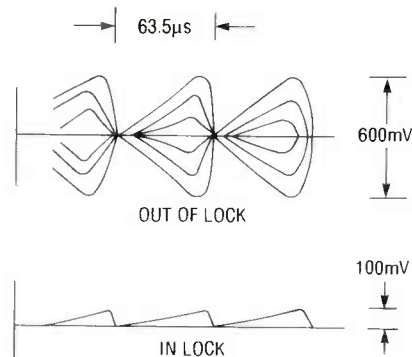


FIG. 6—VCO LOCK AT PIN 7 OF IC2. In (a) is an incorrectly adjusted signal; (b) shows the correct waveshape.

volts in amplitude. Also, verify that you have a chroma signal similar to that shown in Fig. 3-d at pin 22 of IC2. If you examine pin 17 with a scope, it will probably resemble something halfway between Fig. 3-b and Fig. 3-c. Adjust L1 for minimum subcarrier by making the signal look like in Fig. 3-c as much as possible.

Continue adjustments by connecting the scope probe to pin 7 of IC2 and referring to Fig. 6. An out-of-lock waveform is shown in Fig. 6-a; adjust C1 until you obtain a stable waveform as shown in Fig. 6-b. There will probably be two spots in the adjustment range where lock occurs; either is OK. That signal is the VCO lock, and once set, you should be able to see nice, stable signals at the RGB outputs (pins 12–14 of IC2). Refer to the output waveforms in Fig. 3 and watch your monitor while adjusting the saturation, hue, and contrast controls to your liking. Outputs should be set anywhere from 0.7 to 1.0 volt peak-to-peak.

### I want my MTV/2!

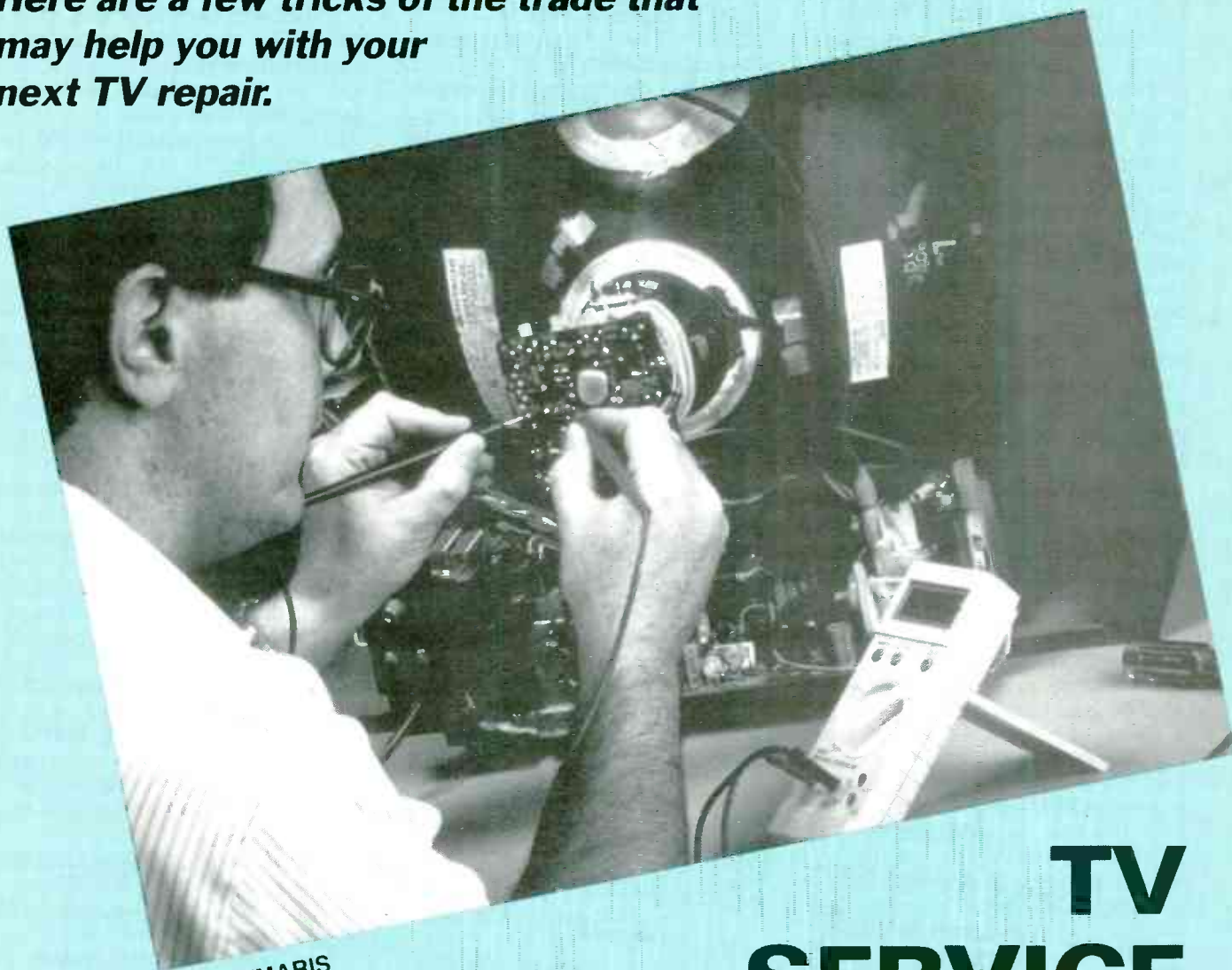
After making all of the adjustments to the unit itself, leave them alone; instead use the brightness and contrast controls on your monitor to compensate for ambient lighting. The decoder should be able to lock on to anything that comes anywhere close to NTSC video, but it can't deal with some of the copy-protection schemes that many pre-recorded tapes use. However, you may be able to compensate by running the composite video signal through a descrambler or stabilizer first.

You may notice that some video looks better on your monitor than on a TV, whereas other video looks worse. The reason is that a high-resolution display cannot improve a low-resolution input, and in some cases the high resolution might even bring out some unwanted artifact that a low-resolution display would cover up.

Some day, with all the hoopla over HDTV and multimedia, video and graphics displays will most likely merge. We will be running our CAD program on the same screen that we sit back and watch STAR WARS 15 on. Until then, projects like this will inch us a little closer.

R-E

**Here are a few tricks of the trade that may help you with your next TV repair.**



CLEO ZYMARIS

# TV SERVICE CASE HISTORIES

TV SERVICING CAN BE A PRECARIOUS business, but with a little intuition—and a firm background in TV repair fundamentals—your job can be made easier. We'll discuss a few examples of some common problems a service technician might come across, and how that intuition and background can lead to a solution.

## **An AFT problem**

Many TV repairs are fairly obvious examples of cause-and-effect; sometimes the cause is created by the customer! A customer came into the shop with a Samsung model CT-510AL, complaining that several channels

were distorted, with unsynchronized video and an annoying audio buzz. Luckily, raster, sound, and video were present. Those symptoms indicated a tuning problem, perhaps a malfunction of the fine tuning circuit or simply a misadjustment. The receiver had a preset button that set the tint, contrast and color. In addition, another button energized the automatic fine tuning (AFT) circuit. The customer was probably unaware that he misadjusted the preset and AFT buttons.

If the fine-tuning control was adjusted with the AFT activated, no change would occur in the pic-

ture until the frequency was so far from its correct value that the AFT lost control and the set tuned off-channel. A common characteristic of an AFT circuit is that the hold-in range is greater than the pull-in range. A fine tuning adjustment, with the AFT on, would initially produce no change to the picture because of the hold-in characteristic. If the channel was changed, however, and then returned to the original channel, the picture might be completely detuned because the pull-in capability had been exceeded. In the case of the Samsung model, that was indeed what happened.

The customer wanted to modify the tint to his liking. Because the preset button had been energized, the set controls were inoperative. With the AFT activated, he proceeded to rotate the only control available to him (other than volume) which was the fine tuning. As each channel was detuned he proceeded to the next. The icing on the cake was his fiddling around with a few control shafts on the back of the set.

The repair was obvious. First, I disabled the AFT, then each channel was adjusted properly for good color. The automatic gain control (AGC) was adjusted for minimum snow and no overload on any channel. I touched up the vertical controls that had been disturbed and sprayed clean the front panel controls that were acting erratic. Finally, the preset color, tint, and contrast controls were adjusted for good flesh tones. I ran the set for a few hours to make sure there was no front end drift.

When the set was picked up, the owner was instructed to adjust the fine tuning *only* with the preset button de-energized. Do you think he remembered?

Since we are on the subject of AFT, let's look a little deeper into its operation. All AFT circuits are basically limiter-discriminators. The discriminator is tuned to the video intermediate frequency (IF) at 45.75 MHz. If the set is tuned properly, the discriminator will produce zero volts with respect to a reference. Tuning too high or too low produces a more positive or more negative output from the discriminator. It should be noted that the polarity depends on circuit wiring and the maximum amplitude depends on the tuned

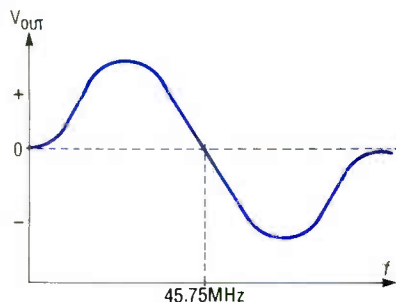


FIG. 1—DISCRIMINATOR OUTPUT TUNED to video IF at 45.75 MHz and zero volts with respect to reference.

circuit bandpass, circuit gain, and saturation level.

Figure 1 shows the discriminator curve with an IF of 45.75 MHz. The discriminator output is routed to a varactor, or a transistor acting like a varactor, in the local oscillator (LO) tuning circuit. With proper polarities chosen, any detuning of the set would result in an error signal from the AFT circuit that would change the varactor's capacitance to properly tune the LO.

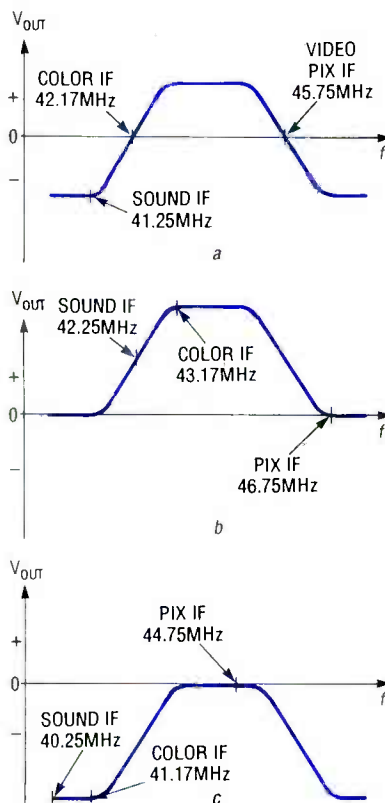


FIG. 2—INTERMEDIATE FREQUENCY RESPONSE as the local oscillator (LO) frequency is varied; (a) is the LO properly tuned, (b) is the LO tuned high and (c) is the LO tuned low.

Figure 2 shows the IF response as the LO frequency varies. For proper tuning, the video IF carrier at 45.75 MHz and the color subcarrier at 42.17 MHz (45.75 MHz minus 3.58 MHz) should appear at the proper amplitude points on the IF response curve. Figure 2-a is a graph of amplitude versus frequency of a correctly tuned LO. In this receiver, the video IF carrier and color subcarrier frequencies are located at 50% of the mid-range amplitude. In addition, the sound carrier, which operates at 41.25 MHz, is

located at a low amplitude point.

If the local oscillator was tuned too high, the color subcarrier and the sound carrier would both increase in amplitude, as shown in Fig. 2-b. That would result in a 920-kHz beat which would be very noticeable on the screen. Figure 2-c shows the LO tuned too low—the amplitude of the color subcarrier is reduced, resulting in a loss of color.

The Samsung model discussed here used an IC to perform the AFT function. Figure 3 shows that portion of the circuit. An IF sample is fed to pin 11 of the IC, a TA7070. The IF is amplified and the level stabilized by the first section of the IC and is output to pin 4. The amplified IF is passed through a discriminator transformer tuned to the video carrier at 45.75 MHz. The transformer feeds into pins 3 and 5 of the IC, where differential DC voltages are produced that are proportional to the tuning error. The DC differential voltages are amplified and appear as differential outputs on pins 7 and 8. Variable resistor VR158 sets the quiescent level, and a single ended output from pin 8 is finally routed to the tuner's varactor.

It is interesting to note that the AFT circuit adds to, or subtracts from the varactor bias, which is always reverse-, and never forward-biased. Another aspect of the AFT circuit is that the operating voltages for the IC's are stabilized by an internal shunt regulator, in conjunction with an external dropping resistor R173.

### An orphan TV

When a set comes into the shop for repair, it's comforting to go to the file cabinet and pull out its service information. Even before getting too deeply involved in the problem at hand, it can be helpful to identify major components and controls from the layout drawing. Take a look at the schematic and try to spot some clues for the repair. Is the power supply connected directly to the line? What form of voltage regulation is being used? How are the major components accessible? Are there plug-in modules?

The owner of a Supre-Macy model 20MK came into the shop with a complaint of no operation. I had no Supre-Macy service in-

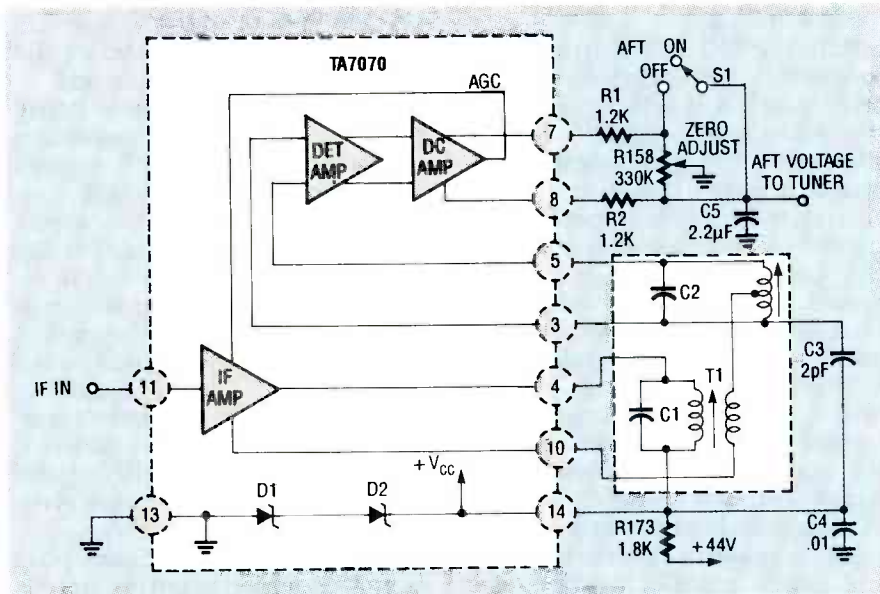


FIG. 3—THE AUTOMATIC FINE TUNING (AFT) IC and associated circuitry. The discriminator transformer is tuned to the video carrier at 45.75 MHz.

formation on file. *Sams Photofacts* index, the serviceman's bible, was of no help either. Macy's was a local department store and that was their private label. I was sure that by contacting the store, I would eventually find a source for service information. For the time being, however, this was an orphan TV. Here's how I attempted to repair the set without the security of a schematic to fall back on.

The back was removed and revealed a neat printed circuit board onto which several modules were plugged. The main board had a fuse wired directly on the PCB, with a smoky look indicating a blown fuse. Tracing a few lands on the bottom of the board showed the fuse in series with the AC line. A single rectifier and 200 volt filter capacitor indicated half-wave rectification.

The back of the set conveniently identified the modules in English and French. On the regulator/audio module, a TO-3 transistor Q1 and a TO-220 transistor Q3 were mounted on heat sinks. The module was unplugged and some lands were traced. The collector of Q1 was connected to the unregulated B+ source, shown in Fig. 4. The base was connected to a small plastic transistor Q2 with the emitter wired on the board. That was the regulator section. A little more tracing showed that Q3 operated as a single ended or class-A audio output amplifier, in conjunction

with a main board transformer. The three transistors were checked for shorts with an ohmmeter and found to be normal.

The regulator/audio module was plugged in and a few continuity measurements were made to check for AC or DC short circuits. The load side of the blown AC fuse showed a resistance of approximately 350 ohms with reference to ground—a little low, but not a short. Disconnecting the degaussing coil increased that value to a more reasonable value in the range of tens of kilohms. Of course! The degaussing coil was in series with a thermal resistor, as it heated up its resistance increased, degaussing only on turn-on. Those measurements were made with a cold re-

sistor. Continuity measurements with respect to ground were made at the cathode of the rectifier diode, and at the collector of the horizontal output transistor. No shorts were revealed.

Access into the set was difficult, so I decided to make life easier by mounting the fuse onto a stiff fuseholder on the PCB. Fuse replacement would be much quicker using a clip-type fuseholder.

The set was connected to a Variac and an isolation transformer. I adjusted the variac to produce a low value of about 30 volts DC at the rectifier cathode. The presence of B+ voltages were checked at the regulator output, the audio output transistor, and at the horizontal output transistor. I carefully increased the voltage gradually until audio noise was heard. The set seemed ready to work. The aroma of burning plastic was becoming noticeable and a wisp of smoke was seen coming from the PCB attached to the CRT socket. Shut off the power!

Inspection of the PCB showed charring around the connector pins leading off the board, which indicated a dielectric breakdown between the PCB land patterns. Unplugging the connector showed burning between pins 3 and 4. Pin 4 had continuity to ground, pin 3 was on the high side of the screen control.

Typically, a set with an in-line CRT has a circuit similar to that shown in Figure 5, where the connector details have been added. The high side of the screen

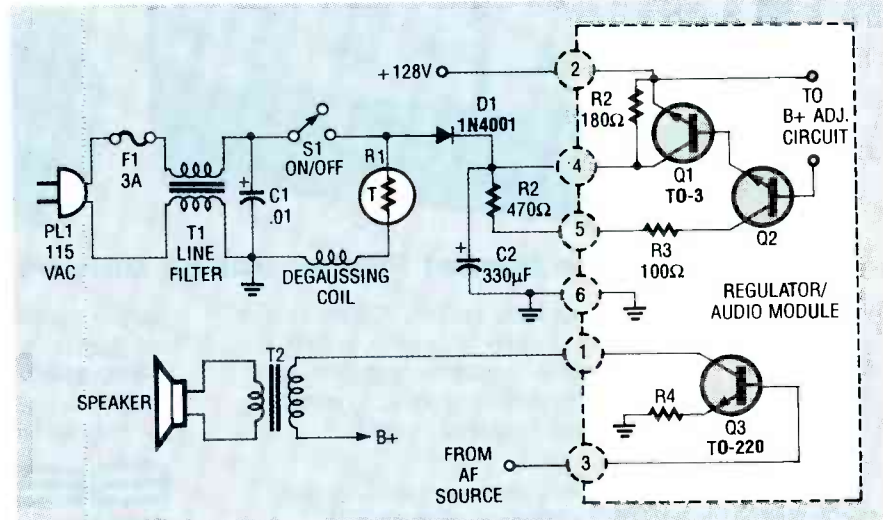


FIG. 4—POWER SUPPLY CIRCUIT.

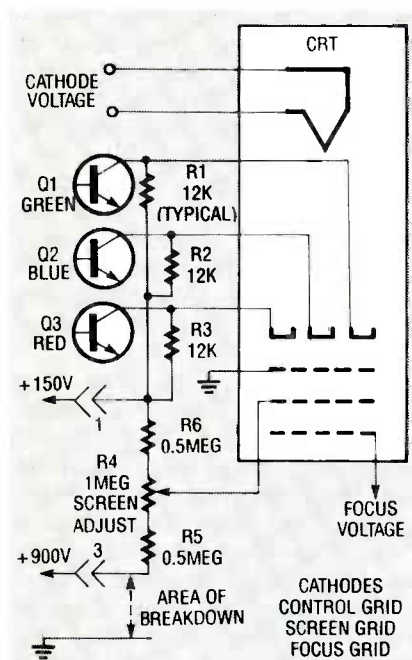


FIG. 5—CRT CIRCUIT SHOWING connector details.

control usually operates at about eight or nine hundred volts, derived from either a B+ boost circuit or from a tap-off in the focus circuit. It is important to determine the presence of the screen

control voltage.

With the CRT PC board still disconnected, the variac was set to produce a low B+ value. Pin 3 of the charred connector was checked with a voltmeter and showed over 100 volts. The source was still operating. I turned off the power, unsoldered the connector pins from the board, and cut the connector plug from the cable leading to the main board. The wires were individually soldered to the CRT PC board without the benefit of a connector. Then, the area where the connector was located was cleaned of soot using a solvent.

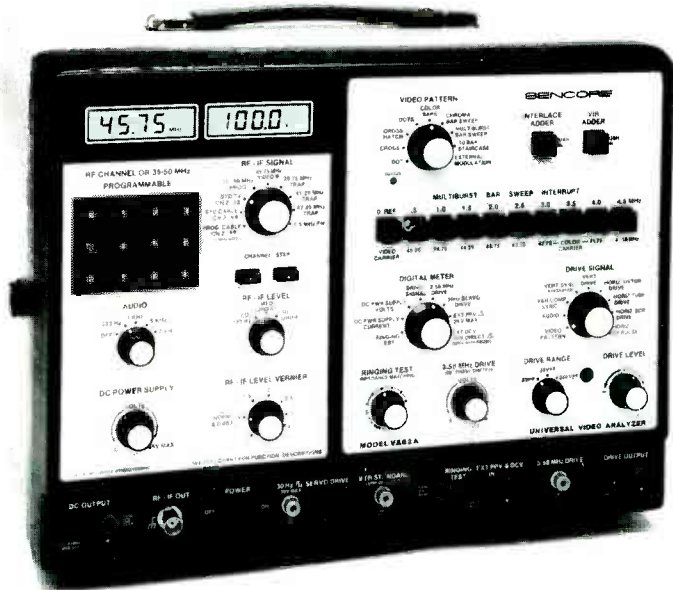
I slowly applied power by gradually increasing the variac setting, while monitoring the regulator emitter and observing the CRT PCB. Soon sound was heard and a picture was visible. The input voltage was increased until 110 volts AC was applied. The regulator's output leveled off at +128 volts and there was no evidence of breakdown at the repaired PCB. I cleaned up the controls and adjusted the fine tuning for each channel, with the

AFC off. I removed the Variac and isolation transformer and let the set run for the rest of the day.

That was an example of being able to make a repair without any service information. TV repairs depend on the knowledge that modern day TV circuitry has evolved into a predictable configuration in the CRT area. It requires the patience to trace lands in order to determine the type of circuit used in the critical power supply and CRT areas. Servicing TV sets without adequate information is not recommended. But, when you're fighting the clock and a wisp of smoke gives you a clue, it's worth a try.

The type of breakdown phenomenon which occurred here is not unusual. A dielectric breakdown can occur on terminal boards, between PCB land patterns, as it did in this case, or between adjacent connector pins.

A postscript—further inquiry uncovered that the manufacturer of the Supre-Macy model was Technika, which is listed in *Sams Photofacts*. R-E



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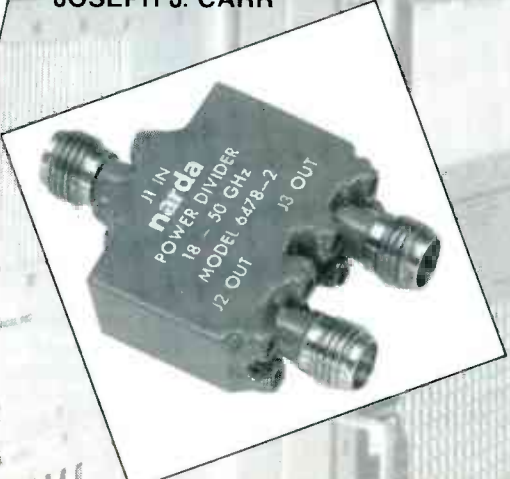
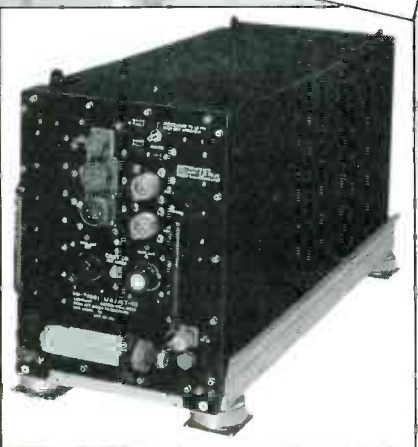
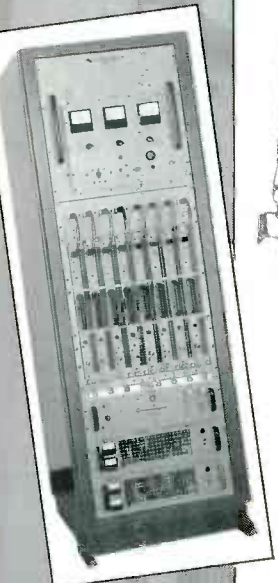
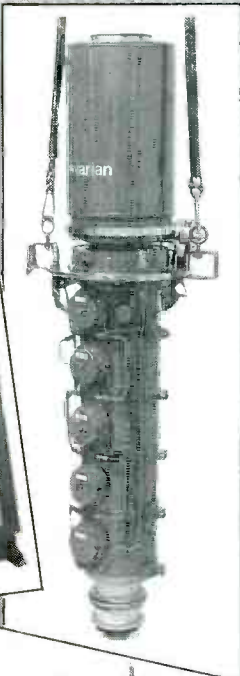
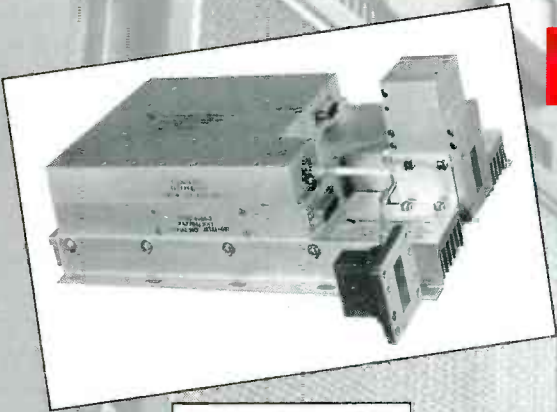
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# INTRODUCTION TO MICROWAVE TECHNOLOGY



Last time, we covered the major factors that kept classical vacuum tubes from generating microwaves in normal use: inter-electrode capacitance, lead inductance, gain-bandwidth product, and transit-time effects. The major effort in the 1930's and 1940's was to either circumvent those limitations, or exploit them to good advantage.

In a magnetron, electrons accelerate toward the anode as in a classical vacuum tube, but are deliberately returned to the cathode by a magnetic field as their speed increases. If an RF wave of the right frequency is in the cavity when the magnetic field returns the electrons, and the electrons move at the right speed (the phase velocity) they transfer

kinetic energy to the RF wave by resonance.

The electrons re-bombard the cathode, and the process repeats. Only those electrons transferring enough energy to the RF wave at resonance reach the anode, and only if they're close enough to be attracted to it. M-type magnetrons are efficient, so very few electrons reach the anode.

The whole point of classical vacuum tubes is anode current. The goal of a magnetron is to *not* generate anode current, since an electron reaching the anode can't be reexcited to generate more kinetic energy to transfer to the RF wave by resonance. An RF probe in the cathode-anode interaction space conducts the RF energy to an outside waveguide. The RF wave is the output, not the anode current.

## Learn the principles of magnetron tubes.

JOSEPH J. CARR

### Electric and magnetic fields

There are really four quantities relevant in electromagnetics: electric field intensity  $E_o$ , magnetic field intensity  $H_o$ , electric flux density  $D_o$ , and magnetic flux density  $B_o$ . The British physicist James Clerk Maxwell, in the 19th century, found the complex equations governing all four quantities.

The units of electric field intensity are volts per meter, or volts/m. The units of magnetic field intensity are amps per meter, or amps/m. The units of electric flux density are coulombs per square meter, or coulomb/m<sup>2</sup>, where

$$1 \text{ coulomb} = 6.25 \times 10^{18} \text{ electrons.}$$

The unit of magnetic flux density is the tesla, where

$$1 \text{ tesla} = 1 \text{ weber/m}^2$$

The weber is the metric unit of magnetic flux (not flux density), and is the magnetic analog of the coulomb. Just as

$$1 \text{ coulomb} = 1 \text{ amp} \times \text{s}$$

in the electric case,

$$1 \text{ weber} = 1 \text{ volt} \times \text{s}$$

in the magnetic case.

In most simple materials and vacuum, flux density is linearly proportional to field intensity. For the electric case,

$$D_o = \epsilon \times E_o,$$

and for the magnetic case,

$$B_o = \mu \times H_o.$$

The permittivity of free space is  $\epsilon_o$ , and the permeability of free space is  $\mu_o$ . In other than free space (or vacuum),

$$\epsilon = \epsilon_r \times \epsilon_o,$$

and,

$$\mu = \mu_r \times \mu_o.$$

The permittivity of free space is

$$\epsilon_o = 10^{-9} / (36 \times \pi) \text{ farads/m} = 8.85 \text{ pF/m},$$

and the permeability of free space is

$$\mu_o = 4 \times \pi \times 10^{-7} \text{ henry/m} = 1.26 \text{ } \mu\text{H/m}.$$

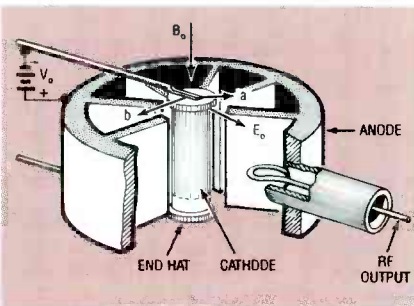


FIG. 1—A BASIC CONVENTIONAL cylindrical or conventional magnetron. The individual chambers between the spokes are the reentrant cavities, and connected to the gaps between the walls of the cavities. They're cavity resonators, metallic enclosures that confine RF energy.

### The M-type magnetron

A conventional cylindrical magnetron is shown in Fig. 1. The chambers are reentrant cavity resonators—metallic enclosures confining RF energy, connected at the gaps between their walls. They have an infinite number of oscillating modes, the lowest-frequency one being dominant. At resonance, a standing wave is generated, and the peak electric and magnetic field energies are equal.

There's a DC operating poten-

tial  $V_o$  between cathode and anode, while magnetic flux density is in the +z-direction, into the page. The anode is grounded, and the cathode is highly negative. If the anode were positive,

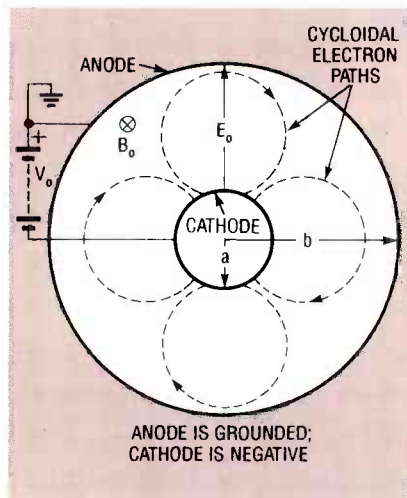


FIG. 2—ELECTRON PATHS IN A conventional magnetron. If an electron is injected into the electric field  $E_o$  between cathode and anode, it accelerates linearly. If the lines of magnetic flux density  $B_o$  is present into the page, and both  $E_o$  and  $B_o$  are properly adjusted, the electron moves cyclodially.

both it and the output waveguide would need insulation, and be dangerous to service.

Figure 2 shows electron paths in a conventional magnetron:

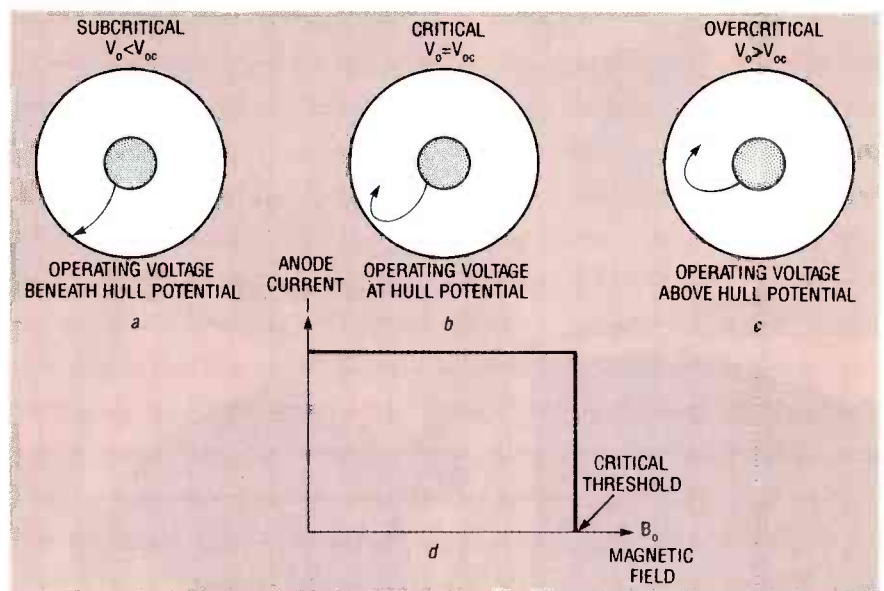


FIG. 3—THE THREE ELECTRON TRAJECTORIES in conventional magnetrons. The lines of electric field  $E_o$  goes from anode to cathode, while those of magnetic flux density  $B_o$  are into the page. The subcritical case (a) yields true anode current. In the critical case (b), electrons graze the anode, and in the supercritical (cutoff) case (c), they never reach it. A plot of anode current  $I$  as a function of  $B_o$  is shown in (d).

when electrons are injected into the electric field between cathode and anode, they're linearly accelerated. If the magnetic field is into the page, and both the electric and magnetic fields are properly adjusted, the electron moves cyclodially.

### The Hull cutoff condition

Figure 3 shows three views of a simple conventional magnetron. The electric field lines go from anode to cathode, and the magnetic field lines are into the page. For a constant magnetic field, operation is governed by the Hull magnetic cutoff criterion. The first form gives the Hull cutoff potential in terms of magnetic flux density. The second form gives the Hull cutoff magnetic flux density in terms of operating potential. The first form is

$$V_{oc} = \left( \frac{e}{8m} \right) B_o^2 b^2 \left( 1 - \frac{a^2}{b^2} \right)^2.$$

The second form is

$$B_{oc} = \frac{\left( 8V_o \frac{m}{e} \right)^{1/2}}{b \left( 1 - \frac{a^2}{b^2} \right)}.$$

In the above expressions

$V_o$  is the operating potential,  $V_{oc}$  is the Hull cutoff potential in volts.



$a$  is the cathode radius in meters,  $b$  is the anode radius in meters,  $e = 1.6 \times 10^{-19}$  coulombs, the electron charge,  $m = 9.11 \times 10^{-31}$  kilograms, the electron mass,  $B_o$  is the magnetic flux density in webers per square meter ( $\text{Wb}/\text{m}^2$ ),  $B_{oc}$  is the Hull cutoff magnetic flux density in webers per square meter ( $\text{Wb}/\text{m}^2$ ).

The relative values of operating potential and magnetic flux density govern magnetron operation. For the first form, if magnetic flux density is above cutoff for a given operating potential, the electrons don't reach the anode. The reverse holds true for the second form; if the operating voltage is under the Hull cutoff potential for a given magnetic flux density, the electrons again don't reach the anode.

Figure 4 shows the three conditions for the second form of the Hull cutoff criterion. Figure 3-a shows the subcritical case, where the operating potential is below cutoff, with a true anode current. Figure 3-b shows the critical case, where the operating potential is at cutoff, and the electrons graze the anode before returning. Figure 3-c shows the supercritical case, where the operating potential is above cutoff, and the electrons are deflected back before hitting the anode. Figure 3-d shows anode current  $I$  as a function of magnetic flux density  $B_o$ .

### Magnetron anodes

The circular anodes in Fig. 3 have an infinite number of modes, and are useless. Real magnetrons use cavity resonators like those in Fig. 1: each is

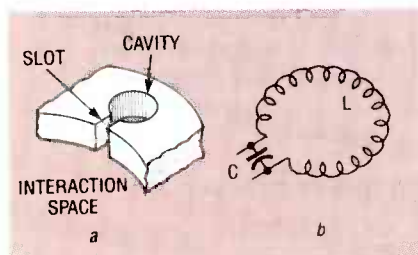


FIG. 4—THE CAVITY RESONATORS IN Fig. 2 act like a resonant L-C tank. The cavity walls primarily contribute to cavity inductance, while the spacing between the walls of the gap at the base of the cavity primarily contributes to cavity capacitance.

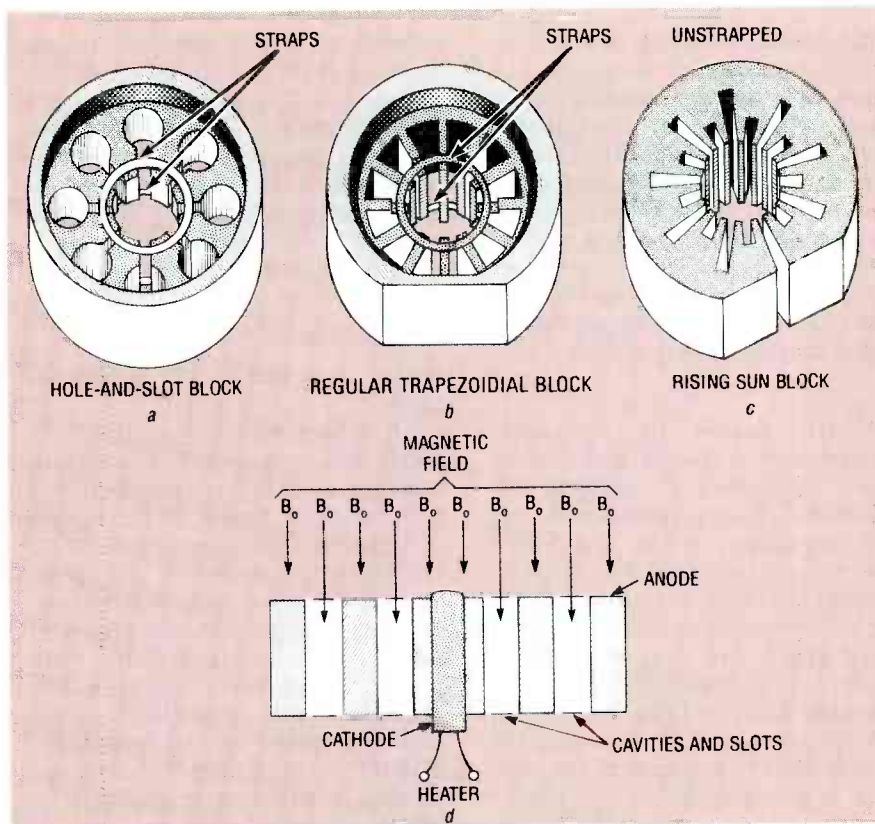


FIG. 5—SEVERAL DIFFERENT MAGNETRON ANODES; a hole-and-slot block (a), a regular trapezoidal block (b), and a rising sun block (c). In each, the cavities and anode are made from a single metal block;  $B_o$  is arranged as in (d).

a resonant L-C tank as in Fig. 4: the cavity walls fix inductance, the wall conductivity fixes resistance (not shown). Several versions are shown in Fig. 5: each is a single metal block, and  $B_o$  appears in Fig. 5-d.

Consider the hole-and-slot block in Fig. 5-a: the others are similar. For unstrapped (unshorted) anodes, the tanks are in series, as in Fig. 6-a. However, if alternate cavities are strapped (shorted) as in Fig. 6-b, the anode is an array of parallel L-C tanks, as in Fig. 6-c. That's normal for most magnetrons: due to the strapping of alternate cavities, adjacent resonators are  $180^\circ$  out of phase.

### Pi-mode operation

Most magnetrons work in  $\pi$ -mode, where the phase shift between adjacent resonators is  $\pi$  radians, or  $180^\circ$ . The radian is an alternate unit of angle, where 1 radian =  $57.3^\circ$ . When a magnetron is turned on, the electron cloud shock-excites (rings) the cavities, setting up a spatially- and time-varying electric field in the cathode-anode interaction space, adding to that due to the

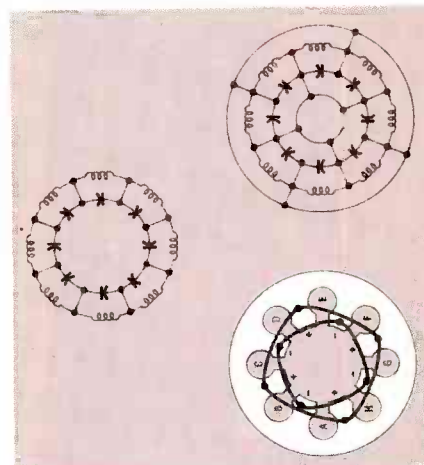


FIG. 6—EACH HOLE AND SLOT CAVITY IS A parallel-resonant L-C tank. In unstrapped (unshorted) anode, the tanks are in series, as in (a). If alternate cavities are strapped (shorted) as in (b), the magnetron becomes an array of parallel L-C tanks, as in (c). Magnetrons are normally strapped, so adjacent resonators are  $180^\circ$  out of phase.

operating potential. It varies the acceleration of the electrons due to the operating potential  $V_o$ , modulating their velocity and  $V_o$  density, creating a "bunched up" pattern.

Figure 7-a shows the electric field due to the operating potential for a hole-and-slot block, and

for a trapezoidal block in Fig. 7-b, both in  $\pi$ -mode. For oscillation to occur, the electron velocity must equal the phase velocity of the RF wave, so resonance can transfer kinetic energy into RF energy. If that occurs, the electron cloud keeps ringing the cavities, generating RF waves. The electron velocity is the ratio of the electric field from the operating potential to the magnetic flux density, or

$$v_o = E_o / B_o.$$

At that speed, the electrons lose energy to the RF wave, slow down, and return. During oscillation, there's no anode current, as shown in Fig. 3-d. Since the magnetic field is perpendicular to the electron motion, the centripetal acceleration inward from the magnetic field equals that radially outward from the electric field.

A reentrant cavity resonator is a "slow-wave" structure: its purpose is to slow down the phase

velocity of an RF wave (more below), so it interacts with an electron beam. The cavity is designed so oscillations occur only if the total phase shift around the anode is a multiple of  $360^\circ$  or  $2 \times \pi$  radians, creating a standing wave. For an N-cavity anode, the phase shift between adjacent resonators is

$$\phi_n = (2 \times \pi \times n) / N,$$

where n is the mode of oscillation.

All RF waves have a group velocity and a phase velocity. Group velocity  $v_G$  is the speed of energy propagation, equal to the speed of light in free space divided by the refractive index of the medium an RF wave passes through. Phase velocity  $v_p$  is the speed of phase propagation, the rate phase varies with distance, the speed of light multiplied by refractive index of the medium. The refractive index of a medium is always the square root of the product of its relative permeability and permittivity, so that

$$v_G = c / \sqrt{\mu_r \times \epsilon_r},$$

and

$$v_p = c \times \sqrt{\mu_r \times \epsilon_r},$$

where

$$c = 3 \times 10^8 \text{ m/s}$$

is the speed of light in free space. In the vacuum of a magnetron, both group and phase velocities equal c.

Another way to think about these two speeds is that group velocity means, "So many joules of energy per square meter pass a point per unit time," while phase velocity means, "So many radians of a wave pass a point per unit time." For a magnetron to oscillate, the electron tangential speed must equal the phase velocity, or

$$v_o = v_p$$

In Fig. 7, the electric fields shown are for two different eight-cavity blocks, or  $N=8$ . For those two blocks, the mode can be found since

$$\phi_n = (2 \times \pi \times n) / 8 = \pi,$$

so that those two anode blocks exhibit fourth-order modes, or  $n=4$ . The successive adjacent cavities create a traveling RF wave along the surface of the

slow-wave structure. The "spokes" in Fig. 7-b represent segments of the space-charge cloud as it revolves.

For a magnetron operating in  $\pi$ -mode, the number of cavities has to be even, or  $N=2, 4, 6, \dots$ . Since the phase shift between adjacent cavities is  $180^\circ$ , each pair of cavities shifts the phase  $360^\circ$ , or one cycle, maintaining a standing wave. The operating frequency of a magnetron is the speed of light divided by the product of the number of cavities N and the mean distance L between them, or

$$f = c / \lambda = c / (N \times L).$$

### The Hartree cutoff condition

The Hull condition expresses the cutoff potential in terms of magnetic flux density, or vice-versa. A more complex companion condition relating magnetic flux

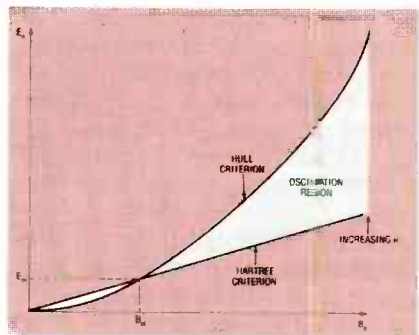


FIG. 8—THE RELATIVE EFFECTS of the hull and Hartree criteria, plotting the electric field  $E_o$  versus the magnetic flux density  $B_o$ . The electric field is directly proportional to the operating potential  $V_o$ , since the cathode-anode spacing is fixed. The Hull criterion is above, the Hartree criterion below, and they intersect both at the origin and when  $V_{oc} = V_{oh}$ . If  $V_o > V_{oh}$  and  $B_o > B_{oh}$ , oscillation occurs; if not, the RF energy is cutoff.

density to the cathode-anode spacing and the operating potential is the Hartree criterion. For the conventional magnetron

$$V_{oh} = \frac{2\pi f B_o}{Nc} (b^2 - a^2).$$

In this expression

$V_{oh}$  is the Hartree potential in volts,

$B_o$  is the magnetic flux density in webers per square meter ( $\text{Wb}/\text{m}^2$ ),

$f$  is the frequency in Hz,

$N$  is the number of resonators,

$b$  is the anode radius in meters.

continued on page 76

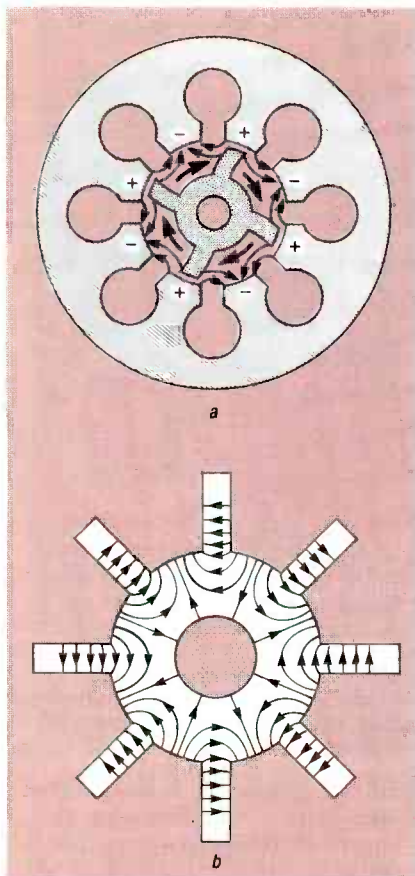


FIG. 7—THE SHOCK-EXCITED, spatially-varying  $\pi$ -mode  $E_o$  for a hole-and-slot block in (a), and a trapezoidal block in (b), both with  $N=8$ . They cause nonuniform electron acceleration resulting in velocity and density modulation, and "bunching up" of electrons.

## MEMORY CARD

*continued from page 58*

strobe) enable signals for the RAM. In order to keep the board size small, a PEEL programmable logic device was used for IC2. For those interested in programming their own device, or for those simply interested in how the decoding works, the truth table for IC2 is shown in Table 1.

The address and control signals to the RAM are buffered by IC3 and IC4. A four-position jumper, J1, is used to select the amount of on-board memory you will use and whether the printer is a IIP or III. The 8048 microcontroller is programmed to communicate to the printer such information as "I am here," and "I have 1 megabyte of memory installed," etc., and its hex code is shown in Listing 1.

### Assembly

Although the circuit is simple, the need to accommodate up to 4-megabytes of memory (32 IC's) makes the PC board rather complex. The foil patterns are provided for the board, but you will have to drill 945 holes if you wish to make your own.

Referring to the parts-placement diagram in Fig. 2, install the parts in the following order. Start by installing and soldering all of the IC sockets. The 20-pin sockets should have built-in 0.1  $\mu$ F decoupling capacitors. (The finished board is shown in Fig. 3, where you can see the IC sockets with the built-in decoupling capacitors.) Orientation of these sockets is important, as the capacitor must go to pins 10 and 20 of the pads on the board. However, you can use regular sockets and mount the capacitors on the bottom side of the board or underneath the sockets. Because you don't have to install the full 4 megabytes of memory on the board, you might want to install only as many sockets as needed. Install 8 sockets per row per megabyte, starting in the row next to IC1.

Install capacitors C1 through C5. Make sure you properly orient the polarized capacitors, C1 and C5.

Jumper block J1 may be either an 8-pin dual-row male header

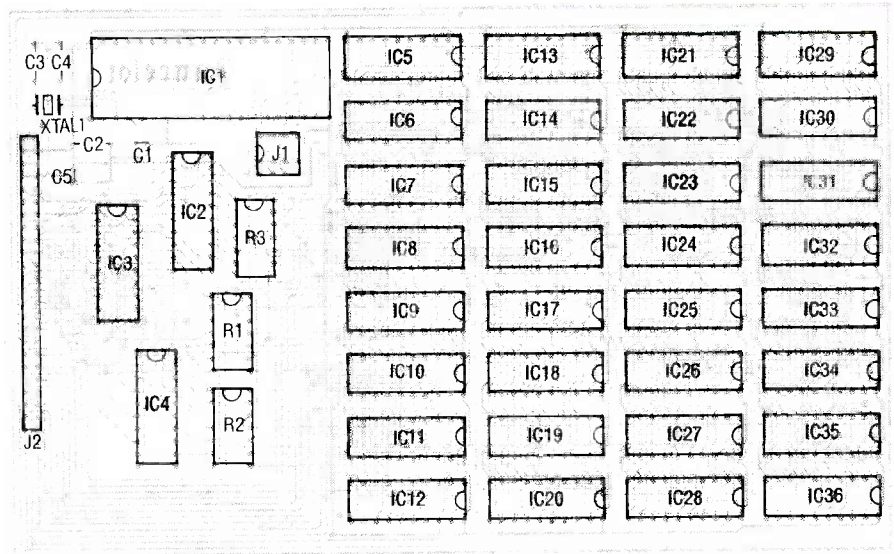


FIG. 2—ALTHOUGH THE CIRCUIT IS QUITE SIMPLE, the PC board is rather complex, in order to accommodate up to 32 dynamic RAM IC's.

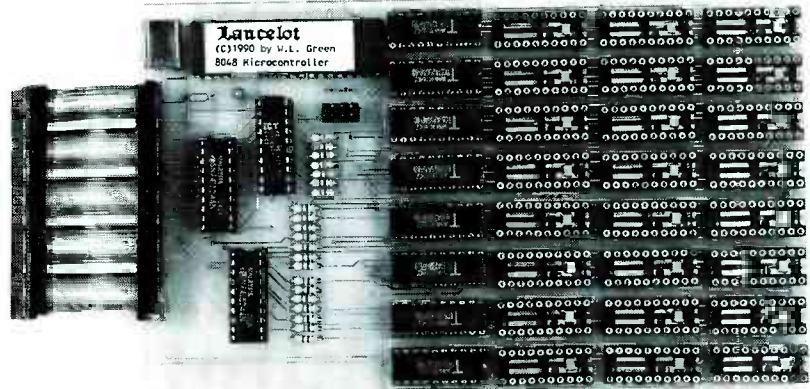


FIG. 3—THE PROTOTYPE BOARD uses IC sockets with built-in decoupling capacitors. Orientation of these sockets is important, as the capacitor must go to pins 10 and 20. You can also use regular sockets and mount the capacitor under the socket or on the solder side of the board.

TABLE 1  
TRUTH TABLE FOR 011273 DECODER

Inputs				Outputs							
1	2	3	4	12	13	14	15	16	17	18	19
1	X	X	X	H	H	H	H	H	H	H	H
0	0	0	0	L	H	H	H	H	H	H	H
0	1	0	0	H	L	H	H	H	H	H	H
0	0	1	0	H	H	L	H	H	H	H	H
0	1	1	0	H	H	H	L	H	H	H	H
0	0	0	1	H	H	H	H	L	H	H	H
0	1	0	1	H	H	H	H	H	L	H	H
0	0	1	1	H	H	H	H	H	H	L	H
0	1	1	1	H	H	H	H	H	H	H	L

"X" = Don't Care

TABLE 2

	MODEL IIP				MODEL III			
	PIN1	PIN2	PIN3	PIN4	PIN1	PIN2	PIN3	PIN4
1 MEG	O	O	O	O	O	X	O	O
2 MEG	O	O	O	X	O	X	O	X
3 MEG	O	O	X	O	O	X	X	O
4 MEG	O	O	X	X	O	X	X	X

LISTING 1

```

00 31 00 09 06 0C 21 48 01 4E 23 ED A3 ED A3 4E 23 ED A3 20 F4 CD DA 00
DD 21 35 01 CD E6 00 CD 24 01 FE 24 28 EF CD 7A 00 20 F1 E5 CD OD 01 E1
E9 CD DA 00 DD 21 3E 01 CD E6 00 CD 24 01 FE 24 20 F6 0E 08 21 00 02 ED
A3 DB 05 CB 7F 28 FA DB 05 CB 7F 20 FA ED A3 18 F0 CD DA 00 DD 21 43 01
CD E6 00 CD 24 01 FE 24 20 F6 76 01 FF 07 21 00 08 11 01 08 36 00 ED B0
18 9B 06 03 0E 04 16 40 ED 51 DB 04 E6 0F 20 06 CB 0A 10 F4 04 C9 CB 2F
4F 3E FB C6 05 10 FC 81 FE 03 FA 9F 00 D6 01 FE 07 FA A6 00 D6 01 FE 0B
FA AD 00 D6 01 87 16 00 5F FD E5 FD 21 5C 01 FD 19 FD 6E 00 FD 66 01 FD
E1 AF C9 CD E6 00 FE 24 20 F9 FD 7E 00 FD E1 F5 CD EC 00 CD OD 01 F1 CB
42 C9 DD 21 30 01 CD E6 00 FE 24 20 F9 C9 DD 7E 00 FE 24 C8 01 03 00 21
02 08 11 03 08 ED B8 FE 2A 20 03 3A 03 08 12 D0 23 01 04 00 21 03 08 11
03 10 ED B8 C9 3E 70 D3 04 21 00 02 CD 27 01 DB 04 E6 0F 20 F4 21 00 02
CD 27 01 C9 21 00 18 11 00 00 37 ED 52 20 FB C9 20 20 20 20 24 43 4F 4D
4D 41 4E 44 3F 24 52 45 44 59 24 44 4F 4E 45 24 0A CF 00 08 FF 0B CF 00
09 00 06 CF 0F 04 00 07 CF 80 05 3C 15 00 06 00 15 00 15 00 15 00 15 00
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0F 0F FF FF 0F 0F 0F 0F FF FF 0F 0F 0F FF F0 F0 F0 FF FF F0 FF F0 FF
FF F0 F0 FF FF 0F 0F 0F FF FF 0F 0F 0F FF 0F 0F 0F EF EF FF F0 F0 F0 FF
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FF FF F3 F3 F3 FF FF F3 F3 F3 FF FF F3 F3 F3 FF FF 3F 3F 3F FF 3F 3F 3F
3F 3F 3F 3F 3F 3F FF FF F3 F3 F3 FF F3 F3 F3 FF F3 F3 F3 FF F3 F3 F3
3F 3F 3F 3F 3F 3F FF FF 3F 3F 3F FF 3F 3F 3F FF F3 F3 F3 FF F3 F3 FC
F0 FC FC F3 FF 3C 3C FC 3C 3C FC FC FC FC 3C 3C BC BC FC 30 30 FC 30
FC 3C FC FC FC 3C 30 30 FC 38 FC 30 30 FC 30 FC 30 FC 3C FC F0 30 30 BC
70 FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC FC
30 3C FC F0 F0 38 34 FC DC CC CC CC CC CC CC CC CC CC CC CC CC CC CC 00
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**MICRO TECH**  
continued from page 74

a is the cathode radius in meters.

Figure 8 shows a simultaneous plot of the Hull and Hartree criteria for a conventional magnetron, where the electric field  $E_o$  is a function of magnetic flux density  $B_o$ .

The electric field between two conductive surfaces is always the operating potential divided by the distance between them. Since the geometry of the magnetron is fixed, with the anode-cathode spacing a constant, then that proportionality is valid. The Hull curve is on top, the Hartree curve below. They intersect at two locations: at the origin, and when the Hull and Hartree potentials are equal, which really also means that  $E_{oc}$  equals  $E_{oh}$ .

If  $V_o$  is greater than  $V_{oi}$  and  $B_o$  is greater than  $B_{oi}$ , anode current is cutoff and the magnetron oscillates; otherwise, anode current flows and oscillation is cutoff.



FIG. 9—THE VARIAN SFD-352 TUNABLE, conventional magnetron; the output waveguide flange appears on the top of the front. It has a tuning range of 8.5–9.6 GHz set by the vernier, a peak power of 220 kilowatts, a nominal anode potential of 22 kilovolts, and a peak anode current of 28 amps.

**Conclusion**

Figure 9 shows a typical example of a magnetron, the SFD-352 tunable, coaxial version from Varian Assocs. A coaxial version differs from a conventional version by a high-Q stabilizing cavity that surrounds the anode. The output waveguide flange appears on the top of the front, and it has a tuning range of 8.5–9.6 GHz set by the vernier dial. R-E

connector with shorting blocks or a 4-position DIP switch; install it now. Also install and solder J2, a 48-pin double-row straight male header.

Make or purchase a cable to plug the memory board into the printer. The cable must be a 48-conductor ribbon cable, about 2 inches long, with a 48-pin female IDC (insulation displacement) connector on each end.

Install the 6-MHz crystal (XTAL1) so that it lays on top of C3 and C4, parallel to the PC board. A dab of epoxy will keep it

from getting broken off later.

Check your work carefully. Examine your soldering under an illuminated magnifier for solder bridges.

Install the IC's in their sockets. You will need 8 256K x 4-bit dynamic RAM's (no slower than 120 ns) for each megabyte of memory you wish to install, starting with the row nearest IC1, continuing toward the rear edge of the board.

Table 2 indicates how to set J1 (the DIP switch or jumpers) for the amount of memory and type  
continued on page 94

# HARDWARE HACKER

This month we look at various types of filters and a digital thermometer.

DON LANCASTER

Our no-charge Hardware Hacker helpline sure gets a lot of traffic on filters and filtering. So this month, I thought we might go over some filter fundamentals, especially in deciding just what kind of filter should get used where.

## Passive filters

An electronic *filter* is some frequency-selective network that favors certain frequencies at the expense of others. Filters are normally used to strengthen wanted signals while trying to reject unwanted ones.

Traditionally, filters were built by using combinations of inductors and capacitors. These are called *passive filters*, and three examples appear in Fig. 1.

In 1-a, we have an example of a *low-pass* filter. At very low frequencies the inductor appears as a piece of straight wire and the capacitor's reactance is extremely high. So DC and very low audio frequencies are readily passed. At very high frequencies, the inductor looks like a high blocking impedance and the capacitor looks like a very low shunting impedance, so all the high frequencies will get strongly attenuated.

The one-two punch of this example makes it a *second order* filter. At low frequencies, the response is flat. At very high frequencies, the response

will quarter with each doubling of frequency, or fall off at a  $-12$ -decibel-per octave rate.

What will happen at the *corner frequency* with this circuit? Well, that depends on the *ratio* of the inductance to capacitance. Should you want the smoothest possible response, you can adjust the ratio of L to C so your response ends up precisely 3 decibels down, or roughly 70 percent of the amplitude at the corner frequency. This  $-3$ -decibel point could also be called the *cutoff frequency*. Such a low-pass filter with the smoothest possible passband is usually called a *Butterworth* filter.

The L/C ratio of the circuit is also known as the *damping*. If you are *critically damped*, you will get the smoothest possible response. If you are *underdamped*, you get a rising or a peaked response at your corner frequency. If you are *overdamped*, you get a very droopy result.

A simple *treble* control on a Hi-Fi is an example of a low-pass filter.

A *band-pass* filter appears in Fig. 1-b. At rather low frequencies, the capacitor provides a high reactance, and your response *increases* at a  $+6$ -decibel per octave rate. At resonance, otherwise called the *center frequency*, the reactances cancel, giving you unity gain. At the higher frequencies, the inductor provides a

high series reactance, and the response *decreases* at a  $-6$ -decibel-per octave rate.

The ratio of the inductance to the capacitance sets the damping, which in turn will set the sharpness of your resonant peak. Since very low damping values are usually involved, a factor called the "*Q*" is used instead. The *Q*, or "quality" factor is the inverse of the damping. The *Q* is also the bandwidth of the center peak between its  $-3$  decibel points.

Note that, no matter how high the *Q*, the slopes at very low and very high frequencies will stay at  $+6$  and  $-6$  decibels per octave. Your choice of *Q* determines only the narrowness and the peakedness of the response *at or near resonance*. The tuning dial on an AM radio is an example of a band-pass filter.

A second-order *high-pass* filter appears in Fig. 1-c. Here, the high impedance of the series capacitor and the low impedance of that shunting inductor attenuates the very low frequencies, creating a double whammy attenuation rate of  $+12$  decibels per octave. At higher frequencies, the capacitor's reactance is low and the inductor's is high, freely passing the highs without attenuation.

Once again at the corner frequency, you will get a peaked, smooth, or drooping response depending on your L/C ratio and its damping factor.

The *bass* control on a Hi-Fi is one example of a high-pass filter.

Actually, there is no such thing as a true electronic high-pass filter, since one of these would also have to pass microwaves, heat, light, and X-rays. At very high frequencies, the circuit strays (such as a capacitor self-resonating on its own leads) can alter the response.

High-pass filters also tend to be "noisy," since they freely pass all the harmonics of all supposedly rejected waveforms. Compared to a low-pass filter, which performs one or more integrations, a high-pass filter does

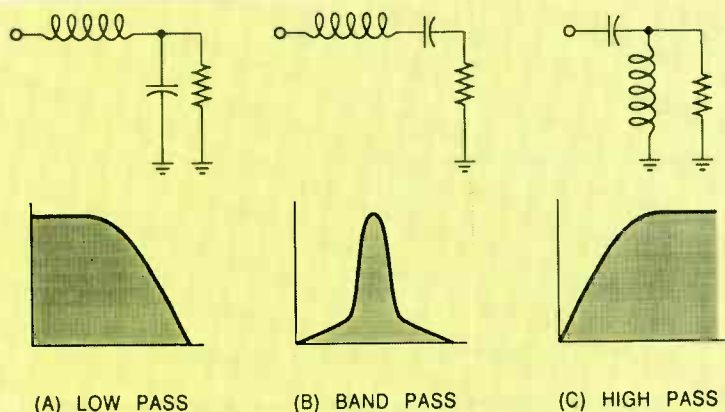


FIG. 1—THREE EXAMPLES OF SECOND-ORDER passive LC filter sections.

one or more differentiations, or slope extractions. This also can add to the overall noise.

Fancier filter responses are picked up by using additional inductors and extra capacitors to increase the *order* of your filter. Unfortunately, you can not just "stack up" passive sections. Each in turn has to play a specific and non-obvious part in your overall desired response.

My favorite design book on passive filters remains Louis Weinberg's almost ancient *Network Analysis and Synthesis* (McGraw Hill, 1962). The *Radio Amateur's Handbook* also has lots of good passive filter design information in it, as do most college-level circuit or network texts.

These days, you usually try to avoid passive filters like the plague, since they are bulky and expensive, and hard to redesign, calibrate, or adjust. They also lack gain and do need carefully controlled source and load impedances. So, you'll want to avoid passive filters at all costs—unless you happen to be working with ex-

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tremely low signals, at very high power levels, or at very high frequencies where nothing else will do the job. The usual way of filtering stuff today involves...

### Active filters

With an *active filter*, you can use combinations of resistors, capacitors, and operational amplifiers to fake the response you would get from a passive LC filter. The energy from the power supply is used to substitute for the energy normally stored in an inductor's magnetic field.

Important advantages of the active filters are that there are no inductors involved, they are easy to design, and they are easy to tune.

Since active filters can also provide buffering and gain, they are far less

sensitive to source or load impedances than passive filters.

While there have been many different active-filter design methods in the past, only two have really survived and stay popular today. These are the everyday *Sallen-Key* single op-amp filters and higher performance *State Variable* filters that need three or four op-amps per second-order section.

Figure 2-a shows to you a second-order Sallen-Key low-pass filter, normalized to a 10K impedance level and a 1-kHz cutoff frequency.

The original horse's mouth on this was R. Sallen and Key's *A practical method of designing RC active filters* from the IRE Transactions on Circuit Theory, March 1955, pp 74-85.

Their prototype Sallen-Key filters were intended for use with cathode followers, the vacuum-tube precursor to a transistor emitter-follower circuit. These were designed to work with a unity or slightly lower gain, which forced you to select weird ratios of capacitors and caused an interaction between the corner frequency and the desired damping.

Many years ago, I played around with the Sallen-Key math in detail and came up with a twist that made these filters far simpler to design and use. I

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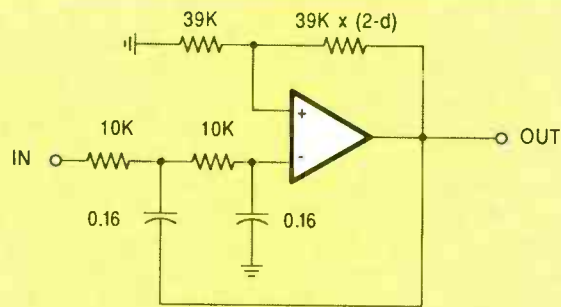
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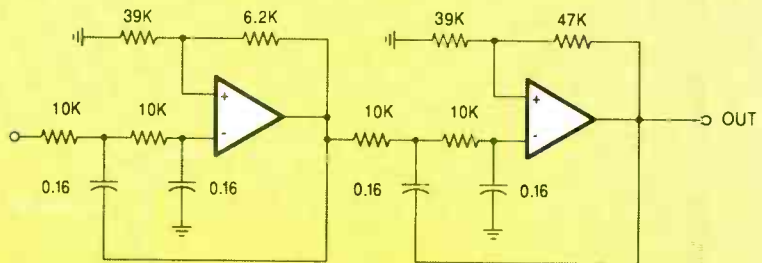
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(A) SIMPLE SECOND ORDER SALLEN-KEY SECTION



(B) FOURTH ORDER BUTTERWORTH LOW PASS AUDIO FILTER

FIG. 2—TWO SALLEN-KEY LOW-PASS active filters. Most any premium grade of op-amp can be used. Components should be 5% or better.

renamed it the *Equal Component Value Sallen-Key* filter. In the Fig. 2-a design, both capacitors are of identical value and set only frequency. Both resistors are of identical value and also set only frequency. The op-amp gain independently sets the damping.

To scale your frequency, you just *increase* either resistor pair or either capacitor pair to *lower* frequency, and vice versa. To scale impedance, proportionately raise the resistors and lower the capacitors. Full details appear in my *Active Filter Cookbook*.

Normally, you combine, or *cascade* second order sections to build up a fancier filter of higher order. By very carefully selecting the damping value

and that corner frequency of each second-order section, you can produce an overall filter response of most any desired complexity.

Some of these fancier responses do have specific names. For instance, a *Bessel* filter will give you the flattest possible time delay at the expense of the amplitude fall-off. As we've just seen, a *Butterworth* filter can give you the smoothest possible amplitude response. If you are willing to allow some ripple in the passband, you end up with a *Chebyshev* filter. Popular Chebyshev filters could be created with one, two, or even three decibels of passband ripple. Finally, the *Cauer*, or *Elliptical* type filter will

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also add "zeros" to your stop band, giving you the fastest possible fall-off.

One thing that many beginning hackers miss: if your filter is made up of cascaded and isolated second-order sections, *the only difference between these filter types lies in how you select the damping and the corner frequency of each section.* That's all. Thus, once you have a filter built, all you need do is change the damping and the corner frequency of each section to get any desired result from Bessel on through Chebychev.

As with passive filters, you do not simply stack up identical second-order sections. Instead, you must carefully select your damping and corner frequency of each section to properly interact with the others to get the final desired response.

Figure 2-b shows a fourth-order Butterworth low-pass filter having a 1-

kHz cutoff frequency and a -24-deci-bel per octave rolloff. Note that the two sections are *not* identical. Also note that a DC return path to ground must be provided back through the input source resistance for a low-pass active filter to work properly.

It has been pretty much proven to everyone's satisfaction that you can *not* build up a high-Q active band-pass filter using only a single op-amp. The impedance levels, interactions, and gain requirements all gang up on you as you raise the Q.

Figure 3 shows you the best of a sorry lot of single op-amp second-order band-pass filters. This one is called a *multiple feedback* circuit. It is recommended only for Q values much less than 10. Thus, while that type of filter is useful for such things as an equalizer or a simple psychedelic lighting filter, it is strictly limited

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to lower Q applications.

The higher performance workhorse second-order active filter circuit is called a *state variable filter* and is built using three or four op-amps per Fig. 4. This one has three separate low-pass, band-pass, and high-pass outputs, is very well behaved, and can work with very high Q or low damping values. A fourth op-amp can be added to the circuit shown to make the gain independent of the damping.

Finally, Fig. 5 shows you a Sallen-Key single op-amp high-pass circuit. This one is simply the low-pass circuit of Fig. 2 "insided out" to get the complementary response.

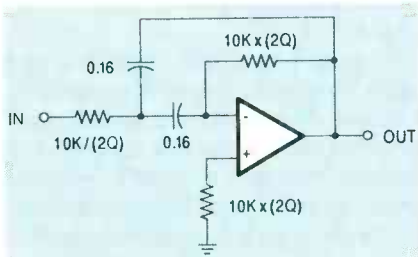


FIG. 3—THIS SINGLE-AMPLIFIER multiple-feedback band-pass active filter can be used only for Q values of 10 or less.

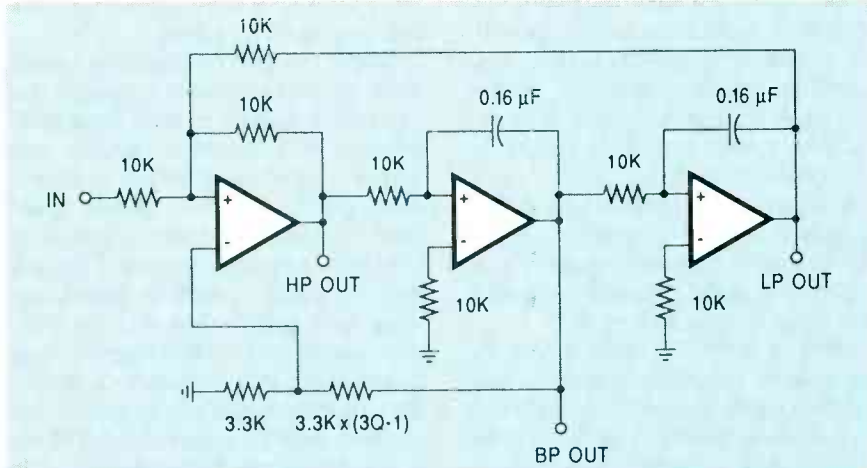


FIG. 4—THIS STATE-VARIABLE ACTIVE FILTER gives low-pass, band-pass, and high-pass outputs and is best used for high-Q or low-damping applications.

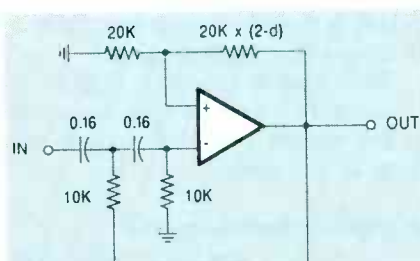


FIG. 5—THE SALLEN-KEY HIGH-PASS second-order filter section is simply the low-pass circuit of Fig. 2-a inside out. Values are for 1 kHz.

Active filters are limited by the frequency response, the slew rate, distortion, and noise floor of the op-amp used. They are best used at audio and low video frequencies having signals which are neither very small nor excessively large. Quality op-amps for active filters are available from *Linear Technology, Burr-Brown, Analog Devices, Maxim, National, and PMI*.

By one of those utterly astounding coincidences that seem to infest this column, I've written an *Active Filter Cookbook* that somehow has gotten up to its fifteenth printing. It includes everything you need to build all your own real-world active filters. Write or call for an autographed copy.

### Other filter types

Besides passive and active filters, there are several other major new methods of filtering electronic signals that are of more than passing hacker interest. These now include *switched capacitor filters, digital signal processing, and surface wave devices*.

A *switched capacitor* filter is just that—some integrated circuit which contains a bunch of small capacitors

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that are switched on and off to sample an input signal. If the switching is just right, the charge on the capacitor will follow and reinforce the input signal. If it is wrong, the charge on the capacitor will average out to zero. By carefully arranging the network of properly switched capacitors, you can favor certain frequencies and reject other ones.

The big advantages of switched capacitor filters are electronic tunability and minimum cost. In the past,

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switched capacitor filters were noisy and produced significant distortion. Today's circuits are far better, but they still don't handle extremely small input signals very well.

Important uses for these switched capacitor filters are modems, touch-tone detection, disk drives, CD players, industrial instrumentation, and data acquisition.

Several large suppliers of switched capacitor filters now include *Linear Technology*, *Maxim*, and *Exar*. All three sources have detailed data sheets and ap notes available.

A *digital signal processor* is just a specialized type of microcomputer. To do filtering using digital signal processing, you first analog-to-digital (A/D) convert your input signal into strings of numbers in memory. Then you use digital techniques to modify these numbers in memory. Finally, your digital-to-analog (D/A) convert your filtered results.

While that may sound like a real runaround, these days you can digital signal process in one single and reasonably priced chip. There are many big advantages to DSP filtering. One major advantage is that you can easily create filters that can be extremely difficult or impossible to handle with passive or active analog techniques. Examples include "brickwall" filters with near-infinite response slopes, and filters with constant phase or controlled group delay.

Another major advantage is full programmability. Nothing changes except some software words if you want to completely change what your filter does or how it does it.

Most of the DSP chips are really specialized microprocessors. Usually they have powerful internal firmware commands which let you rapidly multiply, shift, and add. They also usually provide specialized functions such as barrel shifting and zero time testing and branching. Both fixed point and floating point processors are available today.

DSP is obviously limited to lower frequencies unless you do not need real time results. You also have the usual aliasing problems and the A/D quantization noise limitations to cope with as well.

Important use areas for DSP include geophysics, for biological research, in speech synthesis and recognition, radar, and electronic music. Just about all of the latest per-

sonal computers and synthesizers have gone the DSP route for most of their sound capabilities. The main manufacturers of DSP products include *Analog Devices*, *Texas Instruments*, *Motorola*, and *TRW*. All of these folks have extensive data books and detailed application notes available.

*Surface acoustical wave*, or SAW devices are a specialized type of low-cost filter which is quite popular in television and cable systems. They consist of a piezoelectric disk which has an acoustical transmitter and an acoustical receiver on it. Unlike your usual audio devices, these acoustical waves involve sound waves whose frequency typically lies in 40- to 400-MHz range.

Special finger-like contacts are placed between the transmitter and receiver. These fingers cause constructive and destructive interference patterns that give the SAW device a specified response. Typical uses are for TV vestigial sideband filtering, for various descrambling circuits, and to set the IF amplifier passband in TV receivers.

The big advantages of SAW filters are that they're cheap, accurate, stable, and need no tuning.

Sadly, the SAW filters don't really hack all that well, even though you can readily find them for a buck each surplus. A SAW filter handles one and only one specified job in a carefully specified manner at one specified frequency and into a specified load from a specific source. They are not in any way tunable or adjustable. What you got is what you get. And your own custom SAW filter involves a very steep setup charge, comparable to a full custom integrated circuit.

One leading supplier of SAW filters is *Plessey Signal Technologies*, while bunches of surplus sources are available.

Let me know if you need any more details or use circuits for any of these alternate filter technologies.

This month's resource sidebar is on active filters and shows you many of the names and numbers you will need to get started.

### A digital thermometer

*Radio Shack* now has an amazingly sophisticated digital thermometer that sells for less than twenty bucks. It is part number 277-123.

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battery and has a four-digit LCD to display temperature in Fahrenheit or Centigrade over a -40- to 122-degree F range.

Incredibly, there is both a recording *max-min* feature and a settable alarm and controller capability. Both on-off levels and a 2-kHz piezo tone are provided as outputs.

You have a choice of a one-second or a fifteen-second update for your display. Total operating current is in the microamp range.

The out-of-the-box accuracy is only a degree or so Fahrenheit, but the circuit seems stable enough that you might custom calibrate it for such things as a hot-tub controller or for cave-stream temperature logging. Unit-to-unit variations are also within a degree. The resolution is a tenth of a degree and seems real. Although not waterproof, that is easily fixed with a tube of silicon bathtub caulk.

As received, the device displays Centigrade at fifteen seconds per update. To select Fahrenheit with a one-second update, just jumper pins 13, 14, and 16 on the edge connector.

We'll probably look at this gem in more detail in a future column. For now, let's make a contest out of it. We'll have all the usual *Incredible Secret Money Machine* book prizes, along with an all-expense-paid (FOB Thatcher, AZ) *tinaja quest* for two going to the very best of all.

Either (A) show me a new and un-

usual application for a miniature and micropowered max-min thermometer, or (B) show me some simple and clean way to get the digital data out of the 277-123 thermometer into a remote computer. Send your written entries directly to me, and *not* to the **Radio-Electronics** editorial offices.

### New tech literature

New data books this month include the *Microcontroller Handbook* from Siemens, a new *Optoelectronics Data Book* from Sharp, an *Op-Amp Macromodel Data Manual and Disk* from Texas Instruments, and that *Semiconductor Data Book and Ap Notes* from Unitrode.

From International Rectifier, a *Microelectronic Relay Design Manual*, and an IGBT product catalog.

There's a stupendously impressive *Selection Guide to Integrated Circuits* from Telefunken that is chock full of unusual TV and auto chips.

Inks which let you plot patterns directly onto all your printed circuit boards are available through Loch Ness. They also have some low-end multilayer prototyping systems you may find of interest.

Testing surface-mount devices and other weird or tiny packages can be a real hacker challenge. So, *Emulation Technology* has all sorts of adaptors and accessories that ease interfacing. Ask for their current catalog.

*An Overview of SCSI Concepts* is a great new manual available free from *Peer Protocols*. Three off-the-wall odd magazines are *Extraordinary Science*, *Surplus News*, and *Science Frontiers*.

Free software demos this month include the 48SX calculator disk from Hewlett-Packard, and the 945 heater controller demo from Watlow.

A free mechanical sample of GUR is available from Hoechst. This is a new plastic which is tough, cheap, self-healing and slippery.

Turning to my own products, for the fundamentals of digital integrated circuits, check into either my *TTL Cookbook* or *CMOS Cookbook*. And for those of you interested in the PostScript language or in Book-on-Demand publishing, our ongoing roundtable is doing fine on *Genie*. By the time you read this, over 1000 free downloads should be available.

Finally, I do have a new and free mailer for you which includes dozens of insider hardware hacking secret sources. Write or call for info.

Our usual reminder here that most of the items mentioned appear either in the *Names and Numbers* or in the *Active Filter Resources* sidebars.

As always, this is your column and you can get technical help and off-the-wall networking per that *Need Help?* box. The best calling times are weekdays 8-5, *Mountain Standard Time*. Let's hear from you.

R-E

OCTOBER 1990

# AUDIO UPDATE

## The Sound of Audio: An AES conference report, Part 2

LARRY KLEIN

Last month I started my report on a special Audio Engineering Society Conference held early last may in Washington, D.C. The four-day conference was a wide-ranging exploration of the latest findings on the perception, measurement, and reproduction of sound. I regret that because of space and time limitations, these two reports are at best a once-over-lightly review of an extremely enlightening series of lectures and discussions.

The audibility of distortion has been a controversial matter, probably from the moment the very first amplifier was designed. In the beginning, there was simple harmonic distortion (HD) that had an important virtue: It was easy to measure. However, the correlation between high HD and sonic unpleasantness was far from perfect—which lead researchers to discover/invent other types of distortions and new ways to measure them. During the 1950's, intermodulation distortion (IM), which is the unwanted arithmetic sum and difference products of two interacting frequencies, achieved instant fame as being more audibly obnoxious than HD. That was said to be true because, unlike HD, its spurious products are not harmonically related to the desired signals.

In any case, as I've said in these pages and Richard Cabot stated in his conference paper, "Audible Effects vs. Electrical Measurements in the Electrical Signal Path," HD and IM are *not* different kinds of distortion as much as they are different effects of the same nonlinearities in the equipment being tested. And because with most amplifiers there is a predictable relationship between IM and HD levels, either measurement can be used to somewhat predict audible performance.

### Distortion data

As I did for the authors in Part 1, I'll extract and paraphrase (when necessary) some of Mr. Cabot's more interesting points. In his bibliography, Cabot cites the previous relevant researches of more than 50(!) inves-

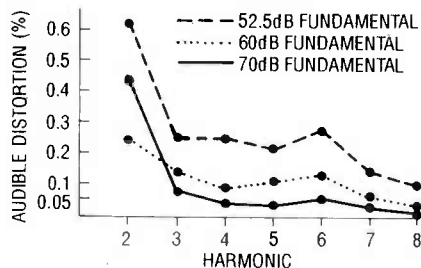


FIG. 1—THREE TEST-TONE LEVELS showing the amounts of just-audible distortions up to the 8th harmonic.

tigators, certainly a daunting task to evaluate and synopsize!

- The audibility of distortion clearly does not depend on its relative percentages alone. Other significant factors are: (1) the characteristics of the equipment's nonlinearity; (2) the instantaneous level of the reproduced sound; (3) the type and complexity of the audio test signal; (4) the spatial qualities in the reproduced sound field; (5) the characteristics of the listening environment; (6) the distortion levels in the associated equipment and in the program material itself; and (7) the listener's ability to marshal his talents, if any, as a "golden ear."

- Crossover distortion (CD), which became an important factor during the early days of transistor amplifiers, results from a push-pull amplifier's nonlinearity in the area where the signal passes through zero on its way to the set of output device(s). A "witch's brew" of high-order HD and IM products are produced whose relative amplitudes increase as the signal level decreases. This means that, like noise, CD is *more* audible at low signal levels.

- Different nonlinear conditions that measure the same with a given test setup may afflict the ear quite differently depending upon the levels and frequencies of the test program.

- Although the distortion in today's best analog audio equipment is barely measurable and (to most listeners)

completely inaudible, digital has introduced several potentially ear-disturbing phenomena. For example, the digital sampling process introduces a new and different type of distortion known as "aliasing." Spurious harmonics are produced in the audio band in the range above half the sampling-rate frequency. For example, with a 44-kHz sampling clock, the third-harmonic of a 10-kHz tone will appear at 14 kHz (44 kHz minus 30 kHz). Such problems can occur even in units with well-designed anti-alias filters, if nonlinearity is present after the filtering. Today, the problem seems well taken care of, but it illustrates the fact that new circuitry can produce new distortions.

### Dynamic range results

Dynamic range does not appear to be an important factor in distortion, other than in the obvious situation where the signal level exceeds the capabilities of a component. Clipping and other overload effects are the prices paid for pushing a component too hard. However, the other side of the dynamic-range coin—noise level—also has a great deal to do with the audibility of distortion effects. Here, we are looking at very low-level distortions and the masking effects on them of electronic and environmental noise. Specifically, if the noise is high enough in level and occurs in the same frequency areas as the distortion, the distortion will be masked.

### Audibility of distortion

As I noted earlier, the minimum level of distortion that can be detected by the human ear has been the subject of much ill-informed controversy over the years. The graph in Fig. 1 illustrates the results of a research project on the perception of HD using a 357-Hz test tone. At a listening level of 70 dB, fourth-harmonic distortion as low as 0.05%(!) was audible. It was noted that the basic sensitivity of the human ear was the limiting factor in detecting distortion. That should come as no surprise, since distortion of pure tones or simple music such as

a solo flute is *not* heard as a wave-form aberration—which is what it looks like on a scope—but rather as a distinct and separate tone or noise.

That's why the addition of high-order harmonic distortion to single mid-range frequencies is so readily audible. But in real life, with complex classical or rock music, distortion has to reach 6% or so before even the most golden of ears become upset. There's no mystery to all this—it's our old friend *masking* at work. If there happen to be loud musical frequencies present in the same areas where the spurious harmonic and IM frequencies occur, the distortions simply won't be heard. All this reaffirms the difficulty in generalizing about what we can and can't hear, and under what conditions.

I can't resist adding a personal distortion-oriented note to this report. More than 10 years ago, the Nakamichi Corporation held a press party to celebrate the opening of their East Coast offices. Part of the new facility was a small demonstration recording studio completely outfitted

with Nakamichi tape decks, microphones, monitors, amplifiers, and so forth. As I came in through the control-room door, Etsuro Nakamichi greeted me and pointed out that a live string quartet, specially hired for the

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occasion, was about to perform in the small studio area.

To my ears, the sound of the live musicians as reproduced in the control room has a harsh, distorted quality. I wondered what to say to Mr. Nakamichi, who was obviously proud

of his new installation. I decided that honesty was the best policy, and opined that the sound we were hearing was "a little shrill." To my surprise, Etsuro agreed with a grin, and ushered me through the sound-proofed door into the studio. I was shocked to discover that the live musicians in the studio sounded exactly as distorted as their reproduction in the control room—which was a real tribute to the fidelity of the Nakamichi equipment. Etsuro explained that the acoustic design of the studio still needed some work—increased damping mostly—to control an over-emphasis of the highs, but they hadn't had time to complete the work before the scheduled opening.

Two distortion-related morals can be drawn from that story: A boost in the upper half of the audio spectrum (due to room reflectivity or other causes) where the higher musical harmonics can easily be misinterpreted by the ear as gross HD or IM. And even unamplified *live* music can sound distorted under (im)proper conditions. **R-E**

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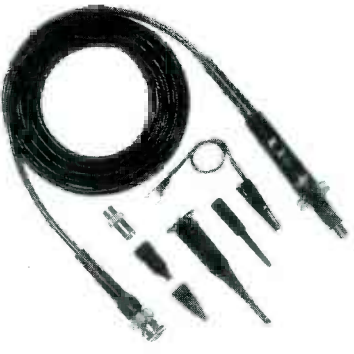
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# COMPUTER CONNECTIONS

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**JEFF HOLTZMAN**

**F**orte, a small company in upstate New York, has combined a Z80 running a home-brew multitasking operating system, a pair of 6582 SID's (sound interface devices, used in several Commodore computers), and a high-speed analog-to-digital converter. The result is a full-length card that fits in any 8- or 16-bit IBM-compatible expansion slot, and that gives you an extremely powerful environment for creating MIDI-compatible stereo musical scores, and for digitizing and editing any sound with a maximum frequency of about 40 kHz. The \$350 package is called Audio F/X.

The card provides a line-level mono input for digitizing external sounds, and line-level stereo outputs suitable for driving a quality stereo system. When playing back digitized sound, the output is mono; when playing back scored music, each channel is driven independently by one of the SID's.

The hardware is controlled by several different graphically oriented software modules. The music scoring module is called Sonata; it uses the GEM graphical interface (also used by Ventura Publisher), as shown in Fig. 1. A series of drop-down menus allow you to load and save files, choose notes and rests, key signatures, instrument parameters, etc. A control panel at the bottom of the screen allows you to set volume, balance, tempo, instrument, and to initiate playback (either from the current position or from the beginning).

The options menu brings up a dialog box that allows you great freedom in creating instruments. You can choose a basic waveform (sawtooth, square, triangle, or white noise), and then vary its attack time, sustain level and time, delay time, and release time, all independently of one another. Advanced features allow you to modulate an instrument, filter it in various ways (lowpass, bandpass, highpass), and add resonance. The

software makes it easy to create just the right sound, because you can play a sample note or scale from within the dialog box, as well as hear the effect, modify settings, play another sample, and so on.

Scoring music is fairly efficient, due to the presence of a number of keyboard shortcuts. There are keys to select notes and rests (whole, half, quarter, etc.), load and save files, interact with a MIDI device, add sharps and flats, change keys, and more. A "floating" toolbox (as in PageMaker) would allow convenient mouse-only operation. You can add repeats, fermatas, and dotted notes. Other effects includes slurs, crescendos, and decrescendos.

Sonata provides an option to print your score, but only a few common dot-matrix printers are supported, so graphics printing is *slow*; laser-printer support would be another welcome addition.

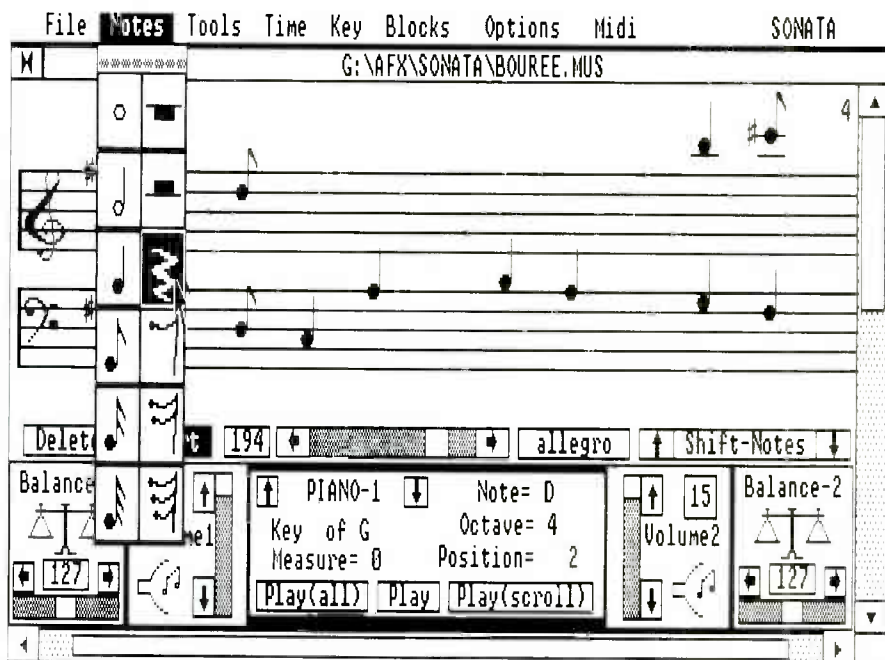
The editor provides an overall

range of eight octaves, four of which display at any time. Scroll bars along the side of the screen allow you to switch octaves; horizontal scroll bars move you through the score.

Editing functions allow you to define a block of notes and then copy it, delete it, and shift it up or down. A function to shift a block up or down an entire octave at once would be useful.

MIDI functions allow you to record from a Roland or compatible keyboard, to "quantize" notes to ensure perfect timing, and play back scored music through the MIDI device. Although the built-in playback hardware offers six voices—three for the left channel and three for the right—eight voices can be recorded from and played back through a MIDI device.

You can't score some notes and subsequently create an instrument and apply it to those notes; however you can modify the instrument associated with a voice at any time.



**FIG. 1—THE MUSIC SCORING MODULE, called Sonata, uses the GEM graphical interface. A series of drop-down menus allow you to load and save files, choose notes and rests, key signatures, instrument parameters, etc.**

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## Sound editor

The other main software component of Audio F/X is the sound editor. It, too, runs in a graphical mode, as shown in Fig. 2, but all commands must be executed from the keyboard, which is less convenient than the GEM environment of Sonata.

Basic functions allow you to record and edit sound. To record, you press Alt-F3, and specify the number of samples to record; the range is 1-65,000. Sampling rate is specified elsewhere, before you enter the record function. Naturally, the more often you sample, the higher the fidelity of the sound that is recorded, but the more disk space is used. A demo file containing a fairly hi-fi rendition of a popular song requires almost one megabyte of space for about 50 seconds of music. An 8-bit A/D converter is used, so each sample comprises of one byte with a decimal value of 0-255.

After you specify the sample rate, the program displays a simulated VU meter that allows you to set the level of your source, after which you press any key to begin. The program then digitizes sound at the specified sample rate. After all samples have been collected (or you press the space bar to halt prematurely), the waveform is displayed, and you can play it back (Shift-F3), edit it, and save it to disk.

The program supplies two cursors, L and R, that generally define an editing area. Separate pairs of function keys move the two cursors; another key allows you to zoom the area between them; yet others allow you to mark that area (for subsequent copying), or to delete, reverse, amplify, or attenuate it.

You can split the screen, and copy

a marked block from one window to another. The split-screen mode is useful for creating special effects, particularly reverb and echo. It's also useful for assembling a waveform from bits and pieces of other waveforms. To create a reverb effect, you mark a block, move the left cursor slightly to the right of its initial position, and then execute the mix com-

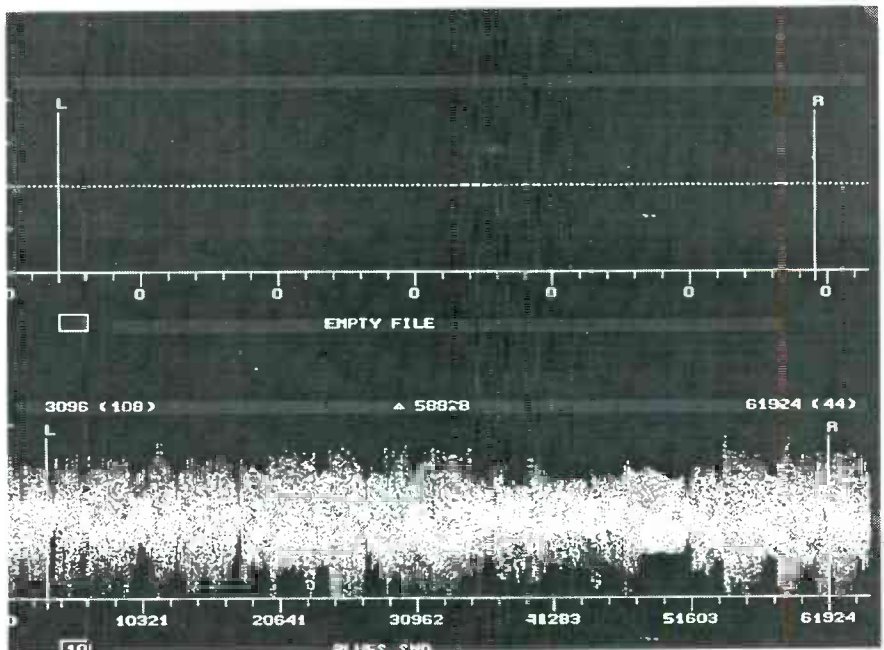


FIG. 2—THE SOUND EDITOR runs in a graphical mode, but all commands must be executed from the keyboard. Basic functions allow you to record and edit sound.

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mand. Creating an echo is similar; you just move the cursor a little further to the right before mixing. Some experimentation is necessary to determine the amount of cursor motion required to achieve a particular effect.

Each sound file normally consists of a maximum of 65,500 bytes. However, the program supplies a direct-to-disk mode, in which larger files can be created and played back. When editing a large file, you can scroll through it in 32K chunks.

A set of filters (lowpass, bandpass, highpass) is available for the sound editor. In addition, drivers for Show Partner and GRASP are included; those programs allow you to create interactive, animated computer-based tutorials and training. The Audio F/X drivers allow you to synchronize sound with the on-screen presentation. Other companies have written drivers for other "multimedia" programs, including Autodesk's wonderful Animator; contact Forte for more information.

## Options and upgrades

A programmer's kit is available; it allows you to get directly at the hardware. In addition, the company sells an amplifier/filter box that allows you to drive the Audio F/X board with an inexpensive microphone.

## Impressions

The first time I installed the board and played a demo Sonata piece, I was entranced. Sure, other computers (Macs, Ataris) have sound capabilities—but I'm mostly a PC chauvinist. So hearing full-bodied sound emanate from a board controlled by my PC was thrilling. In short, I haven't had as much fun playing with a PC product in a long time.

## UltraVision 2.0

Most VGA cards (and EGA cards as well) provide numerous hardware-enhanced modes, but DOS supports only the least-common denominator. As a consequence, that extra capability often goes unused. A program called UltraVision provides a way of tapping those capabilities. In particular, it gives you full control over screen colors, the ability to change the display font, and the ability to use text-mode programs with more rows and columns than usual. The program also provides its own enhanced video BIOS, which speeds up video output

two to five times.

UltraVision's enhancements depend on the specific capabilities of your video adapter; I tested the program with a Video 7 VRAM board. With UltraVision installed, I could run text modes with just about any combination of 80, 94, 108, 120, or 132 columns, and 25, 36, 50, or 63 rows. (A maximum of 60 rows are available at 132 columns.)

## ITEMS DISCUSSED

● Audio F/X (\$350), Forte, 72 Karenlee Drive, Rochester, NY 14618. (716) 427-8595.

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● UltraVision 2.0 (\$119.95), Personics, 63 Great Road, Maynard, MA 01754. (508) 897-1575.

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DOS itself won't recognize the enhanced modes, but many applications will. Qedit, for example, picks up screen dimensions automatically. WordStar can be patched easily. The company also provides drivers and usage hints for many other programs, including 1-2-3, AutoCAD, Crosstalk, dBASE, Magellan, Word, WordPerfect, and many others. I found that a 36 x 80 mode in Word running on a 19-inch NEC MultiSync XL was quite legible. A standard VGA system can run with a maximum of 94 x 63.

The software driver occupies about 20K of memory, and in addition to the functional enhancements it provides, it also operates faster than the built-in BIOS, because it runs from RAM, rather than relatively slow ROM. In addition, the driver runs just fine from "high" memory on either a 386 or EMS 4.0 system (both of which I tested).

UltraVision provides similar enhancements for EGA systems, including a hardware accelerator that provides VGA resolution for some EGA boards with multi-synchronous monitors.

A separate program allows you to change screen colors; laptop and monochrome VGA users could use that capability to remap illegible screen-color combinations. Several other utilities are provided, including an enhanced version of ANSI.SYS.

If you're tired of the feeling that there is capability in your video system that is being wasted, UltraVision 2.0 can help.

R-E



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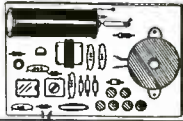
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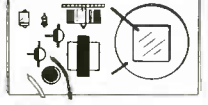
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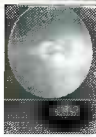
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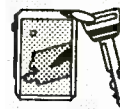
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Scrambling News, 1552 Hertel Ave., #123,  
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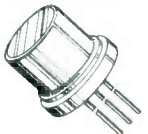
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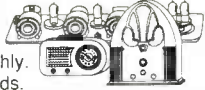
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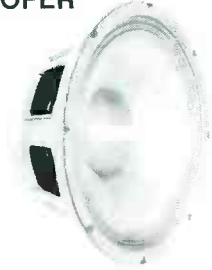
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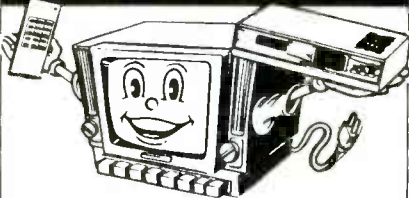
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## LASER JET MEMORY

continued from page 76

of printer. An "X" indicates a closed switch or that a jumper is installed. An "O" indicates the opposite. J1 is viewed with pin 1 to the left.

### Installation and checkout

Plug the 48-conductor cable onto J2 so that the cable runs out and over the front edge of the board. After turning the power off and removing the power cord, remove the memory expansion panels of your printer (see the manual supplied with the printer). Slip the memory board into the card guides inside the printer and plug the free end of the cable into the 48-pin connector.

Power up the printer and run a memory test as described in the printer's manual. Check to see that the amount of memory reported is correct. If problems occur refer to the guide in that manual, and check your work. R-E

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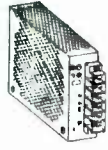












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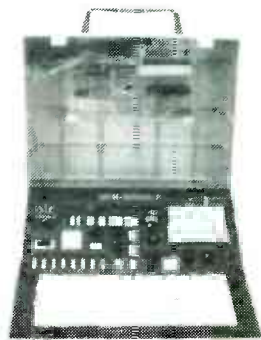
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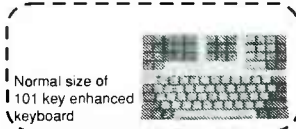
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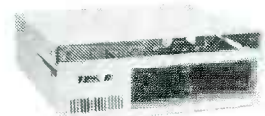
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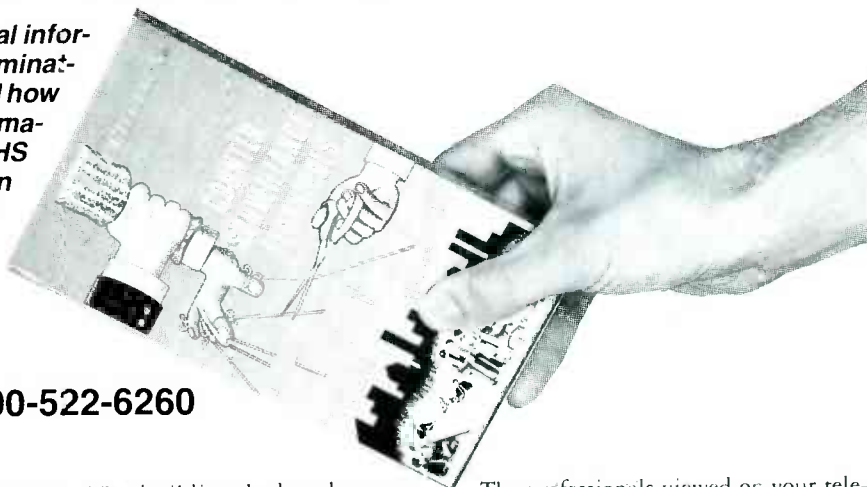
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*Wake up!* You may be the victim of stolen words—precious ideas that would have made you very wealthy! Yes, professionals, even rank amateurs, may be listening to your most private conversations.

*Wake up!* If you are not the victim, then you are surrounded by countless victims who need your help if you know how to discover telephone taps, locate bugs, or “sweep” a room clean.

There is a thriving professional service steeped in high-tech techniques that you can become a part of! But first, you must know and understand Countersurveillance Technology. Your very first insight into this highly rewarding field is made possible by a video VHS presentation that you cannot view on broadcast television, satellite, or cable. It presents an informative program prepared by professionals in the field who know their industry, its techniques, kinks and loopholes. Men who can tell you more in 45 minutes in a straightforward, exclusive talk than was ever attempted before.

## Foiling Information Thieves

Discover the targets professional snoopers seek out! The prey are stock brokers, arbitrage firms, manufacturers, high-tech companies, any competitive industry, or even small businesses in the same community. The valuable information they filch may be marketing strategies, customer lists, product formulas, manufacturing techniques, even advertising plans. Information thieves eavesdrop on court decisions, bidding information, financial data. The list is unlimited in the mind of man—especially if he is a thief!

You know that the Russians secretly installed countless microphones in the concrete work of the American Embassy building in Moscow. They converted what was to be an embassy and private residence into the most sophisticated recording studio the world had ever

known. The building had to be torn down in order to remove all the bugs.

## Stolen Information

The open taps from where the information pours out may be from FAX's, computer communications, telephone calls, and everyday business meetings and lunchtime encounters. Businessmen need counselling on how to eliminate this information drain. Basic telephone use coupled with the user's understanding that someone may be listening or recording vital data and information greatly reduces the opportunity for others to purloin meaningful information.

The professional discussions seen on the TV screen in your home reveals how to detect and disable wiretaps, midget radio-frequency transmitters, and other bugs, plus when to use disinformation to confuse the unwanted listener, and the technique of voice scrambling telephone communications. In fact, do you know how to look for a bug, where to look for a bug, and what to do when you find it?

Bugs of a very small size are easy to build and they can be placed quickly in a matter of seconds, in any object or room. Today you may have used a telephone handset that was bugged. It probably contained three bugs. One was a phony bug to fool you into believing you found a bug and secured the telephone. The second bug placates the investigator when he finds the real thing! And the third bug is found only by the professional, who continued to search just in case there were more bugs.

The professional is not without his tools. Special equipment has been designed so that the professional can sweep a room so that he can detect voice-activated (VOX) and remote-activated bugs. Some of this equipment can be operated by novices, others require a trained countersurveillance professional.

The professionals viewed on your television screen reveal information on the latest technological advances like laser-beam snoopers that are installed hundreds of feet away from the room they snoop on. The professionals disclose that computers yield information too easily.

This advertisement was not written by a countersurveillance professional, but by a beginner whose only experience came from viewing the video tape in the privacy of his home. After you review the video carefully and understand its contents, you have taken the first important step in either acquiring professional help with your surveillance problems, or you may very well consider a career as a countersurveillance professional.

## The Dollars You Save

To obtain the information contained in the video VHS cassette, you would attend a professional seminar costing \$350-750 and possibly pay hundreds of dollars more if you had to travel to a distant city to attend. Now, for only \$49.95 (plus \$4.00 P&H) you can view *Countersurveillance Techniques* at home and take refresher views often. To obtain your copy, complete the coupon below.

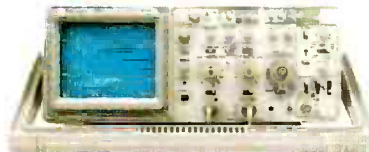
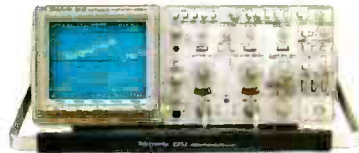
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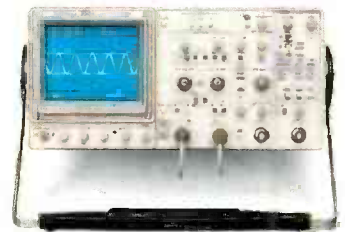
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